# WirelessWorld 

:M. tuner using integrated circnits Felecting an audio amplifier

## TYPE 545B OSCILLOSCOPE

0 (3)
SERIAL 101737




1 MIL mechanically interlocked pair, operating A releases B 2 P33 plug-in version of P.O. 3000, at least 30 m operations 3600 compact version of P.O. 3000,
up to 10A contacts



OUTSIDE• the lot
INSIDE ${ }^{\circ}$
On the outside, Avometers haven't changed much over the years. But inside every genuine Avometer - right across the range from pocketsize Multiminors to $0.3 \%$ Precision Avometers - you'll find the up-to-date guts of the most famous multimeters in the world. Outside - the same familiar functional case and knobs you grew up on. Inside the state-of-the-art circuitry you'd expect from the world leader. Inside and out multimeters to meet every laboratory, test and servicing requirement.


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# Point to Point Broadcasting Radio Relay Ground to Air Navigational Aids Business Radio 

## Design

Site layouts
Aerial System Design

## Aerials

LF ' $T$ ' and ' $L$ ' Aerials, Mast Radiators, HF Dipoles, Quadrants, Rhombics, Log Periodics, Vertical Incidence Arrays, Conicals, Biconicals VHF \& UHF Yagis, Helices, Ground Planes, Colinears, Whips, Marine Aerials,
Television Arrays to 100 kW e.r.p MICROWAVE Passive Reflectors, Dishes $3^{\prime \prime}$ to 60 ft . dia.

## Supporting Structures

Self-supporting Towers, Tubular and Lattice Masts, Telescopic Masts

## Accessories

Coaxial and open wire Feeders, Filters, Aerial Switches, Lead-in panels, Earth Systems. Air-cooled Transmitter Loads. Termination Networks

## Installation

World Wide Service

## C\&S Antennas provide a complete aerial service LF to Microwave r




EEV glass and ceramic hydrogen thyratrons are extensively used to provide more precise and efficient high speed switching. Here are some of the reasons why:
1 Their short anode delay time of between 20 and 120 nanoseconds depending on triggering method
2 Low jitter generally of 1 to 2 nanoseconds but down to less than $\frac{1}{2}$ nanosecond depending on heater supply.
3 The negligible change in anode delay timetypically only 10 nanoseconds over a long period of use.
4 A high peak inverse voltage capability of 20 kV immediately following pulse.
5 The low trigger power required.
6 The wide operating voltage range of $1 \mathrm{kV}-120 \mathrm{kV}$ with four tubes.
7 The ability to control anode delay time and rise time of current, using reservoir.
8 The wide reservoir range for maintenance of gas pressure typically 4.5 V to 5.7 V .
The standard range plus EEV's ability to meet special requirements means that virtually any high speed switching application can be met Here are a few:
Radar modulators with a system output power of $10 \mathrm{~kW}-10 \mathrm{MW}$.
Medical linear accelerators with RF accelerating powers up to 15 MW .
Particle linear accelerators with RF accelerating powers up to 50MW. They may also be used in first-stage particle beam choppers. Particle beam benders where a network of stored energy needs to be discharged into a deflection coil or other device somewhere on the accelerating ring.
Spark chambers
For pulsing light shutters such as Kerr or Pockel cells.
Electronic crowbars and energy diverters

> EEV thyratronsfor better high speed switching

| Type | Peak power output max <br> (MW) | Heating Factor (V.A.p.p.s.) | Peak forward voltage max (kV) | Peak anode current $\max$ <br> (A) | Mean anode current max (A) |
| :---: | :---: | :---: | :---: | :---: | :---: |
| C×1154 | 50.0 | $30 \times 10^{9}$ | 40 | 2500 | 3.0 |
| CX1157 | 3.5 | $7 \times 10^{9}$ | 20 | 350 | 0.35 |
| C×1168 | 100.0 | $70 \times 10^{9}$ | 80 | 2500 | 2.5 |
| C×1171 | 150 | $70 \times 10^{9}$ | 120 | 2500 | 2.5 |
| CX1174 | 120 | $60 \times 10^{9}$ | 40 | 6000 | 6.0 |
| CX1175 | 200 | $140 \times 10^{9}$ | 80 | 5000 | 6.0 |
| CX1180 | 12.5 | $9 \times 10^{9}$ | 25 | 1000 | 1.25 |

Send for full details of the complete range of EEV thyratrons.


## English Electric Valve Co Ltd

Chelmsford Essex England Telephone: 61777 Telex: 99103 Grams: Enelectico Chelmsford


Brief data on some of the ceramic types available.


Please send me full data on your complete range of glass and ceramic hydrogen thyratrons
NAME $\quad$ POSITION

COMPANY

ADDRESS
Peak power output
Peak forward voltage

Peak anode current


## Heathlit Sthe power game

It isn't a game any more - the time has come when the public should be told exactly who is behind the idea that high-quality test instruments can be within the reach of everyone. Heathkit can remain in the shadows no longer - it is time for some plain talking. In Heathkit construction manuals that is exactly what you get instructions clear enough to enable anyone to build their own equipment, thereby cutting costs by up to $50 \%$.

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Tel.Glos. 29451. Telex 43216.

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Send for full details of the complete range of EEV amplifier klystrons.


English Electric Valve Co Ltd
Chelmsford Essex England Telephone: 61777 Telex: 99103 Grams: Enelectico Chelmsford

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I am interested in a klystron with the following parameters:
Frequency Range
Bandwidth

## mhtien electrical radio co. LTD.



| Type | Dimensions |  | Flux Density Gauss | Pole Dia. In. | Total Flux Maxwells | Imp. ohms | Handling Capacity Watts | Bass <br> Res. <br> $\mathrm{c} / \mathrm{s}$ | Frequency Response $\mathrm{c} / \mathrm{s}$ | Weight |  | Price ${ }^{*}$ |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: |
|  | Depth | Dia. |  |  |  |  |  |  |  | lb . | 02. |  |
| HF. 816 | 4.218 | 8* | 16,000 | 1.0 | 63,000 | U | 6 | 63 | 50-15 K | 4 | 8 | £8.15.0 |
| HF. 1012 | $4{ }^{3}{ }^{\prime \prime}$ | 10" | 12.000 | 1.0 | 47.400 | u | 10 | 35 | 30-14 K | 4 | 4 | £6.8.0 |
| HF. 1016 | 420" | 10" | 16.000 | 1.0 | 63.000 | U | 10 | 35 | 30-15 K | 5 | 13 | £10.4.2 |
| HF. 1016 Major | $5 \%^{\prime \prime}$ | 10" | 16.000 | 1.0 | 63.000 | 15 | 10 | 39 | 30-16 K | 6 | 0 | £13.1.11 |
| HF. 1214 | $6 \frac{11}{}$ | 12" | 14.000 | 1.5 | 106.000 | 15 | 15 | 39 | 25-14 K | 9 | 10 | £14.0.7 |
| HF. 1216 | $7{ }^{1 *}$ | 12 " | 16.000 | 1.5 | 121.140 | 15 | 15 | 37 | 20-16 K | 13 | 0 | £21.10.3 |
| T. 816 | A4" | $8{ }^{\prime \prime}$ | 16.000 | 1.0 | 63.000 | 15 | 15 | - | 1500-17 K | 4 | 8 | ¢8.5.9 |
| P2.585 | $\mathrm{H}^{\prime}$ | 21/ ${ }^{\prime \prime}$ | 8.500 | 0.375 | 6.400 | 3 | 0.3 | 330 | 250-9 K | - | 3 | £1.10.6 |

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## Be safe...use EEV magnetrons in your marine radar

|  | Type | Frequency <br> Range ( MHz ) | Peak Output <br> Power (kW) <br> (Typical <br> Operation) | Equivalents (not complete) |
| :---: | :---: | :---: | :---: | :---: |
| Brief data on some of the many types available. The complete range covers S-B and and X-Band types from $3-80 \mathrm{~kW}$. | M5063 | 3025-3075 | 50 | 2J70B |
|  | 2 J 42 | 9345-9475 | 8 | ME1 101, CV3676. MAG3, M526 |
|  | BM1002 | 9415-9465 | 21 | JP9-15B |
|  | M513B | 9345-9405 | 22 | JP9-15, YJ1110 |
|  | M515 | 9380-9440 | 25 | YJ1120 |
|  | M597 | 9380-9440 | 10 |  |
|  | M598B | 9380-9440 | 22 |  |
|  | 599A/B | 9415-9475 | 3 | JP9-2.5D, <br> JP9-2.5E, 7028 |
|  | M5022 | 9415-9475 | 30 | YJ1121 |
|  | M5031 | 9345-9405 | 9 |  |
|  | M5043 | 9380-9440 | 5.8 |  |
|  | M5039 | 9345-9405 | 22.5 |  |
|  |  |  |  |  |
| M5063 | M515 | M5 | A/B | M513B | -aty

English Electric Valve Co Ltd Chelmsford Essex England Telephone: 61777 Telex : 99103 Grams: Enelectico Chelmsford of EEV marine magnetrons.


Please send me full data on your range of marine magnetrons.
I am particularly interested in using a marine magnetron with the following parameters.

| Frequency <br> Range $(\mathrm{MHz})$ | Peak Output <br> Power (kW) | Pulse <br> Length ( $\mu \mathrm{s})$ | Pulse Repetition <br> Rate (p.p.s.) |
| :--- | :--- | :--- | :--- |
| NAME |  |  |  |
| POMPATION |  |  |  |

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*For protection of travelling waveguide amplifiers


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Please send me a copy of "Duplexer Devices". I am interested in a tube with the following parameters:
Frequency range Power

Type of cell

> NAME POSITION

COMPANY
ADDRESS


For all the other desirable fealures
write or telephone:-

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1109


1100


1100/1109


1100 twins


1110

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1109 -often seen around with me, is a most illuminating little pilot light with a variety of colour lenses. At times we are very close and can often be seen working together very harmoniously on a wide range of appliances and equipment.

The 1100 twins are going to be very popular and you can expect to see them on many companies' panels soon.

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| Sangamo |  |
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| CONNECTORS | Birnbach <br> G. C. Electronics |
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| L. M. B. Heeger | Hart Advance |
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| Premier | Line Electric |
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|  |  |
| Simpson |  |
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|  | Mailory |
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| P.A. SYSTEMS | R.C.L. |
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| Eico | JAN \& MIL Units |
| R.C.A. | Stewart Warner |


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| E. F. Johnson | Hunter |
|  | Kraeuter |
|  | Micro Flame |
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| J.B.T. | Triad |
| Mallory | United Transformer Co. |
| Dak | TUBES |
| Dhmite |  |
| Herman Smith | Amperex |
| Switchcraft | Amperite |
| Unimax | Eimac (Eitel McCullough) |
|  | Electrons. Inc. |
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| Audio | General Electronics Mullard |
| Dymo (marking tape) | National Electronics |
| Minnesota Mining (3M) | National Union |
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|  | Raytheon |
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| Lynn Vaco | Illumitronic |
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| Eico | Amphenol |
| Hickok | Belden |
| J.B.T. | Birnbach |
| R.C.A. | Daburn |
| Simpson | Milo/Carolina |
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## IILO ELECTRONICS (UK) LTD.,

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## ... it keeps expanding to reveal new solutions to your measuring problems.

## 1 Multi-function pulse generator <br> 2 A bestselling voltmeter <br> 3 X-Y recorders <br> 4 What ICs can do to counter prices <br> 5 Free book on power supplies



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| FREQUENCY | 0.2 Hz to 1.22 MHz . |  | 1.5 Hz to 150 kHz |  |  |  |
| ACCURACY | $\begin{aligned} & \pm 0.02 \mathrm{~Hz} \text { below } 6 \mathrm{~Hz} \\ & \pm 0.3 \% \text { from } 6 \mathrm{~Hz} \text { to } 100 \mathrm{kHz} \\ & \pm 1 \% \text { from } 100 \mathrm{kHz} \text { to } 300 \mathrm{kHz} \\ & \pm 3 \% \text { above } 300 \mathrm{kHz} \end{aligned}$ |  | $\pm 3 \% \pm 0.15 \mathrm{~Hz}$ |  |  |  |
| DISTORTION | $<0.15 \%$ from 15 Hz to 15 kHz $<0.5 \%$ at 1.5 Hz and 150 kHz |  | $\begin{aligned} & <0.1 \% \text { at I } \mathrm{kHz},<0.3 \% \text { from } 50 \mathrm{~Hz} \text { to } 15 \mathrm{kHz}, \\ & <1.5 \% \text { below } 50 \mathrm{~Hz} \text { and above } 15 \mathrm{kHz} \text {. } \end{aligned}$ |  |  |  |
| SINE WAVE OUTPUT | Source voltage variable from $30 \mu \mathrm{~V}$ to 5 V . Output impedance $600 \Omega$ at all settings. |  | Source voltage variable from $250 \mu \vee$ to 2.5 V . Output impedance $<250 \Omega$ above $250 \mathrm{mV}, 600 \Omega$ below 250 mV . Less than $1 \%$ variation of amplitude throughout frequency range. |  |  |  |
| SQUARE WAYE OUTPUT | None |  | None |  | Variable up to 2.5 V peak. Rise time $1 \%$ of period $+0.2 \mu \mathrm{~S}$. |  |
| OUTPUT METER | Expanded voltage scales and -2 dB to +4 dB . Scale length $3.5^{\prime \prime}$ |  | None | $\begin{aligned} & 0 \text { to } 2.5 \mathrm{~V} \\ & \text { and }-10 \mathrm{~dB} \\ & \text { to }+10 \mathrm{~dB} \end{aligned}$ | None | $\begin{aligned} & 0 \text { to } 2.5 \mathrm{~V} \\ & \text { and }-10 \mathrm{~dB} \\ & \text { to }+10 \mathrm{~dB} \end{aligned}$ |
| POWER SUPPLY | 4 type PP9 batteries, life 400 hours, or, A.C. Mains when: selected by <br> batteries repanel control <br> placed by Power Unit |  | 2 type PP9 batteries, life 400 hours, or, A.C. Mains when batteries are replaced by Levell Power Unit. |  |  |  |
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| TMP | Demmeors |  | Raver <br> Vontage <br> (V) | Range of Notay <br> (v) | $\begin{aligned} & \text { Raver } \\ & \text { lorue } \\ & \text { ( } \mathrm{f} \cdot \mathrm{~cm} \text { ) } \end{aligned}$ | Ratec <br> Soeed <br> ( mm ) | $\begin{gathered} \text { load } \\ \text { Current } \end{gathered}$$(m A)$ |  | $\begin{gathered} \text { Life } \\ \text { (HI) } \\ \hline \end{gathered}$ | Oirection of Revolution |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: |
|  | $(\mathrm{m} / \mathrm{m})$ | $\begin{aligned} & \text { Lengh } \\ & (\mathrm{m} / \mathrm{m}) \end{aligned}$ |  |  |  |  |  |  |  |  |
| EYi73L | 40 | 32.4 | 6 | 4.5-6 | 3 | 2000 | 80 | 35 | 600 | Left |
| DMFP4R-02 | 38 | 34.8 | 6 | 4.5-6 | 9 | 2400 | 140 | 30 | 600 | Ruht |
| (0x 201\% | 47.9 | 48 | 13.2 | $10 \sim 16$ | 30 | 2400 | 210 | 100 | 1000 | Right |
| EFrom | 38 | 30 | 4.5 | 35-5.7 | 8 | 2000 | 160 | 30 | 1500 | Rient |
| ef 200m | 3 | 34.1 | 132 | 155-19-16 | 15 | 2200 | 180 | 30 | 1500 | Right |
| 2F200 | 46 | 50 | 9 | 6 - 9 | 20 | 2200 | 300 | 45 | 3000 | Left Right |
| UP6EOT | 20 | 4.5 | 4.5 | $4 \sim 6$ | 14 | $\begin{aligned} & 3700 \\ & 5000 \end{aligned}$ | 160 | 60 | 30 | Right |
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# Wireless World 

Electronics, Television, Radio, Audio


This month's cover picture shows crossover distortion occurring in a class B output stage. The low-level high-order harmonics contained in the apparently clean sinusoid are quite audible although amounting to less than $0.1 \%$ distortion.
I.P.C. Electrical-Electronic Press Ltd Managing Director: Kenneth Tett Editorial Director: George H. Mansell Advertisement Director: George fowkes Dorset House, Stamford Street, London, SE1

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# How we made thyristors a commercial proposition for consumer products 

Three years ago a Mullard design team was given the problem of developing thyristors for motor speed control in washing machines and drills. Thyristors offered important advantages over conventional power control methods, but at that time, production was confined to relatively expensive industrial devices. The high unit cost was essentially due to specialist production techniques.

Two Requirements The Mullard team set about designing inexpensive thyristors, together with triggering devices, for use on domestic mains supplies. Two current handling capabilities were identified as being necessary to meet the range of
applications-6.5A for washing machines and other heavy current loads, and 2A for drills and lighter loads.

Within six months two consumer type thyristors, BT101 and BT 102, had been developed for 6.5 A applications, and they were soon in mass production. Now these devices, in the TO-64 studmounted metal encapsulation, are well established.

Low-cost Plastic After further design work, a new plastic device, the BT100A, was introduced to meet the lower current requirements. Plastic power device technology is highly specialised, and only intensive effort over many years has resulted in the highly automated manufacturing techniques which ensure extremely good reliability.

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We are constantly receiving letters from private individuals who are finding it impossible to obtain supplies of certain components and whose pleas to manufacturers and distributors are met with stony silence. Even the small company, not in the electronics field, which requires a special component for a one-off job-and which has the advantage of a company letter heading -sometimes receives the same treatment.

One of our correspondents, who was starting a small company, claimed he was asked for two trade references and the name of his bankers, and that was only in order to receive a catalogue!

However, component supply is the result and not the cause of the problem, the whole attitude of the electronics industry towards the private experimenter and the amateur is one of non-co-operation to the point of scorn. Why is this, when many of yesteryear's major innovations in radio and electronics emanated from the results of work carried out on a kitchen table?

In those days the amateur and the professional (often one and the same person) were working on similar problems and there was a mutual respect. The technology has advanced in leaps and bounds since then and industry is staffed with people who more than likely do not have an amateur background and who have no appreciation of the problems and frustrations that can face anyone trying to work on his own for interest, self-education or amusement.

Because of the great amount of publicity given to electronics, and the aura of mystery surrounding it in the eyes of the layman, more people are taking a practical interest. This has led to manufacturers and distributors being bombarded with letters requesting the solution to private electronic problems, many of which are nonsensical or frivolous, and others could have been answered easily if the writer had shown a little initiative or visited a good library. To answer all these queries would cost a company a great deal and what would they get in return? Perhaps an order for two or three components, the value of which may be less than the cost of the handling.
By making their components generally available on the retail market, to be bought by people who may not be qualified to use them, a company feels that it is inviting the sort of costly correspondence mentioned. The reason for the reticence in this respect can be understood.

All this has led to the present ultra-low status of the amateur in the eyes of industry and the reluctance of many concerns to accept small orders.

The industry does, however, have a responsibility to the public, even if it is only to maintain its own image, and attempts must be made to give assistance in genuine cases. Refusals because of a couldn't-care-less attitude can never be justified and small losses should be accepted at times.

Manufacturers could easily set up machinery to ensure that their products can be sold on the retail market through a distributor. Because of the difficulty in assessing the possible quantities required perhaps some sort of sale or return arrangement could be operated with the distributor. At the present time many components are completely unobtainable on the retail market.

In addition, all private individuals seriously interested in electronics should put their own house in order, and as a first step may well think of joining a club. If there is not one in the area-start one. The answer to nearly all the problems likely to trouble the experimenter could be found amongst a group of people with a common aim. Particularly difficult problems could be made club projects. Benefits could be reaped in terms of central facilities, pooled test equipment, tools and literature.

A great deal of useful work can be done by a well-run organization of this nature and the local community can benefit. For instance, club projects could aid local handicapped people, small electronic systems for local firms could be designed and constructed (power supplies, control systems, photo-electric switches etc.). Often these firms can advantageously use electronic equipment, but, because only a one-off is required, it is uneconomic to employ professionals to do the job.

The companies who supply components would, we feel sure, be more than willing to assist such organizations so long as things were done on a business-like basis. A good example of the sort of co-operation that can be achieved is to be seen in the components list for the Logic Display Aid in this issue.

# F.M. Tuner using Integrated Circuits 

# Non-critical mono design with no i.f. and discriminator coils 

by G. J. Newnham,* A.M.I.E.E.

The tuner described has been developed primarily for sound distribution systems but is also suited to home construction. For sound distribution systems reliability is of great importance since operation may be for up to 24 hours per day and service calls are expensive. This tuner has been designed to maximize reliability by eliminating the major causes of previous failure and drift in f.m. tuners. To achieve a high reliability factor in any electronic equipment the components themselves must be stable. The most unstable components in conventional f.m. tuners, apart from the valves, are the i.f. and discriminator coils. Thus, even if crystal control of the local oscillator is used, realignment will be required after a time. Now that integrated circuits with an indefinite life are available, if the i.f. and discriminator coils can be eliminated the reliability should be improved considerably.

With this philosophy in mind the design objectives aimed for were as follows:
(1) The requirement for servicing should be negligible, even after lengthy periods of continuous operation.
(2) The circuit should be non-critical such that if wired correctly it will work "first time".
(3) The assembly and alignment should require very little specialized knowledge.
(4) The circuitry should be the most up to date consistent with commercial economics.
(5) The electrical performance of the tuner should not be sacrificed in order to achieve the other objectives.

In accordance with these aims four integrated circuits are incorporated, but it is noticeable from the circuit diagram, Fig. 1, that a large number of discrete components is still necessary. This is because the i.cs are being used here as "powerful" discrete components and were not specifically designed as f.m. tuner circuits. The next step in the advance of integration, as production becomes cheaper and more efficient, will be an i.c. with a more specific system function, i.e. multiple functions per chip or package. There are signs of this already but such i.cs will still *Marconi-Elliott Microelectronics Lid.

Fig. 1. Circuit diagram of the f.m. tuner

require some discrete components to enable them to have a useful function. After this, or even alongside it, will come total integration of a complete electronic system such as an f.m. tuner, but it will be some time before it is a commercial practicality, even though the technical ability is available now.

The basis of the present design is a low frequency i.f. amplifier centred on 160 kHz , using three Marconi-Elliott E3016 monolithic dual differential amplifiers, followed by a pulse rate discriminator. This principle has been used in previous designs published in Wireless World ${ }^{1,2,3}$ and enables the conventional i.f. and discriminator coils to be dispensed with. The front end employs a Marconi-Elliott 316-04 cascode amplifier as a mixer with built-in oscillator, and has a broad tuned input circuit. Automatic frequency control is applied to the oscillator to ensure and maintain accurate tuning, allowing reliable push-button programme selection. This is all that is really required on v.h.f. and, as with crystal control, the human error involved every time the received station is changed is also eliminated. No r.f. amplifier stage is used.

## Front end

The front end of a v.h.f. tuner is often the cause of poor performance owing to critical layout and adjustment; however, the rather unconventional approach used here has been found very uncritical and stable. The 316-04 i.c. (Fig. 1) is a multi-chip circuit providing useful power gains to frequencies in excess of 200 MHz and as such is being used well within its limits in this application. The lower transistor of the cascode pair in $I C_{1}$ is used as a grounded-collector Clapp oscillator at the fundamental frequency, 160 kHz away from the wanted signal. Owing to the nature of the a.f.c. characteristics the oscillator is always on the low side, but with a.f.c. off, the signal can be tuned in equally well either side. This oscillator configuration is basically stable because the already small transistor junction capacitances are not effectively magnified by voltage gain in the circuit and are therefore easily swamped by the tuned circuit capacitance. Crystal control can be used but crystals are expensive and would have to be specially made for each desired station. Measurements show that without the a.f.c. diode this oscillator moved less than 100 kHz at 100 MHz , when its supply voltage was increased from 10 to 20 volts. This shift is too small to lose a station which is correctly tuned in at 20 volts. A convenient point to monitor the oscillator output, if a valve voltmeter or sufficiently fast oscilloscope is available, is at pin 6 of $I C_{1}$ as it is at relatively low impedance. Approximately 80 mV should be measured at 90 MHz at this pin.

Fundamental as distinct from harmonic mixing was chosen as it gave the best and most consistent conversion gain of 16 dB at 100 MHz . Assuming that correctly set-up switched preset tuning is used, as is advocated with this design, no interference is experienced by adjacent tuners tuned to the same or different programmes.

The upper transistor of the i.c. acts as a mixer, being supplied at pin 1 with a signal from the broad tuned input circuit and local oscillator injection via the internal bias chain. Capacitor $C_{13}$ on pin 3 serves both to ground the collector of the oscillator and to decouple the emitter circuit of the mixer at the i.f. frequency; its value affects the lower 3 dB point of the i.f. bandwidth. A 75 -ohm coaxial feeder is matched to the mixer by $L_{1}$, resonated by $C_{1}$ and the input capacitance at pin 1 . The coupling capacitor $C_{8}$ serves also to decouple the base of the mixer, which would otherwise tend to pick up strong low frequency interference. Capacitor $C_{14}$ serves to cut the residual mixing products other than the difference frequency desired, and is used also to tailor the i.f. upper frequency limit. An input signal as high as 10 CmV does not
affect operation of the mixer, but protection against voltage transients on the aerial is no less necessary than with any other transistor input stage. As can be seen from the layout (Fig. 3), station selection is achieved with four preset trimmer capacitors selected with a printed circuit mounted push-button switch.

## I.F. section

The i.f. section of the tuner amplifies signals centred on 160 kHz and has the advantage that its bandwidth can be defined by $R C$


Fig. 2. Circuit of the type E3016 i.c. used in the i.f. section of the tuner
Fig. 3. Component layout on the printed circuit board supplied by General Avionic Associates Ltd.

networks rather than by $L C$ tuned circuits. A further advantage is that a pulse rate discriminator ${ }^{4,5}$ cạn be used which provides a useful output voltage of excellent linearity without the necessity for alignment. An additional feature of this discriminator is that a direct voltage is available for a.f.c. purposes. A disadvantage of this system is that two tuning points occur per station, although only one is apparent with a.f.c. on. This makes it difficult to search for weak stations among strong ones, but where preset tuning is used this is of no consequence. Another disadvantage is interv modulation whistles, easily produced if the bandwidth is not tailored sharply enough and aggravated if the transfer characteristic does not produce symmetrical limiting. This design ensures a sharp cut-off by using three isolated $R C$ networks, and a symmetrical limiting characteristic is ensured by using a differential amplifier (Fig. 2) for each stage. The use of differential amplifiers also eases the supply decoupling problem, which is important with an overall i.f. gain, including the interface stage $T r_{2}$ of some 110 dB . Impedances in the i.f. chain are low, minimizing the likelihood of instability and spurious pick-up. As shown on the circuit diagram (Fig. 1) each i.c. is decoupled by a capacitor adjacent to the package.

The emitter follower stage $T r_{1}$ is necessary in order to maintain the conversion gain of the mixer, which would otherwise be reduced when working into the low input impedance of the i.f. amplifier. The resistors $R_{5}$ and $R_{6}$ provide a d.c. negative feedback path over the three E3016 stages. Capacitors $C_{20}$ and $C_{21}$ prevent a.c. feedback except at very low frequencies and hence, together with $C_{17}$, contribute to the low frequency cut-off of the i.f. response. The high frequency cut-off is determined by the $R C$ networks $R_{1} / C_{14}, R_{10} / C_{22}$ and $R_{9} / C_{25}$.

A symmetrically limited waveform of approximately 0.8 V peak to peak appears at pin 10 on $I C_{4}$ and to drive the discriminator this is increased to 5 V peak-to-peak by the interface stage $\mathrm{Tr}_{2}$. The d.c. working point of this stage can be adjusted with $R V_{1}$ to suppress noise when a signal is not being received (see "Alignment procedure" section). It was not found convenient to plot the overall i.f. response because the amplification is such as to cause limiting on noise. However, on an oscilloscope frequencies from


Fig. 4. Completed prototype of the f.m. tuner

20 kHz to 350 kHz were observable as a c.w. signal was tuned through (with a.f.c. off).

## Discriminator

The discriminator is a conventional pulse rate type ${ }^{6}$, the operation of which has been fully discussed in earlier issues of Wireless World, but its function basically is to produce a d.c. voltage output (across $C_{31}$ ) proportional to the frequency of the input signal. With suitable component values it can do this very linearly over wide frequency ranges and it has a certain amount of inherent de-emphasis. It is very important that the circuit be loaded correctly with a high impedance, otherwise reduced output and frequency-response distortion will result. For this reason and also to ensure that any length of screened lead may be used on the output without degrading the frequency response, an emitterfollower buffer stage has been included. In conjunction with $C_{32}$, $C_{33}, R_{13}$ and $R_{21}$ this serves also as a low-pass filter to further attenuate residual 160 kHz i.f. output without attenuating frequencies up to 50 kHz by more than 1 dB .

The a.f.c. voltage is applied to the variable capacitance diode $D_{1}$ via $R_{15}$ and $R_{18}$, the capacitor $C_{19}$ ensuring closed-loop stability. The effectiveness of the a.f.c. can be increased or decreased by respectively decreasing or increasing these resistors, but care must be taken not to load the discriminator or make $C_{19}$ too small. One effect of the latter can be to reduce bass response. The effect of the a.f.c. switch in the off position is to supply a fixed bias to the diode of the same value as it would receive from the discriminator when correctly tuned, thus simplifying setting up.

## Construction

The double-sided printed-circuit board as illustrated (Fig. 4) together with all the necessary components are available, by mail order only, from General Avionic Associates Ltd, 9 Wimpole Street, London, W.1. The complete kit including i.cs and instructions costs $£^{9} 196 \mathrm{~d}$ and is perhaps the most straightforward form of construction for the amateur. Before mounting any components make certain that all the holes have been drilled, and insert the eyelets where indicated to join the two sides of the circuit board. If eyelets are not used it can be difficult to solder both sides, particularly with the i.c. leads. If all the components as listed are mounted with careful respect for polarity where capacitors, diodes, transistors and i.cs are concerned, and earth points are soldered both sides of the board, no trouble should be experienced. The board can be mounted such that the push buttons are accessible through a front panel. Use of an earthed metal cabinet is recommended and, if hum troubles are experienced, better supply smoothing may be required.

With some arrangements of the final system (tuner, p.s.u., amp., etc.) 50 Hz hum was experienced and traced to the a.f.c. line. This trouble was entirely eliminated by using in place of $R_{18}$ an r.f.c. $(0.6 \mu \mathrm{H})$ consisting of 20 turns of 26 s.w.g. enam. wire close wound on a $10 \mathrm{M} \Omega \frac{1}{2} \mathrm{~W}$ resistor body. Also $C_{19}$ was increased to $1 \mu \mathrm{~F}$. These modifications had the additional effect of increasing the low frequency response and appeared to seduce interference from electrical apparatus in close proximity to the tuner.

For those who wish to make their own layout there should be few problems as long as an 'earth plane' form of construction is used. This is very important, and ensures that different parts of the circuit that require to be earthed are earthed through the lowest common impedance possible. A convenient method of achieving this form of construction is to use a plain piece of singleplated printed-circuit board. Then, having decided on the component layout, drill holes where the component leads should go, arranging that the components sit on the same side as the copper. hoard with a continuous copper sheet on one side.

## COMPONENTS LIST



## Capacitors



| 1.5k | carbon film |  | dW | 5\% |
| :---: | :---: | :---: | :---: | :---: |
| $100 \Omega$ | .. | .. | .. | . |
| 8.2k | .. | . | . | .. |
| $330 \Omega$ | .. | .. | . | ., |
| $10 \Omega$ | .. | .. | ., | . |
| 1k | .. | . | - | ', |
| 2.2k | .. | .. | .. | , |
| 15k | .. | .. | .. | .' |
| 47k | : | ., | .. | . |
| 180k | ., | . | . | . |
| 1.8k | .. | ., | .. | ' |
| 100k | . | - | $\cdots$ | - |
| 1.2k | ., | ., | $\frac{1}{2} \mathrm{~W}$ | . |
| 180S | " | ., | $\frac{1}{2}$ W | . |
| $4.7 \mathrm{k} \Omega$ | " | .. | JW | ' |
| $150 \Omega$ | .. | . | $\frac{1}{2} W$ | . |
| $5 \mathrm{k} \Omega$ | preset |  |  |  |

4.5-20pF ceramic trimmers 10pF polystyrene 1,500 pF polystyrane
$0.1 \mu \mathrm{~F}$ matallized polyester
47pF polystyrene
22pF polystyrene
390pF polystyrene
$80 \mu \mathrm{~F}$ electrolytic. 16 V
$1 \mu \mathrm{~F}$ electrolytic, 6.4 V
3.300 pF polystyrene
$100 \mu \mathrm{~F}$ electrolytic. 6 V
100 pF polystyrene
1000 pF polystyrene
220pF polystyrene
120 pF polystyrene
$6.4 \mu \mathrm{~F}$ electrolytic. 6.4 V

4 turns 16 s.w.g. tinned copper 0.4 in dia. 0.5 in long tapped 3 turns from earth.
3 turns 16 s.w.g. tinned copper 0.4 in dia. 0.3 in long.

## Integrated circuits

316-04 cascode amplifier. Marconi-Elliott Microelectronics. (Avaflent dual differential amplifier. Marconi-Elliott Microelectronics

Transistors
$T_{r_{1}}$
$\substack{r_{2}, T_{r_{1}}}$
$D_{i}$
Diodes
$D_{1}$
$D_{3}$
$D_{3}$
$D_{4}$
ME4103. BC107
MEO411. BCY70
BFY53, BFY50, 2N3053

BA110. S.T.C
IN916 silicon
12 V zener
6.8 V zener

## Sundries

Double-sided circuit board
Push-button switch assembly. A.8. Metal Products Ltd
A.f.c. switch (not supplied in kit)

Transistor and diode mounting pads and clips
Heat sink for $\boldsymbol{T r}_{\boldsymbol{B}}$
rather than copper strips, is ideal as it saves drilling holes. Where the component leads are not required to be earthed the copper can be cleared away from these holes with a small twist drill and the leads fed through to the other side for wiring up. Wiring can be done with the leads themselves for the most part, but where cross-overs do occur an insulated wire link should be used. Where a component has one lead earthed, this can be done direct to the earth plane, no earth wiring being required. Using this system various layouts have been tried and all worked well.

Remote tuning by means of a d.c. voltage is easily achieved should it be required, but in order to obtain a sufficiently wide tuning range, some circuit modifications must be made. Fig. 5 shows the tuning voltage ( $0-6 \mathrm{~V}$ ) applied to the a.f.c. diode from preset potentiometers remote from the board, $C_{6}$ having been removed and $L_{2}$ increased to 5 turns. Resistors $R_{15}$ and $R_{18}$ have been increased to $1 \mathrm{M} \Omega$, and if a $1 \mathrm{M} \Omega$ resistor is connected across the a.f.c. switch no trouble should be experienced when switching between stations. For maximum tuning range it is recommended that the supply to $R_{3}$ be taken from the top of $D_{4}$, and a $1 \mathrm{k} \Omega$ resistor be connected from pin 6 of the 316-04 to ground. $R_{20}$ and $D_{3}$ are no longer required and only one trimmer capacitor is needed for setting the tuning range instead of $C_{2}$ to $C_{5}$.
A voltage tuned version of the tuner designed for sound


Fig. 5. Modifications to the circuit to allow electronic tuning to be used
distribution systems can be obtained from General Avionic Associates Ltd.

## Alignment procedure

No test equipment is required for alignment of the tuner but some form of monitoring is needed, either headphones direct on the output or an amplifier and loudspeaker. With the aerial disconnected adjust $R V_{1}$ for a maximum of rushing noise in the output. Assuming all is well this should occur over a small section of the track; either side of this should be silence. Set $C_{1}$ about a quarter meshed-it can be peaked later if necessary-and connect an aerial. With a.f.c. switched off it should be possible to tune most of the f.m. band using an insulated trimming tool on any of the trimmers $C_{2}$ to $C_{5}$, selected by the appropriate push button. If all of the available stations are not tunable, $L_{2}$ can be stretched or compressed slightly to alter the coverage. To set a station, it should be approached from the low frequency end of the band, tuned for best output by ear, and then the a.f.c. can be switched on. If when the a.f.c. is switched on the station disappears or becomés distorted, the oscillator must have been set on the wrong side of the station. The best way to check that the oscillator is set correctly is as follows. Having obtained the station and applied a.f.c., take off the aerial and/or switch off the power supply and then reconnect. If the station is still there, all is correct; if not, the trimmer was set outside the a.f.c. locking range. This procedure can be repeated to set any station to any desired push-button. Four are provided, for Radio 2, Radio 3, Radio 4 and a local radio station if available. Once correctly set up the a.f.c. switch should not need to be used again.

## Performance

The tuner has a sensitivity of better than $10 \mu \mathrm{~V}$ at 90 MHz for i.f. limiting. An audio output of 100 mV r.m.s. on an average programme can be expected but programme content varies greatly. Using a good aerial this degree of sensitivity has been found quite adequate in most parts of the country, but a pre-amplifier can be used in difficult areas. In the Chelmsford area of Essex, about 30 miles from the Wrotham transmitter, very good reception is obtained on a short length of wire at ground level, but for minimum pick-up of electrical interference a dipole as high as possible is recommended.


Fig. 6. A suitable power supply for the tuner. $T_{1}$ is a Radiospares Ltd "Hygrade" filament iransformer

Current consumption is between 120 and 150 mA at 12 V which makes the tuner unsuitable for portable use on dry batteries. However, for the majority of applications mains derived supplies are available (see Fig. 6) and if the tuner is used in a car there should be no power consumption problem.

## Performance on stereo

From tests made using a modified Mullard stereophonic decoder it appears that the tuner will not give an adequate performance on stereo broadcasts. The modifications to the decoder were necessary to ensure that the correct impedance and signal levels were obtained. However, channel separation at 440 Hz was only 6 dB . This result may have been due to a limitation of the decoder, which had no provision for subcarrier phase control, but a more likely reason is that the i.f. frequency of the tuner is too low and the bandwidth inadequate for stereo.

In order to eliminate the possibility of intermodulation whistles in the output caused by mixing of 160 kHz with regenerated 38 kHz and its harmonics a special filter is required to remove residual i.f. content. The amount of filtering incorporated in the tuner as it stands was found to be insufficient in this respect.

Acknowledgement. The author thanks the Managing Director of Marconi-Elliott Microelectronics for permission to publish this article.

## REFERENCES.

1. "Wireless World Crystal-Controlled Transistor F.M. Tuner". Wireless World, July 1964.
2. "A Simple Transistor F.M. Tuner" by J. C. Hopkins. Wireless World, September 1965.
3. "Pulse counting F.M. Tuner" by E. D. Frost. Wireless World, December 1965.
4. "Letters to the Editor" on "The Diode Transistor Pump". Wireless World, September 1966.
5. "The Diode Transistor Pump" by D. E. O'N. Waddington. Wireless World, July 1966.
6. ibid. Fig. 5.

## Conferences and Exhibitions

## LONDON

June 10-20
I.M.E., Mark Lane

Marine and Shipping Conference
(Institute of Marine Engineers, 76 Mark Lane, London E.C.3) June 18-27

Interplas: Plastics Exhibition
(Iliffe Exhibitions Ltd., Dorset House, Stamford Street, London S.E.1)

## EASTBOURNE

June 3-5
Congress Theatre
Microelectronics Conference
(I.E.E., Savoy Pl., London W.C.2)

## MANCHESTER

June 30-July 3
U.M.I.S.T.

Computer Science \& Technology
(I.E.E., Savoy Pl., London W.C.2)

## OVERSEAS

June 1-14 Chania, Crete
Growth and Characterization of Electronic Materials
(E.D. Haidemenakis, 2 rue de Furstenberg, Paris 6e)

June 9-10
Chicago
Broadcast and Television Receivers
(I.E.E.E., 345 E.47th St., New York, N.Y. 10017)

June 9-11
Communications Conference
(I.E.E.E., 345 E.47th St., New York, N.Y. 10017)

June 15-22
Paris
Navigation Congress
(Int. Assoc. of Navigation Congresses, Quartier Jordaens (Rez-deChaussee), 155 rue de la Loi, Brussels 4)
June 16-21
W'arsaw
I.F.A.C. Automatic Control Congress
(U.K. Automation Council, c/o I.E.E., Savoy Pl., London W.C.2) June 17-19 Asbury Park, N.J.
Electromagnetic compatibility Symposium
(C. Joly, Honeywell Inc., POB 54, Eatontown, New Jersey 07724)

## H. F. Predictions-June



> - Median standard M UF
> $=-=-=$ Optimum traffic irequency
> $-\cdot-=$ Lowest usable HF

The graphs, which are prepared by Cable \& Wireless Lid, show median standard MUF, optimum traffic frequency and lowest usable frequency (LUF) for reception in this country.

Decreasing solar activity over the past months has lowered MUFs to a greater degree than LUFs; this reduction of usable spectrum will continue for several years with consequent increase in mutual interference problems. Summer conditions, where daytime MUFs are depressed as for Hongkong and Montreal, further aggravate this situation.

Ionospheric and magnetic disturbances have become more frequent of late and can be expected to continue with an occasional complete fade-out.

## News of the Month

## New training group formed

A working group on scientific and technical nanpower has been set up by the Electronic Economic Development Committee (the "litle Neddy" for electronics). One of its main asks will be to determine the future trained nanpower needs of the industry and, in doing this it will take into account the indings of earlier studies in this field.
The group will suggest to E.D.C. the nethods which they should employ to influnce the bodies responsible for training and leploying manpower.
E.D.C. say that the U.K. is spending about , $1,000 \mathrm{~m}$ a year on research (approx. 2.8 per ent of the gross national product); only smerica and Russia spend more. E.D.C. -hink that the return from this very large nvestment is very small in terms of benefit to -he community and to the electronics indus-$-r y$, and, when judged by the overall perforlance of the economy, they feel that the R \& ) effort has not been adequately reflected in he country's economic growth and producivity.
With this background in mind the group ill re-appraise earlier studies of university nd industrial deployment of scientists and echnologists, with particular reference to the electronics industry.

## رow-cost automation centre

nexpensive methods of automation will be emonstrated in the West country in a new entre at the Plymouth College of Technoloy. The centre was opened on April 2nd and pas the result of co-operation between the ollege and the Ministry of Technology. It rill provide specialized training and conultancy services for West Devon and Cornsall.

## On weather forecasting and racking turtles

in equipment being tried for the first time in the satellite Nimbus- 3 will interrogate all tanner of strategically placed sensors on arth and transmit the total acquired data to central earth station for processing. The
system is called the Interrogation Recording and Location System (I.R.L.S.) and it works in the following manner.

Sensors, and appropriate electronics, are placed at various points on earth along the satellites orbit. These may measure temperature, pressure, water currents, salinity or anything else that can be converted into an electrical quantity. The sensors do not have to be fixed and may be installed on free floating buoys, in balloons, in aircraft, in boats, or on land. It is a feature of the I.R.L.S. to track the sensors and keep a record of their position.

At the start of each polar orbit a ground station (at Alaska or Maryland) commands the satellite to interrogate various sensors at particular times. The times are calculated to ensure that the satellite is within range of the required sensor and are based on predictions based on earlier movements of the sensors.

At the appropriate moment the satellite transmits the address code of the required sensor. The sensor acknowledges by transmit-
ung its address code and the satellite commands the sensor to transmit data on existing conditions which are then stored in the satellites' memory. Also recorded in the memory is the exact time of the interrogation and the satellite-to-sensor range for tracking purposes.

On the next pass over the main command control centre the satellite is instructed to transmit the contents of its memory. After suitable processing the data are available for distribution to users.

Apart from weather forecasting the applications of the I.R.L.S. are numerous; for instance the migratory habits of birds, sea life and animals could be studied. Sensors attached to the backs of giant sea turtles, which regularly migrate across the Atlantic from the Caribbean to Africa, would enable their exact course to be plotted.

The I.R.L.S. which has been developed by Radiation Incorporated of America, fitted to Nimbus-3, will interrogate up to 20 sensor stations in one polar orbit. Under a 3 M dollar development contract awarded to Radiation by the N.A.S.A. Goddard Space Flight Center an advanced I.R.L.S. is to be built for Nimbus-D (due for launching in 1970) which will interrogate as many as 370 sensors in a single orbit.

## Television awards

The first recipient of the Gold Medal of the Royal Television Society is Douglas Birkinshaw "for his outstanding contributions to television during his service with the B.B.C. television from 1932-68". Mr. Birkinshaw, who received the medal at the Society's annual ball on May 9th, was engineer-in-charge at Alexandra Palace for the opening of the B.B.C. television service in 1936 and at the

In the background the B.B.C. advanced field store standards converter, and in the foreground members of the two teams from the B.B.C's Research and Design Departments who were responsible for developing the converter. They are (left-to-right, back row) Eric Rout, David Kitson and Robert Harvey; (front row) George Hunt, Stanley Edwardson, Robin Davies and Peter Rainger

time of his retirement a year ago was general assistant to the director of engineering.

The Society's Geoffrey Parr Award was presented by Mrs. Parr to Eric Rout, head of electronics group, B.B.C., and his team' 'for their outstanding work in the development of the advanced field-store television standards converter". The team has also received the Queen's Award to Industry for this project. The system enables 525 -line, 60 -field N.T.S.C. colour signals to be converted to European 625 -line 50 -field PAL or SECAM standards. The equipment is now in regular use by the B.B.C. The inventor of the system, Robin Davies, received the Pye travelling scholarship, worth 1000 guineas, pluş a trophy "for the most significant technical contribution during the year to the development of colour television". Mr. Davies, who is 34 , joined the B.B.C. Research Department in 1958, and transferred to the Department's Television Group in 1963. He described the converter in our January 1969 issue.

The Baird Travelling Scholarship, worth K350 and financed by Radio Rentals, was received by Chrisiopher Jeggo at present studying for a degree of philosophy at the Clarendon Laboratory, Oxford University Physics Department where he is engaged in research in non-linear optics.

## The Emley Moor Saga

March 19th, 1969: Tubular steel mast ( 1250 ft ) collapses; much speculation as 10 the economic consequences, some sources predict that Yorkshire Television will also collapse because of lost advertising revenue.

March 23rd, 1969: zip-up reduces embarrasment; Yorkshire TV once again on the air serving a reduced number of viewers thanks

The business end of the new 675-ft mast. The aerial, consisting of full-wave dipole panels, was built and erected by E.M.I. in only 20 days.

to a hurriedly installed 200 ft zip-up aerial. Coverage quickly further increased due to the rapid commissioning of a relay station in Sheffield.

March 29th, 1969: first sections of a 675 f mast supplied by Sweden arrive at Manchester Airport. March 30th, 1969; Remainder of new aerial shipped into Hull.

April 16th 1969: Y.TV. back on the air to all its viewers, "give or take a few hundred".

The precise cause of the failure of the original mast has still not been officially announced as an independent inquiry committee is still investigating.

The old mast, which was fully insured, cost about $£ 300,000$. The new mast, when it is fully equipped with u.h.f. aerials will cost something like $£ 100,000$. Studies are being carried out to determine the best ways of ensuring full u.h.f. coverage of the area.

Our comment; A darn good performance by all concerned!

## Electronic page composing system

A great deal of the text in Wireless World is set on a photo-typesetter at our printers, Southwark Offset. Basically the text is translated to a digital form on a punched paper tape. This tape is fed into a computing system; which holds such details as column width, type size and other relevant information; and which produces another punch tape containing in addition to the text, control information for a photo-typesetter. The photo-typesetter responds to this tape and produces a film containing the text set to column width.

This film, together with film containing the photographs and drawings, is assembled on acetate sheets from which the printing plates for the offset press are produced using a photo-chemical process.

A system has just been devised by R.C.A. which enables the drawings as well as the text to be handled in digital form. This means that text and drawings (not photographs) can be assembled by a computing system and a film of a complete page can be produced in one go.

The text and drawings are digitized and reproduced on a high-resolution c.r.t. (1,800 lines per inch) and projected on to the film. The equipment, which is known as the Video Text $70 / 840$, will also produce a microfilm of a complete page for storage purposes. Text is set at 6,000 characters per second.

A software package that can be used with the system enables computer tapes, originally intended to be reproduced by a standard line-printer, to be produced with various sized types ( 4 to 96 point) with bold headings, sub-headings, capitals or small letters and with footnotes.

## Integrated circuit lecture tour

This year's Mullard lecture tour, which will visit 76 centres in the U.K., deals with the use of integrated circuits in domestic ap-pliances-radio, 'TV, cameras, cars, etc., and
prophesies that each car built by 1975 will contain about 100 integrated circuits.

The Mullard lectures, intended for service technicians, have been going on now for nearly 15 years and it is expected that attendance this year will approach the quarter-of-a-million mark. The present session started in Southampton on May 5th.

## As components shrink companies expand

Following their recent acquisition of the Controls and Communications group of companies, Racal Electronics Ltd, have been doing some internal re-organization. Racal Communications have been brought together with BCC L.td in a new company, RacalBCC Ltd, that will be responsible for marketing for the three group companies concerned with radio communications (Racal-BCC Ltd Racal-Mobilcal and BCC). The new company will operate from premises at Bracknell.

Airmec Instruments Lid has been amalgamated with Racal Instruments Lid to operate as the Airmec division of that company.

In order to control central services used by members of the group, and to introduce new services as they are required, a new company, Racal Group Services Lid, has been formed.

A sales office in Singapore, previously handling work for Racal Communications, has now been made into a company, Racal Electronics (Asia) Private Lid. This is an addition to other Racal companies now existing in Australia, Canada, Germany, S. Africa and U.S.A.

## Space centre at Bristol

The Guided Weapons Division of the British Aircraft Corporation is building a centre at Bristol which will be used for the construction and testing of satellites and space systems. The first job to be undertaken at the new establishment is the building and testing of two Intelsat-4 communication satellites.

## I.R.D. and Imperial College collaborate

With the aid of a grant from the Science Research Council of $£ 62,338$ the International Research and Development Company and the plasma physics group of the Physics Department, Imperial College, London, are embarking on a study of non-equilibrium phenomena in a steadily flowing plasma.

One of the objects of the programme is to substantially increase the effective conductivity of a flowing plasma so that a strong interaction between the moving gaseous conductor and a magnetic field can occur.

Some of this work will be done using I.R.D's continuously flowing magnetohydrodynamic plasma apparatus in which very pure helium is circulated at velocities ap-
proaching Mach 1 at temperatures up to $2,000^{\circ} \mathrm{K}$. The gas is "seeded" with a small amount of caesium vapour which partially ionizes to form an electrically conducting plasma.

## Solved! or instant jargon

It can now be revealed how some manufacturers and most public relations consultants (particularly American) manage to baffle us all with page after page of high-sounding-incomprehensible-text. They use the new Honeywell "Buzzphrase generator" which will produce a suitable sentence if fed a four digit word. For instance:- 7026 gives:"Based on integral subsystem considerations a primary interrelationship between system and /or subsystem technologies maximizes the probability of project success and minimizes the cost and time required for the evolution of specifications over a given time period." Which might just as well be applied to a rabbit hutch or a computer.

## Appleton memorial lecture

The Royal Society's British National Committee for Radio Science has proposed that at the triennial General Assemblies of the International Union of Radio Science an Appleton Memorial Lecture be delivered by a leading scientist working in the field of ionospheric physics. The lecture is to commemorate the work of the late Sir Edward Appleton, one of this country's foremost radio physicists and a pioneer in the field of ionospheric research, and particularly his long association with the International Union of which he was president from 1934 to 1952. The Royal Society is providing the honorarium to be awarded to the lecturer.

The first lecturer will be Professor W. I. Axford, of the University of California, distinguished for his contributions to upper


The picture shows a Marconi portable television recording unit (shown at ITEX 69) recording an industrial training film.
atmospheric physics including his wind-sheer theory of the sporadic-E layer of the ionosphere. He will deliver his lecture at the General Assembly of the Union in Ottawa in August 1969.

## British companies at WESCON

Under the auspices of the Electronic Engineering Association, and within the Board of 'Trade joint venture scheme, fourteen British companies will be participating in the Western Electronics Show (WESCON) to be held at San Francisco in August. The firms are, A.E.I., AVO., B.P.L., Ekco, Ferranti, Hawker Siddeley Dynamics, Hellerman, Jermyn Industries, L.C.R. Components, M-O Valve, Racal, Rank, Redifon, and Stow Electronics.

An order for close on $£_{1} 1 \mathrm{M}$ has been received by Plessey from the Commonwealth Bureau of Meteorology for 12 type WF44 meteorological radars. The photograph shows the control panel of one of the WF44 equipments.


## Announcements

"Microelectronics for the Circuit Designer" is the title of a six-day residential course to be held at the University of Surrey from September 24th to October 1st. Details are obtainable from the Course Organizer, Department of Electrical and Control Engineering, University of Surrey, Guildford, Surrey. Fee $£ 54$.
A.S.E.E. The Association of Supervising Electrical Engineers has adopted the revised title "The Association of Supervisory and Executive Engineers" and membership will no longer be restricted to electrical engineers.
The Ministry of Technology, on behalf of the Ministry of Defence, has placed an order worth almost $£ 400,000$ with the Solartron Electronic Group Lid, for an Air Electronics Trainer for the Royal Air Force.
G.E.C. Electronic Tube Co. Ltd has been formed to unite the activities of M-O Valve Co. Lid and English Electric Valve Co. Lid. Both $\mathrm{M}-\mathrm{OV}$ and E.E.V. will continue to manufacture and market under their existing trade names.
Siliconix Incorporated of California, designers and suppliers of field-effect transistors, have announced a new wholly owned British subsidiary based in South Wales. The British company, Siliconix Lid, will manufacture a similar line of products and will be responsible for marketing throughout Europe and the Commonwealth.
General Instrument Corporation of Delaware, U.S.A., has acquired Vitality Bulbs Ltd, of Bury St. Edmunds, Suffolk, manufacturers of miniature and sub-miniature electric bulbs.
The Plessey Company have acquired $49 \%$ of the equity in Electroprints Ltd, a wholly owned subsidiary of Painton \& Co. Lid. The joint company will continue as Electroprints Ltd, manufacturing flexible printed wiring for the electrical and electronics industry.
Ultra Electronics (Components) Lid have acquired Ward Brooke \& Co. Lid as part of their expansion programme. The sales office for connector, terminal and wire-wrapping products will operate from UECL/Ward Brooke Ltd, Fassetts Road, Loudwater, Bucks.
Technograph Printed Circuits Lid, of Fleet, Hants, have changed the name of the company to Technograph Lid.

# Wireless World Logic Display Aid 

# 2: Details of the digital-to-analogue converters and some general information 

designed by B. S. Crank*

Last month a general outline description of the instrument was given and now the time has come to look at the individual circuits themselves. The first circuits to be studied will be the digital-to-analogue converters which produce the staircase $X$ and $Y$ waveforms mentioned last month.

The digital-to-analogue converters employ a current summing principle. Taking the Y dian as an example, each bistable in the counter controls a constant current generator via a buffer amplifier. The amount of current each constant current generator produces is directly related to the decimal weighting of the bistable that controls it. The counters operate in the natural binary code, which is sometimes known as the $1,2,4,8$ code. The constant current generators produce outputs of about $1,2,4$ and 8 mA .

Referring to Fig. 15, which illustrates the operating principles of the dians, it will be seen that all the constant current generators in a particular dian share a common load resistor. The voltage drop across this resistor will of course be directly proportional to the current flowing through it and as the resistor has a value of $1 \mathrm{k} \Omega$ a current of 1 mA will produce a drop of 1 V .

In Fig. 15 the action of the bistables is simulated by switches. One of the constant current generators is connected directly to the negative line and will always have a current flowing through it; this is arranged to be 2 mA . Therefore, with all the switches open the potential at the output will be 2 V below the supply line voltage i.e. 25 V .

If switches 2 and 4 are closed, as would be the case if
*Assistant Editor, Wireless World
the counter held $0110\left(=6_{10}\right)$, an additional 6 mA would flow through the load resistor, causing a voltage change at the output of 6 V . If the switches are replaced by a counter it


Fig. 15. Demonstrating the principle employed in the dians.
can be seen that the voltage output of the dian will be directly proportional to the contents of the counter and the output will alter 1V for each input pulse to the counter.

The constant current generator circuits were originally described in a Letter to the Editor, written by Peter Williams, which appeared in the September 1966 issue of Wireless World.

The complete circuit of the Y dian is shown in Fig. 16. The component reference numbers in brackets refer to the X dian, the circuit of which is identical.

The four switches of our example have been replaced by the BC107 transistors $\operatorname{Tr}_{13-16}$ which are buffer amplifiers between the bistables in the counter and the

Fig.16. The circuit diagram of the $Y$ dian. The component references in brackets refer the $X$ dian.

constant current generators.
The five constant current generators, each consisting of a 2N1304 and 2N1305 complementary pair, can easily be identified. The variable resistors $R V_{1-3}$ and 4-6 serve to adjust the precise current values.

Some additional circuitry; $\operatorname{Tr}{ }_{11,12,} D_{1,2}$ and $R_{7}$; has been incorporated and is associated with the 4 and 8 mA constant current generators. The purpose of this is to modify the output of the dian to obtain the matrix raster shown in Fig. 13 last month to separate the characters in the Truth table and Karnaugh map modes of operation.

During Venn operation the bottom end of $R_{7}$ is connected directly to the negative line. $\operatorname{Tr}_{11}$ and $\operatorname{Tr}_{12}$ will be switched off and the dian will operate as previously described. For Truth table and Karnaugh operation the earth is removed from $R_{7}$ with the result that both $\operatorname{Tr}_{11}$ and $T r_{12}$ switch on by virtue of the current that will flow from the +4.5 V line. The variable resistor $R V_{5}$ will be connected in parallel with $R V_{4}$ and $R V_{7}$ will be connected in parallel with $R V_{6}$. The effect of this will be to increase the current through 4 and 8 mA constant current generators. In other words, when switched on, the once 4 and 8 mA constant current generators will cause a voltage drop of more than 4 or 8 V across the load resistor $R_{6}$. The dian now follows a $10,5,2,1,1$ aw, as can be seen in Table 2.

Table 2
-Decimal
Sontents of zounter

0
1
2
3
Venn mode
Volts Volts

| Volts | mode Volts |
| :---: | :---: |
| 0 | 0 |
| 1 | 1 |
| 2 | 2 |
| 3 | 3 |
|  | - |
| 4 | 5 |
| 5 | 6 |
| 6 | 7 |
| 7 | - |
|  | 10 |
| 8 | 11 |
| 9 | 13 |
| 10 | - |
| 11 | 15 |
|  | 16 |
| 12 | 18 |

The effect on the output waveform is shown in Fig. 17. The steps in the staircase waveform when the counter olds 4,8 or 12 are higher than the other steps. The dots on the matrix raster will be wider spaced at these points, which is what is required.

Some readers will consider that the circuit of the dian is over elaborate and may suggest that a resistive ladder zetwork and amplifier should have been used. In defence of the circuit employed one must point out that it is accu:ate, stable, provides a high level of output and, most imyortant, does not employ any difficult-to nbla'n precision somponents.

At one time during the development it was suggested hat f.e.ts should be employed as the constant current sources; however, after some thought the idea was not ised because f.e.ts would have had to be specially seleced for particular values of $I_{D S S}$.

The form of construction employed is very clearly Ilustrated in Fig. 18. The base-board material is
0.15 inch pitch Veroboard. It is recommended that the dians are built as shown, as it will be found, later on in this series, that when built to this size the dians will fit in very nicely with the mechanical layout as a whole. An idea of this can be gained from Fig. 19 which shows the single

Fig.17. How the staircase waveforms are modified in the Truth table and Karnaugh map modes of operation.


Fig. 18. Physical layout of one dian. The base material is $0.15 i n$ unclad Veroboard.

(2) Collector 2 N 1305 \& base 2 N 1304
(3) Base 2 N 1305 \& collector 2 N 1304 (4) Emitter on 2 N 1304

Fig. 19. The position of the dians on the main logic assembly.

base board which holds both dians and the whole of the logic circuit for the rest of the instrument. A photograph of a completed dian is shown in Fig. 20.

There is only one point in the construction that requires particular attention. This arises from the fact that the cans of the transistors used are common to the collector lead. In order to prevent needless short-circuits it is recommended that the transistor cans be insulated in


Fig. 20. A compleled dian. Sharp-eyed readers may notice that one of the transistors has been substituted for a different type. This was only because we ran oul of slock of the specified type.


Fig. 21. A dian lest circuit.


Hig. 22. The layoul of the circuil board sockets in the main $\operatorname{logic}$ unit.
some way, say with a plastic or rubber sleeve or even with a turn or two of Sellotape. It will be noticed that the buffer amplifiers, $\operatorname{Tr}_{13-16}$ and associated resistors are not included on the dian boards. These are located elsewhere and their description will be given later.

## Adjusting the dians

The dians are connected as shown in Fig. 21 after turning all variable resistors to their maximum value. The 27V can be supplied from three 9V batteries in series-PP9s are ideal-and the 4.5 V can be supplied by a single battery. The switches $1,2,4$ and 8 are connected to the points in the circuit with the same numbering (the BC107 collectors) The switch that has been labelled "Venn" is connected to the bottom end of resistor $R_{7}$, or $R_{18}$ in the case of the X dian. Go through the sequence of operations listed below.
(1) Open switches $1,2,4$ and 8 .
(2) Close Venn switch.

Adjust $R V_{1(8)}$ to make meter read 25 V .
Close switch 1.
Adjust $R V_{2(9)}$ to make meter read 24 V .
Open switch 1.
Close switch 2.
Adjust $R V_{3(10)}$ to make meter read 23 V .
Open switch 2.
Close switch 4.
Adjust $R V_{4(11)}$ to make meter read $21 V$.
Open switch 4.
Close switch 8.
Adjust $R V_{6(13)}$ to make meter read 17 V .
Open Venn switch.
Adjust $R V_{7(14)}$ to make meter read 15 V .
Open switch 8.
Close switch 4.
Adjust $R V_{5(12)}$ to make meter read 20 V .
This setting up procedure is completed when it has been applied to both of the dians. The effect of combinations of switches being closed can be tried to illustrate the way in which the circuit works. This is best done with the Venn switch closed.

## General construction

The next job is to mount the sockets that will eventually take the various circuit boards. The sockets are screwed to a single sheet of perforated s.r.b.p. sheet (Lektrokit part no. LK-141). The positions of the sockets are given in Fig. 22 which shows the lower side of the board. Care must be taken to mount the sockets the right way round.

The boards containing the dians are attached to the edges of the main mounting board using four small metal brackets. Meccano brackets were used in the prototype. The exact positions of the dians can be seen in Fig. 19.

## Buffer amplifiers

The eight transistors, $T r_{13-16}$ and $T r_{29-32}$, are mounted on a piece of 0.1 -inch pitch clad Veroboard which is called "board one". The Veroboard is cut to size using one of the integrated circuit mounting cards as a template. Care must be taken to ensure that the copper strips line-
up accurately with the contacts of the socket when the board is plugged in.

The eight transistors and the eight associated $4.7 \mathrm{k} \Omega$ resistors are mounted on the board as shown in Fig. 23. This drawing also shows the connections between socket one and the X and Y dians; these should be made at this stage.

It is possible that the settings of the variable resistors in the dians will have been upset during the assembly work. To check this and to check the operation of the buffer amplifiers wire up the circuit shown in Fig. 24 and repeat the dian setting-up procedure given earlier.

We will now proceed with a discussion of the circuit boards and the more general aspects of the integrated circuits used before going on to the logic design of the display aid next month.

## Circuit boards

A word or two about the plug-in boards would not be out of order at this stage. The numbering of the board input connections is shown in Fig. 25. With the printed side of the board towards you and the input side to the right the input pins are numbered from one to 24 from bottom to top. The printed conductors are used for the power supplies. The top line, from pin 24 is always the positive line and is connected to pin 14 of each integrated circuit without exception. The lower line is always the negative supply and is connected to pin seven of every integrated circuit, again without exception. Connection to the power supply lines is made by bending the appropriate integrated circuit pins over and soldering them directly to the printed power lines. This serves to hold the integrated circuits in position and prevents them from falling off the board.

In Fig. 25 and Fig. 26 it will be seen that each integrated circuit station on the board has been referenced with a number between one and six; this referencing holds good for every board. An integrated circuit may have the circuit reference IC4/B3. This is read as integrated circuit number four on board three. In the same way P12/B4 would indicate board input socket pin number 12 of board four. Finally, P12/IC4/B3 means pin 12 of integrated circuit number four on board three. It is important to recognise the difference between an integrated circuit input pin reference number and a board input pin reference number.

Wiring the boards is a task that deserves some thought on the part of the constructor as the reliability of the finished instrument depends on it. In the prototype 22 s.w.g.tinned copper wire was used and found to be excellent for the job. The type of sleeving used depends on the preferences of the individual constructor. In the prototype 0.5 mm bore silicon rubber sleeving obtained from Radiospares was employed and was found to be pleasant to handle. Some readers may consider that the 1 mm outside bore of this sleeving is a little on the large side.

The pins on the integrated circuits are only 2.54 mm ( 0.1 inch) apart and can easily be bent. After one has wrapped a wire (or several) round each pin and applied the solder the clearance between pins is very much reduced. The moral is obvious-neat joints, with the minimum amount of solder consistent with a reliable connection.

The constructor is faced with the prospect of interconnecting on each board, with dozens of wires, six integrated circuits, each with 14 pins, and the 24 input pins of the wiring board. There are no "landmarks" in the form of unusually shaped resistors or capacitors to guide the way. Errors are easily made. Be warned!

The approach adopted with the prototype was to complete the inter-gate wiring first, followed by the circuit inputs and finishing with the outputs. In each case the pins to be interconnected can be identified with a small pencil


Fig. 23. Construction of board 1 containing the buffer amplifiers. The vacant space will be used for other components later on in the construction.


Fig. 24. Buffer amplifier/dian test circuil.


Fig. 25. The component side of one of the circuil boards.


Fig. 26. The circuit side of one of the component boards. This is in fact board 7 which has less wiring than most of the other boards.
mark on the board adjacent to the required pins. The best route for the wire to take, consistent with neatness, is then planned and the relevant connections made. As each connection is dealt with it is good practice to mark the fact with a tick on the circuit diagram. In this way wires should not be omitted.

## Integrated circuits

The use of integrated circuits is more than justified in amateur constructional projects even if one forgets the performance advantages and works only on the cost. Each gate consists of two transistors, four diodes and three resistors. The constructor would not be able to produce a similar circuit at an equivalent price in discrete components. And of course, when using integrated circuits, one has the advantage of a guaranteed performance and small size.

The integrated circuits are from the Ferranti Micro-nor-2 family of diode-transistor logic. As discussed earlier, in the introductory article, the basic gate performs the positive logic NAND function.

The circuit of the basic gate used in Micronor-2 departs slightly from the conventional NAND circuit and is worthy of mention. A conventional d.t.l. NAND gate is shown in Fig. 27. With all the input diodes at a potential around 4V, the normal logical $1, T r_{1}$ is switched on by the current flowing through $R_{1}, D_{5}, D_{6}$ and the base emitter junction of $T r_{1}$. The output therefore, will be at earth potential or at logical 0 . The drive to the transistor is limited by $R_{1}$. Thus to achieve high fan-out, that is the number of gates that can be driven from the output, over the operating temperature range the output transistor must be a high-gain device. This is not only undesirable in terms of process yield but additionally generates excess stored charge in the low fan-out condition, severely limiting operating speed.

When one of the input diodes is earthed the base emitter junction of $T r_{1}$ is effectively short circuited and the transistor switches off. The diodes $D_{5}$ and $D_{6}$ act as voltage level shifters to cancel out the effect of the small voltage developed across the now conducting input diode.

The circuit is modified slightly in Micronor-2 as shown in Fig. 28. Additional drive to the output transistor $T r_{2}$ is

Fig. 27.
A conventional d.t.l. NAND gate.

provided by replacing one of the original level shifting diodes by the transistor $T r_{1}$. When the output is unloaded the current flowing through $R_{3}$ is shared equally through two essentially identical impedance paths. Half the current flows through the saturated collector emitter junction of $T r_{2}$. Under these conditions base drive to $T r_{2}$ is at a minimum resulting in low propagation delays at low fanout.

When the output is fully loaded, the flow of load current into $T r_{2}$ sets up an additional voltage drop across the saturation resistance of $T r_{2}$, providing maximum base drive.

Thus the circuit functions in a feedback manner and correctly proportions the base drive to suit the particular load current. This allows the use of a much lower gain output transistor and aids operating speed.

The basic gate has a fan-out of eight and a propagation delay of the order of 15 ns . Two different power gates are used when a fan-out of more than eight is required; one performs the NAND function and the other the AND function (described as OR in the literature). The power gates have a fan-out of 25 . Both types of gates can be supplied with or without an internal load resistor. Where no load resistor is used the gate output is intended to be connected directly to the output of another gate so that they

Fig. 29. Pin connection details of the i.cs used in the instrument. A dot in a gate denotes that it contains a load resistor.


## Components list for basic instrument

The majority of the components are divided into kits for ease of ordering. The prices quoted have been specially negotiated by Wireless World and represent extremely good value for money. It is important to note that these prices apply at the time of going to press and only for complete kits.

Kit LDA/A. Integrated circuits
Price $£ 33-15-0$ Ferranti Ltd., Gem Mill, Chadderton, Oldham, Lancs.

| board | IC reference number |  |  |  |  |  |  |
| :--- | :--- | :--- | :--- | :--- | :--- | :--- | :---: |
|  | 1 | 2 | 3 | 4 | 5 | 6 |  |
|  | ZN330E | - | - | - | - | - |  |
| 2 | ZN324E | ZN324E | ZN324E | ZN324E | ZN322E | ZN330E |  |
| 3 | ZN320E | ZN324E | ZN322E | ZN320E | ZN332E | ZN322E |  |
| 4 | ZN332E | ZN320E | ZN346E | ZN324E | ZN322E | ZN346E |  |
| 5 | ZN346E | ZN362E | ZN346E | ZN346E | ZN362E | ZN362E |  |
| 6 | ZN330E | ZN362E | ZN346E | ZN330E | ZN362E | ZN346E |  |
| 7 | ZN330E | ZN362E | ZN346E | ZN330E | ZN362E | ZN362E |  |
| 8 | ZN330E | ZN362E | ZN346E | ZN330E | ZN362E | ZN346E |  |

Kit LDA/E. Resistors and Hardware
Price £9-10-0 Home Radio (Components) Ltd., London Rd., Mitcham, Surrey.

Lektrokit
qty.
7. P.C. Board Cardic 6
8. Gard guide (pair)
9. Edge connector

1. Chassis plate

Kit LDA/C. Miscellaneous
Price £4-10-0 G.W. Smiths (Radio) Ltd., 3 Lisle St., London, W.C.2.
qty.
2 Radio press button unit 3 button, 3 pole C/O
Terminal unit SLT4
Terminal unit SLT2
Coaxial plug L1465/FP
Coaxial socket L1465/CS
1 Transformer type MT103AT

## 1 Heat sink

1 Toggle switch (TS1)


All variable resistors are type VR100A except $R V_{15}$ which is type VR25.
Kit LDA/E. Resistors and Hardware
Price $£ 9-10-0$ Home Radio (Components) Ltd.,
London Rd., Mitcham, Surrey.

## Resistors (fixed)

The reference number of all resistors is prefixed
$R$, this has been left off below for the sake of clarity. All values in ohms.

| 1. | 4.7 k | 7. | 1 k | 13. | 4.7 k | 19. | 4.7 k |
| :--- | :--- | ---: | :--- | :--- | :--- | :--- | :--- |
| 2. | 4.7 k | 8. | 4.7 k | 14. | 2.7 k | 20. | 4.7 k |
| 3. | 2.7 k | 9. | 4.7 k | 15. | 1.5 k | 21. | 4.7 k |
| 4. | 1.5 k | 10. | 4.7 k | 16. | 1 k | 22. | 4.7 k |
| 5. | 1 k | 11. | 4.7 k | 17. | 1 k | 23. | 150 |
| 6. | 1 k | 12. | 4.7 k | 18. | 1 k | 24. | 180 |

All resistors $1 / 4 \mathrm{~W}$ with the exception of $R_{24}$ which is 2 W

Kit LDA/B. Semiconductors
Price £11-10-0 LST Electronic Components Ltd., 7 Coptfold Rd., Brentwood, Essex.

The reference numbers for all the transistors are prefixed $T r$, this has been left off below for the sake of clarity

| 1. | 2N1305 | 13. | BC107 | 25. | 2N1305 |
| :---: | :---: | :---: | :---: | :---: | :---: |
| 2. | 2N1304 | 14. | BC107 | 26. | 2N1304 |
| 3. | 2N1305 | 15. | BC107 | 27. | BC107 |
| 4. | 2N1304 | 16. | BC107 | 28. | BC107 |
| 5. | 2N1305 | 17. | 2N1305 | 29. | BC107 |
| 6. | 2N1304 | 18. | 2N1304 | 30. | BC107 |
| 7. | 2N1305 | 19. | 2N1305 | 31. | BC107 |
| 8. | 2N1 304 | 20. | 2N1304 | 32. | BC107 |
| 9. | 2N1305 | 21. | 2N1305 | 33. | BC108 |
| 10. | 2N1304 | 22. | 2N1304 | 34. | BF179 |
| 11. | BC107 | 23. | 2N1305 | 35. | 2N3404 |
| 12. | BC107 | 24. | 2N1304 | 36. | 2N3055 |

## Diodes

| $D z_{1-20}$ | $3.3 \mathrm{~V}, 250 \mathrm{~mW}$, zener diodes |
| :--- | :--- |
| $D_{1-2}$ | 1 N 914, or anly small silicon diode |
| $D_{3-4}$ | BXY10, Mullard |
| $D_{5}$ | $\mathrm{SJ103}$ |

## Kit LDA/D. Cabinet

Price £8-19-0 Bedco Ltd., Datumn Division, Colne Way Trading Estate, Watford, Herts.
Cabinet DA 3U12/6 (mushroom top) Chassis SC 3126
operate in parallel. This type of connection is called "Wired OR" and will be discussed in more detail in the section on NAND logic which follows.

It is not proposed to discuss the J -K flip-flop in any detail at all here. In the display aid the $\mathrm{J}-\mathrm{K}$ facility is not employed and the flip-flops are only used as standard toggle bistables. In the article the term bistable will be used in preference to flip-flop.

The different types of integrated circuits used, together with the pin connection details are shown in Fig. 29.

## NAND logic

If two variables $A$ and $B$ are fed to the input of a NAND gate the output, as we saw in the section on positive and negative logic, is false when the condition $A B$ exists. This of course is the negative of the AND function.

If the two input variables are $\bar{A}$ and $\bar{B}$ then the output is given by $\overline{\overline{\mathrm{A}}} \overline{\mathrm{B}}$ :

In other words the OR function is performed. Consider the circuit of Fig. 30. The output of gate (a) will be $\overline{\bar{A} B}$ and the output of gate (b) will be $A \bar{B}$. These will be combined in gate (c) to produce:

$$
\begin{aligned}
\mathbf{X} & =\overline{\overline{\overline{\mathrm{AB}}} \cdot \overline{\mathrm{~A} \overline{\mathrm{~B}}}} \\
& =\overline{\overline{\bar{A} \mathrm{~B}}}+\overline{\overline{\mathrm{A} \overline{\mathrm{~B}}}} \quad \text { (De Morgan's Theorem) } \\
& =\overline{\mathrm{A}} \mathbf{B}+\mathbf{A} \overline{\mathrm{B}}
\end{aligned}
$$

In general, when using NAND logic, the first stage of gating performs the AND function and the second stage gives OR. Subsequent odd stages give AND and even stages give OR.

From the earlier example gates (a) and (b), Fig. 31, will produce the functions $\mathrm{AB}+\mathrm{CD}$ and $\mathrm{EF}+\mathrm{GH}$. The expressions will be combined in gate (c) to give:

$$
\begin{aligned}
\mathbf{X} & =\overline{\overline{\mathbf{A}} \overline{\mathbf{B}}} \\
& =\overline{\overline{\mathbf{A}}}+\overline{\overline{\mathbf{B}}} \text { (De Morgan's Theorem) } \\
& =\mathrm{A}+\mathrm{B} \text { (double negatives) }
\end{aligned}
$$

$$
(A B+C D)(E F+G H)
$$

Gate (d) will merely invert this to give:


Fig. 32
Fig. 30. A typical NAND circuil.
Fig. 31. Another NAND circuit described in the lext.
Fig. 32. The wired OR connection.
In the section on integrated circuits it was stated that some of the gates were supplied without an integral load resistor so that the "wired OR" function could be performed. In the logic diagrams the presence of a load resistor in a particular gate is denoted by a dot in the circle representing the gate.

The "wired OR" connection is performed by connecting gate outputs in parallel as shown in Fig. 32. Gates without load resistors are paralleled with a gate with a load resistor. A moment's thought will show that the output of such a combination cannot be "up" until the outputs of all the gates in parallel are "up". The function performed by the circuit of Fig. 32 can be written as:

## $\overline{\bar{A} \bar{B}+A B}$

Now:

$$
\begin{aligned}
\overline{\mathrm{A}} \overline{\overline{\mathrm{~B}}+\mathrm{AB}} & =\overline{\overline{\mathrm{A}} \overline{\mathrm{~B}} \cdot \overline{\mathrm{AB}} \quad \text { (De Morgan's Theorem) }} \\
& =(\overline{\bar{A}}+\overline{\bar{B}})(\overline{\mathrm{A}}+\overline{\mathrm{B}}) \text { (De Morgan's Theorem) } \\
& =(\mathrm{A}+\mathrm{B})(\overline{\mathrm{A}}+\overline{\mathrm{B}}) \text { (double negatives) } \\
& =\mathrm{A} \overline{\mathrm{~B}}+\overline{\mathrm{A}} \mathrm{~B}
\end{aligned}
$$

This is the same result that was achieved with the circuit of Fig. 30; however, one gate fewer was used. "Wired OR", therefore, can result in fewer gates being needed to perform a particular function.

An expression in AND/OR form can easily be converted into NAND form by repeated use of De Morgan's theorem:

$$
\begin{aligned}
& \text { (ABC+DEF) (GHI+JKL) }+(\mathrm{MNO}+\mathrm{PQR})
\end{aligned}
$$

$$
\begin{aligned}
& =\overline{\overline{\overline{\overline{A B C}} \overline{\overline{\mathrm{DEF}}}} \overline{\overline{\overline{\mathrm{GHI}} \overline{\mathrm{JKL}}}} \overline{\overline{\overline{\mathrm{MNO}} \overline{\mathrm{PQR}}}} . \overline{\bar{x}}} \\
& \text { which reduces to: }
\end{aligned}
$$



Next month: The logic design and construction of the counter and code converter.

# Wireless World Reprints 

In response to the demand for issues of Wireless World which are now out of print we have prepared reprints of several of the more popular constructional articles. This service will be particularly useful to new readers or those who, not having a regular order for Wireless World, have found that, by the time they hear that a certain issue contains something of interest to them, it is out of print. Reprints of articles of educational interest, enable instructors to have enough copies to distribute round the class, and of course when a series is involved it is much handier to have all the information together in one booklet. Readers who have already built the equipment will find the booklets useful as manuals-especially if it is intended to sell the equipment at a later date. The reprints are listed below and may be obtained from the Trade Counter, Dorset House, Stamford Street, London S.E.1. Prices include postage and packing

No. 1. High-fidelity Amplifiers by A. R. Bailey (Nov. and Dec. 1966, and May, June and Nov. 1968). This reprint is still in preparation and an announcement will be made as soon as it is available. It will contain articles on 20 - and $30-\mathrm{W}$ amplifiers; a pre-amplifier; and an article on output transistor protection plus modifications relevant correspondence.

No. 2. Stereo Decoder and Simulator by D. E. O'N. Waddington, (Jan. and Oct. 1967). Describes the construction of a stereo decoder for positive or negative power supplies and contains details of an instrument for producing a stereo multiplex signal. Price 3 s .

No. 3. Portable $\mathbf{1 - M H z}$ Frequency Standard by L. Nelson-Jones (Feb. 1968). Presents a design for a frequency standard which is phase locked to the 200 kHz Light l'rogramme transmissions. Price 3s.

No. 4. Wide-range General Purpose Signal Generator by L. Nelson-Jones (April 1968). Range 150 kHz to 120 MHz in five bands; output attenuator range 100 dB in 20 dB steps $( \pm 0.5 \mathrm{~dB})$; modulation depth 0 to $50 \%$ (can be set to within $\pm 5 \%$ of meter indication); max. output 100 mV (from $75 \Omega$ ). Price 3 s .

No. 5. Low-cost High-quality Loudspeaker by P. J. Baxandall (Aug. and Sept., 1968). Can be built for a few pounds! Excellent performance above 100 Hz but is improved if used with a woofer for the low frequencies. Price 5 s .

No. 6. Wireless World Crosshatch and Dot Generator (Sept. 1968). A pocket sized instrument using digital integrated circuits. Price 3 s .

In addition, the following reprints from earlier issues are still available:
Wireless World Oscilloscope: Main frame, X amplifier, E.H.T. unit (March June, July and August 1963), price 5 s ; No. 1. (audio) Y amplifier (Apri 1963), price 2s 6d; No. 1. (audio) Timebase Unit (May 1963), price 2s 6 d Calibration-Alternative E.H.T. Unit (Feb. and Oct. 1964), price 2s 6d; anc Wide-band Amplifier (April 1964), price 2s 6d.

Wireless World Audio Signal Generator (Nov. and Dec. 1963). Price 3s.
Wireless World Crystal-controlled F.M. Tuner (July 1964). Pulse counting type not suitable for stereo. Price 3 s .

Transistor High-quality Audio Amplifier by J. Dinsdale, (Jan and Feb. 19t Very popular 10W design. Price 5 s .

Wireless World Computer (Aug. to Dec. 1967). Eight-bit digital machine for instructional purposes. Price 10 s .

## Quasi-complementary Output Stage

## Modification

## A single diode used to overcome distortion at low listening levels

by I. M. Shaw*

The quasi-complementary output stage (Fig. 1) has differing input impedances for its upper and lower halves. This is because there are two emitter-base junctions in series in the upper half, but only one in the lower half. In the configuration of Fig. 2 it can be seen that the lower has an input impedance consisting of one emitter-base junction and one forwardbiased diode in series, which in practice should approximate to two emitter-base diodes in series. Thus it should be possible to construct a low distortion transformer-less output stage using one pair of low-current complementary transistors and one pair of identical output transistors.

An amplifier with an output stage similar to that in Fig. 1 was constructed, and the distortion levels measured down to 2 mW output at quiescent currents of $7 \mathrm{~mA}, 20 \mathrm{~mA}$ and 80 mA . The distortion was measured using a wave analyser (Marconi TF2330) and a low distortion generator (Marconi TR2100/ 1M1).

The results of the measurements are given in Fig. 3. From these it can be seen that at the normal quiescent current for

## - Wellbrook Engineering Electronics Lid

Fig. 1. Typical quasi-complementary output stage.

class $B$ operation ( 20 mA ) the total harmonic distortion rises to approximately $1 \%$ at 15 mW output from $0.1 \%$ at full output. This distortion is clearly well above the accepted limit for highquality reproduction and it can be seen to reduce as the quiescent current is increased towards class A conditions.

An amplifier was constructed with Fig. 2 as a basis, the complete circuit of which is given in Fig. 4. This second amplifier, which had the same amount of negative feedback as the previous amplifier, gave the results indicated in Fig. 5 at 20 mA quiescent current.


Fig. 3. Distortion characteristics of conventional amplifier with $7 \mathrm{~mA}, 20 \mathrm{~mA}$, and 80 mA quiescent current.


Fig. 4. Complete circuit diagram of modified power amplifier.


The amplifier was operated from a simple unstabilized power supply (Fig. 6), and the d.c. level at the output was set below half of the supply voltage so that the output voltage at full output would not be clipped due to the ripple-limited positive rail.

It can be seen from Fig. 5 that the distortion level does not rise, down to a measured output of $100 \mu \mathrm{~W}$, thus showing that the extra diode has equalized the input impedances giving a fourth and cheap alternative output stage for true high-quality reproduction.

The amplifier has successfully driven a Quad electrostatic loudspeaker without any instability and tests were carried out with the latter and with the simulated circuit (Fig. 7) which is the salient part as regards high frequency instability.

Above 15 W output the supply rails clip the output voltage giving rise to a large increase in the harmonic distortion levels, but up to this point the distortion level is extremely low.

## Literature Received

## CATAlOGUES

Connector Catalogue. The Electronics Division of Greenpar Engineering Lid., Station Works, Harlow, Essex, have produced a large catalogue devoted to various types of coaxial, twin-axial, and tri-axial connectors. In all variations on eight basic patterns are described and performance data given. WW 400 for further details.
"SGS Linear Microcircuits" is a catalogue published by Quarndon Electronics (Semiconductors) Litd, Slack Lane, Derby, which gives brief technical data, prices and application notes for a range of SGS devices


Fig. 6. Simple power supply used with amplifier.

Fig. 7. Test circuit equivalent to Quad electrostatic speaker.


Fig. S. Distortion characteristics of modified amplifier at 20 mA quiescent current.
including operational amplifiers, current sources, comparators, $A / D$ and $D / A$ converters. WW 401 for further details.
"Lemosa Cable Connector Catalogue" gives details of a range of multicontact, coaxial, tri-axial, bulkhead and thermocouple connectors which have a spring locking action. The catalogue contains an offer whereby you send them a cable and they will send you a connector to suit it. Lemosa Lid, Box 306, Shoreham-by-Sea, Sussex. WW 402 for further details.
"He-Ne Lasers". The Ferranti range of d.c. excited Helium-Neon lasers are described in this publication which is available from Ferranti Led, Laser Sales, Dunsinane Avenue, Dundee, DD2 3PN. WW 403 for further details
"CO $\mathrm{CO}_{2}$ Lasers', also from Ferranti, are described in a leaflet available from the above address. WW 404 for further details.
"Catalogue of Used Scientific Equipment" includes second-hand vacuum equipment, laboratory instruments, etc., available from V. N. Barrett anc Co. Lud, 1 Mayo Rd, Croydon, CRO 2QP. WW 405 for further details.

Supplement No. 3 to the 1TT (S.T.C.) Electronic Services component: catalogue has been published and lists the International Rectifier range 0. semiconductors. ITT Electronic Services, Edinburgh Way, Harlow, Essex WW 406 for further details.
"ISEP-ITT Standard Equipment Practice" is an 80-page booklet, avail able from the above address, which shows how numerous cabinets ans equipment racking systems can be made up from ISEP. WW 407 for furthe details.

## GENERAL INFORMATION

"Consumer Electronics" is the title of a new quarterly magazine fron Mullard. It covers radio and television and the use of electronics in othe appliances: electric blankets, washing machines, toys, watches, etc C.I.H./C.M.S. Dept., Mullard Ltd, Mullard House, Torrington Place, Lon don W.C.1. WW 408 for further information.

BS 4421:1969, "Digital input/output interface for data collection systems" is a development of a system devised by the National Physical Laboratory t enable their measuring and data processing devices to be easily set-up an connected for any particular application. Copies are available from BSI Sale Branch, 101 / 113 Pentonville Road, London N.1, price 12s.
"Export Markets for Electronics-E.F.T.A." is a 57 -page booklet whic has been produced by the Economic Development Committee for th Electronics Industry. It contains a great deal of interesting statistic: information covering the market for electronic products and scientifi instruments in E.F.T.A. countries. The Library, National Economic De velopment Office, $21 / 24$ Millbank, London S.W.1. WW 409 for furthe details.
Choice of careers booklet No. 66-"Radio and Television Servicing" ha been produced by the Department of Employment and Productivity. It available from H. M. Stationery Office, price 1 s 9 d .
"Become an Apprentice Technician with NATCS", is the title of pamphlet produced by the Board of Trade for the National Air Traff Control Service's Technician Apprenticeship Scheme. It can be obtained frol T. H. Mallett, Board of Trade (Civil Aviation Dept) Room 705, The Adelph John Adam Si, London, W.C.2.

In last month's Literature Received we inadvertently gave the address the advertising agents for Vitality Bulbs. Requests for information should ? sent to:-Beetons Way, Bury St. Edmunds, Suffolk.

## Wireless World

## Units Converter

## An aid to radio and electronics calculations

Available to readers of this issue (see coupon below) is a "slide rule" units converter specially designed by Wireless World's technical staff as an aid to calculation in radio and electronics work. Produced for us by the slide-rule manufacturers Blundell Harling Ltd, the instrument has 20 conversion scales, and other data, clearly engraved in rigid p.v.c., a plastic noted for its good mechanical stability and hard wearing quality. The scales are sufficiently expanded to give the degree of reading accuracy normally needed in each case (typically $0.5 \%$ of full scale), but the converter is small enough ( $7 \frac{1}{2}$ in long, 3 in wide) to be carried in a jacket pocket. The laws and limits of the scales have been decided on the basis of practical experience in various calculations. At the price of 12 s 6 d the converter is substantially cheaper than it would be if sold retail. In fact there is no equivalent instrument available on the market.
The converter provides the following facilities:
Wavelength/frequency. Two pairs of $\log _{10}$ scales, one pair ranging from 10 m to $10,000 \mathrm{~m}$, the other from 1 cm to 10 m .
-Frequency/angular frequency. Linear scales for conversion bet ween cycles per second (f) and radians per second $(\omega=2 \pi f)$. Range for f: 1.0 to 10.0 .
?eak/r.m.s. values (voltage, current, power) of a sinusoidal signal. Linear scales, peak values ranging from 1.0 to 14.14 .
Musical pitch/frequency. Linear/ $\log _{2}$ scales giving frequencies (in Hz ) of notes in the equally tempered chromatic scale. Range: twooctaves above middle C.

Loudness, phons/sones. Linear/ $/ \log _{2}$ scales relating loudness level (phons) to auditory impression of loudness (sones). Range: 20.0 to 120.0 phons.

Power ratio/decibels. Two pairs of $\log _{10} /$ linear scales: one pair, expanded scales, ranging from 0 to 10 dB ; the other pair, compressed scales, ranging from 10 to 100 dB .
Percentage/decibels ( $\log _{10} /$ linear scales). Can be used, for example, to convert harmonic distortion between a percentage and dB below a fundamental; or to convert between voltage or pressure ratios (expressed as \%) and dB . Range: $0.03 \%$ to $100 \%$.
Frequency (Hz)/period(s) relationship of a periodic signal. Two pairs of $\log _{10}$ scales: one pair, compressed, ranging from 1 Hz to 100 GHz ; the other pair, expanded, with $f$ ranging from 1.0 to 10 .

Magnetic field strength, oersted to ampere/ metre (SI unit) conversion. Two pairs of scales: one, $\log _{10}$, ranging from 1 milli-oersted to 10,000 oersteds; the other, linear, ranging from 1.0 to 10.0 oersteds.
Heat sink size for semiconductors. Scales giving area of $\frac{1}{8}$-inch aluminium sheet needed to secure the temperature/power dissipation ratio ( ${ }^{\circ} \mathrm{C} / \mathrm{W}$ ) permitted by the semiconductor. Range: 2 in to 12 in side of square.
Gas pressure conversion between torr ( mm mercury) and $\mathrm{N} / \mathrm{m}^{2}$ for low pressure or evacuation work. $\log _{10}$ scales. Range: $5 \times$ $10^{-8}$ to $2 \times 10^{-1}$ torr.
Inches/millimetres. Linear scales; range 0 to 12in.
Feet/metres. Linear scales; range 0 to 50 ft . Sq.inches/sq.centimetres. $\log _{10}$ scales, range 1.0 to $100.0 \mathrm{in}^{2}$.
Temperature, ${ }^{\circ} \mathbf{F} /{ }^{\circ} \mathbf{C}$. Linear scales, range $-20^{\circ} \mathrm{F}$ to $+320^{\circ} \mathrm{F}$.
Ounces/grammes. Linear scales, range 0 to $80 z$.
Pounds/kilogrammes. Log $_{10}$ scales, range 1.0 to 100.01 b .

Tabulated "easy" conversion factors, all powers of 10 (or nearly); for dynes/newtons; $\mathrm{dyn} / \mathrm{cm}^{2}$ to $\mathrm{mN} / \mathrm{m}^{2}$; angstroms/microns; gauss/tesla; ft candles/lux; joules/ergs.
$L$ and $C$ values, resonance and reactance.
Table of widely used frequencies with the $L$ and $C$ (preferred) values required for resonance. Also the corresponding reactances ( $\Omega$ ) and $L C$ products ( $\mu \mathrm{H}-\mathrm{pF}$ ).
Waveband names. $\log _{10}$ edge scales of the electromagnetic spectrum, marked in wavelength and giving waveband names. Range $10 \mu \mathrm{~m}$ to $100,000 \mathrm{~m}$.


The units converter in use. The conversion scales are engraved on the slider and are read through a víndow carrying a "cursor" line.

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## Mono into "Stereo"

# Techniques being used to make pseudo-stereo gramophone records from mono masters 

by Sean Davies*

The first half of 1969 has seen the virtual disappearance of new classical records in mono form, although light and popular issues will probably continue in mono and stereo for some time. This process will produce a climate in which the classical record buyer refuses anything which does not bear the magic word 'stereo'. Unfortunately many performances of great aesthetic value were recorded in mono only, so we have the increasingly familiar mono record processed into a stereo reissue-welcomed by some, despised by others.

Let us be clear on one point: given a complex single channel signal it is not possible to derive therefrom two separate signals bearing the correct temporal and spatial relationships characteristic of true stereo information. What is possible is a lessening of the point-source effect of a mono signal-in essence not too difficult, but there is one rather large fly in the ointment: for the present (and immediate future) the sales office demands that the record should be playable on mono apparatus without loss of quality. This rules out some of the methods of obtaining a spread of information, e.g. if a mono signal is fed equally to two loudspeakers the sound appears central, but if a portion of the signal is injected in antiphase the image will be spread. However, if the two signals are now combined, the anti-nhase relationship will prevent a satisfactory mono summation. In practice, a limited amount of phase difference is introduced in parts, usually confined to selected bands of frequen${ }^{*}$ General Recording Services
cies, and the result is checked by comparing the mono and stereo results on an A-B basis.

Two other means of separation are frequency division and selective reverberation. In its simplest form frequency division consists of feeding low frequencies to one and high to the other: this has the disadvantage that the harmonics of an instrument such as the cello appear on the opposite side from the fundamentals, while the player may seem to be dashing from loudspeaker to loudspeaker according to the note being played. Nevertheless, selected bands of frequencies may be divided as long as care is used. Reverberation can be added so that the ambience appears to come from an area other than the direct source point. Two possible methods are: (i) The mono signal is fed to a common drive unit on the echo device (chamber or plate), while two separate pick-up units give an apparently random mixture of return signals, which may be filtered before remixing with the direct signal. (ii) Two separate echo systems may be used, fed from different portions of the mono spectrum, the outputs being cross mixed, or a portion of the output of one being fed to the other in order to spread the effect.

It will be appreciated that any system of division is likely to suit one passage of music more than another, so in order to ensure the optimum conditions at any instant there must be an engineer with good reflexes and a complex control system following the score. An alternative system showing good promise allows the programme content to
control the division systems. For instance, two filter networks may have their active elements controlled by a voltage (derived from the mono programme) serving also to determine the relative reverberation and phase conditions. A subsequent cross-mixing of low frequencies ensures that the bass remains in position (often central) and assists good conditions for playback tracking. A further advantage of this system is that the active elements in the two channels may be balanced relative to one another so that at no instant is any part of the mono signal totally excluded from the outputs.

Actual figures for frequency spectra and levels used in division vary from disc to disc and from one company to another, but some general patterns may be noted. Brass instruments may be separated by a peak boost of some $6-10 \mathrm{~dB}$ at 5 to 6 kHz (which of ten improves the quality of the brass sound), although if strings are present this may not be possible as it lends a distinct edge to the violins. A very good concert hall ambience is obtained by setting the echo device (if adjustable) to a reverberation time of 3.5 seconds and delaying its input signal by a feu milliseconds in order that the first echo shall not arrive too soon and destroy the overall effect.

The space below has been left to avoid reader removing text when cutting out the coupon on the previous page for the Units Converter.
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## Circuit Ideas

## Schmitt trigger with "zero" backlash

 To the conventional Schmitt circuit ( $\operatorname{Tr}_{1}$ and $T r_{2}$ ) is added a level shifter $T r_{3}$, and an electronic switch $\operatorname{Tr}_{4}$. The circuit has two table states. When the input signal is

Schmitt trigger with "zero" backlash.
above the upper trip-point $T r_{1}$ is on, $T r_{2}$, $T r_{3}$, and $T r_{4}$ off and $R$ is in circuit. When the input signal is below the lower trip-point $T r_{1}$ is off, $T r_{2}, T r_{3}$ and $T r_{4}$ on and $R$ shorted. Lowering the value of $R$ will reduce backlash to zero. It is possible to go below zero "backlash" and cause the circuit to oscillate.
A. E. Crump,

Broadstone,
Dorset

## Linear scale power <br> meter

A usually undesirable property of semiconductor diodes - curvature of the $I / E$ characteristic at low forward voltages - is exploited in this circuit. The curvature approximates a square law for most diodes so that $I_{\text {diode }} \propto E^{2}$ while for power in a resistive circuit, $P \propto I^{2}$ or $E^{2}$. Thus if a suitable fraction of the voltage across the load is used to feed a diode and meter then:

Meter indication $\propto I_{\text {diode }} \propto E \mathcal{Z} \propto P$ i.e. the meter scale will be linear.

Type OA85 diodes were chosen as their characteristics closely follow a square law up to $1.3-1.4 \mathrm{~V}$.

The circuit illustrated has $30,20,10$ and 5 watt full-scale ranges at an impedance of 15 ohms, but by changing the input resistors

$R_{1,2,3,4}$, it may be adapted for other impedances and powers, provided that no more than 1.4 V is applied to the bridge input. K. D. James,

Fiji Broadcasting Commission.

## A non-blocking limiting amplifier

The need arose for a simple capacitancecoupled amplifier to amplify small signals (about 1 mV ) without blocking after receiving a train of large signals (a few volts).

In the circuit shown, the zener diode conducts when the signal tries to turn the transistor off. The transistor remains conducting until

the current from the signal source exceeds a value of about $\left(V_{C C}-V\right\rangle / R_{C}$; the transistor is then cut off. Diode $D$ prevents the negative part of the signal waveform being passed on to the next stage through the zener diode.

Two such amplifier stages together were used in a design for a microwave Doppler radar speed meter.

## F. Hibberd,

The University College,
Dar es Salaam,
Tanzania.

## Synchronized oscilloscope timebase generator

This unit gives a perfectly linear saw-tooth output that can be varied over the frequency range 1 Hz to 150 kHz . The synchronization circuit incorporated has an input impedance of $1 \mathrm{M} \Omega$ and is easily locked to low-level ' Y ' amplifier signals. A beamblanking output pulse is also available. $\mathrm{Tr}_{3}$ is connected 'upside-down' in the bistable to eliminate leakage problems. Linear charging of the tuning capacitor, $C_{T}$, is achieved by using $T r_{1}$ as a constant current source. Frequency is altered by $R_{V_{1}}$ and the different ranges obtained by altering the value of $C_{T}$ as follows:
\(\left.\begin{array}{rr}Frequency range \& C_{T} <br>
1 \mathrm{~Hz}-15 \mathrm{~Hz} \& 20 \mu \mathrm{~F} <br>
10 \mathrm{~Hz}-150 \mathrm{~Hz} \& 2 \mu \mathrm{~F} <br>
100 \mathrm{~Hz}-1.5 \mathrm{kHz} \& 0.2 \mu \mathrm{~F} <br>
1 \mathrm{kHz}-15 \mathrm{kHz} \& 0.02 \mu \mathrm{~F} <br>

10 \mathrm{kHz}-150 \mathrm{kHz} \& 0.002 \mu \mathrm{~F}\end{array}\right\}\) mylar | reversible |
| :--- |
| tantalum |

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# Operational Amplifiers 

## 5. Applications

by G. B. Clayton,* B.Sc., A.Inst.P.

## Bridge Amplifiers

In instrumentation systems using resistive transducers the transducers are normally included in the arms of a balanced bridge. Changes in the physical variable to which the transducer is sensitive cause an unbalance in the bridge, the extent of the unbalance being used to measure the change in the physical variable. Thermistor bridges for temperature measurement and bridges using resistive strain gauges are examples of such systems. Op. amps. are well suited for application in such balanced bridge circuits.
The most suitable configuration depends upon the particular application. Here are some of the points that have to be considered in choosing a particular circuit: earthed or floating bridge voltage supply; earthed or floating unknown resistor; output voltage linearly related to changes in the unknown resistor for both large and small changes; sensitivity of the arrangement dependent on the bridge impedance level (this will determine whether or not the circuit is affected by temperature changes affecting all the arms).
Bridge supply earthed (no amplification).


But

$$
\mathbf{e}_{\mathbf{A}}=\mathrm{e}_{\mathbf{B}}
$$

Substitution and rear rangement gives

$$
e_{0}=\left[\frac{R_{4}-\frac{R_{2}}{R_{1}} R_{3}}{R_{4}+R_{3}}\right] E
$$

Features. The circuit is basically an application of the adder subtracior amplifier previously discussed. It may be used in two ways.
(a) Make $R_{1}=R_{0}$, and $R_{2}=R_{x}=R_{0}(1+\boldsymbol{x})$ the unknown; make $R_{3}=R_{4}=R$. Substituting these values in the expression for the output voltage gives $e_{n}=\alpha . E$. Used in this way the circuit gives an output voltage which is linearly dependent upon ( $R_{x}-R_{o}$ ), the difference between the unknown and standard. This linearity is maintained even for large deviations. The output is independent of bridge impedance levels. The circuit does not provide amplification and the measurement of small resistance changes may necessitate the addition of another amplifier to increase sensitivity. The unknown resistor is floating. (b) If it is required to earth one end of the unknown and to perhaps drive quite large currents through it then we put it in another arm of the bridge. Make $R_{3}=R_{R}$. $R_{1}=R_{x}=R_{0}(1+\alpha)$ and $R_{1}=R_{2}=R_{\text {. }}$. Used in this way the amplifier does not need to carry the current passing through $R_{o}$ and $R_{y}$ and it is practicable to use large currents. The output voltage is now $e_{0}=(\alpha /[2+x]) E$. The output is now linear only for small deviations in the unknown ( $\alpha \ll 2$ ). In both arrangements the maximum common-mode voltage for the particular op. amp. in use must not be exceeded.

Amplification with Bridge Supply Floating.


The feedback circuit forces the amplifier to develop a voltage at the point $A$ which is equal and opposite to the unbalance voltage developed across the bridge. The bridge unbalance voltage is

$$
\frac{E}{2}-\frac{E}{R_{0}+R_{0}(1+\alpha)} R_{0}=E \frac{\alpha}{4\left(1+\frac{\alpha}{2}\right)}
$$

The voltage developed at $A$ by $e_{0}$ is

$$
e_{0} \frac{R_{1}}{R_{1}+R_{2}}
$$

Equating and rearranging gives.

$$
e_{0}=\left\{1+\frac{R_{2}}{R_{1}}\right\} \frac{E}{4}\left(\frac{\alpha}{\left(1+\frac{\alpha}{2}\right)}\right.
$$

Features. The circuit is basically al adaptation of the inverting amplifier and a such has no common-mode voltage limita tions. The output does not depend o bridge impedance levels; it is linear for sma deviations in the unknown $\left(\begin{array}{l}\alpha \\ 2\end{array}<1\right)$. Th bridge unbalance voltage is amplified $b$ ( $1+R_{2} / R_{1}$ ). The necessity for a floatin bridge supply may sometimes be a di: advantage.

Amplification with Earthed
or Floating Supply.


Feedback maintains the opposing corners of the bridge at equal potential; the amplifier output voltage establishes the differential current needed to balance the bridge. Using a single supply with the lower end of the bridge earthed:
Summing currents at A

$$
\frac{E_{5}-e_{A}}{R_{0}}-\frac{e_{A}}{R_{0}}+\frac{e_{0}-e_{A}}{R}=0
$$

Summing currents at B

$$
\frac{E_{5}-e_{B}}{R_{0}}-\frac{e_{B}}{R_{0}(1+\alpha)}-\frac{e_{B}}{R}=0
$$

Equating $\mathrm{e}_{\mathrm{A}}=\mathrm{e}_{\mathrm{B}}$ and rearranging gives

$$
e_{0}=\frac{R}{R_{0}} E_{9} \alpha \frac{1}{(1+\alpha)\left(1+\frac{R_{0}}{R}\right)+1}
$$

Features. This circuit may be used with a earthed bridge supply but the sensitivity dependent on bridge impedance levels.
linear output is obtained for small deviations ( $\alpha \ll 1$ ). The amplifier type used should be insensitive to the possibly quite large common-mode voltage level at the input.

Solar Cell Amplifier.


Features. In the circuit shown the polarity of the output voltage is dependent on the relative intensity of the light falling on the two cells. Circuits of this type are useful in measuring small deflections of a beam of light.

## Photodiode Amplifier

A photodiode is essentially a reverse biased p-n junction, the reverse leakage current through the junction being dependent on the illumination falling on the junction. In use the diodes are connected in series with a high value resistor, but the input resistance of a

general purpose op. amp. is normally not high enough to allow it to be connected directly to this circuit. A transistor capable of operating at low currents and acting as an emitter follower can be used to increase the input resistance. A balanced input stage is used to reduce temperature drift. The gain of the amplifier is set by the choice of $R_{2} / R_{1}$.

## Light Level Detector

A variation of the photodiode amplifier employing positive feedback can be arranged so that when the light intensity falling on the cell reaches some fixed level the amplifier output switches between saturation states. With no light falling on the photodiode the phase inverting terminal of the op. amp. is positive with respect to its other input terminal and the amplifier is in negative saturation. Light falling on the cell causes the potential of the phase-inverting terminal to fall, and when the amplifier comes out of saturation positive feedback applied via $R_{1}$ and $R_{2}$ causes a regenerative switching action which drives the amplifier to positive

saturation. If the light intensity is reduced a regenerative action returns the amplifier to its negative saturation value. The circuit exhibits hysteresis.

## A.C. Amplifiers

Op. amps. are basically high-gain d.c. amplifiers, but they are equally suitable for applications not requiring a d.c. response. In such cases d.c. blocking capacitors are used in the signal path, and it is often possible to operate the amplifiers with a single power supply and a split zener biasing or resistive network divider technique, thus reducing the requirement for separate positive and negative supplies.

Phase Inverting A.C. Amplifier.


The basic inverter amplifier with capacitor $C$ in series with the input. The gain of the amplifier is $R_{2} / R_{1}$ with the low frequency 3 dB fall in gain occuring at a frequency $1 /\left(2 \pi C R_{1}\right)$. The upper frequency limit of the amplifier will be dependent on the loop gain and the compensated open-loop frequency response (see March article). The input resistance is $R_{1}$.

Non Inverting A.C. Amplifier.


Basically the follower with gain with the addition of blocking capacitors and the d.c. bias path $R_{3}$. The gain of the amplifier is $\left(1+R_{2} / R_{1}\right)$ with low frequency 3 dB frequency determined by the shorter of the two time constants $C_{1} R_{1}, C_{2} R_{3}$. The input resistance is $R_{3}$.

High Input Impedance A.C. Amplifier.


The non-inverting amplifier, being a voltage follower, is intrinsically capable of providing a high input impedance, but this is reduced in the simple follower by the d.c. biasing path $R_{3}$. In this circuit positive feedback is applied from the output via $R_{2} C_{1}$ and $R_{1}$ to the lower end of $R_{3}$. This results in a large effective input impedance. The technique of raising the apparent value of an impedance by driving its low potential end with a voltage in phase with, and almost as large as, the voltage at its high potential end is known as 'bootstrapping'. The gain of the amplifier is $1+R_{2} / R_{1}$ and the effective input impedance is increased by a factor equal to the loop gain; e.g. if the closed-loop gain is, say, 20 and the open-loop gain of the amplifier is 4,000 , the effective value of $R_{\mathrm{s}}$ is increased 200 times.

## Frequency Selective Amplifier

This is a bandpass amplifier employing a twin-T filter. The circuit uses the inverting feedback configuration, and in order to develop a specific frequency response characteristic the feedback path is made to

Choose $C_{1}$ so that $C_{1} R_{1}>C R$

$$
\text { Peak gain } \bumpeq \frac{R_{2}}{R_{1}}
$$

Input impedance $\bumpeq \mathrm{R}_{1}$
include a frequency selective network-a twin-T network in this case. The twin-T is a rejection filter and has a high impedance at its characteristic frequency; the feedback is thus a minimum and the gain of the amplifier a maximum at this frequency.

## Letters to the Editor

## The Editor does not necessarily endorse opinions expressed by his correspondents

## Base-connections of f.e.ts

It has come to my notice that various suppliers of field effect transistors are publishing misleading information in their catalogues regarding the arrangement of the lead connections of these devices. The compilers of these catalogues have assumed that the manufacturers have followed the logical arrangement of: collector $=$ drain; base $=$ gate; and emitter $=$ source.

Unfortunately this is not so-even particular makes vary. The following examples from the Motorola range illustrate the point:


Several colleagues and I have spent many hours attempting to get MPF 102s to function-following the connections given in the retailer's catalogue, only to find that this information was wrong and that the devices had probably "gone down the drain"!

If nothing can be done by the makers to identify the leads, either on the device or in the packet, would you please give this letter the widest publicity as we feel sure that other users are also being misled.
T. N. Lloyd (G3SL),

Hounslow,
Middx.

## Labelling components

I should like to back up Mr. Short's suggestion that Wireless World adopts, what he calls the Continental practice of abbreviating component values in circuit diagrams, but I should also like to point out the inconsequence in mentioning only the resistors and omitting the capacitors (and the coils for that matter).

It seems obvious that the safety in reading resistance values, which is certainly gained by the adoption of the "Continental" practice of replacing the decimal point by the multiplier abbreviation, has even more bearing on the labelling of capacitors.

Surely, it necessitates the further
adoption of a couple of multiplier abbreviations to which many British and American engineers seem somehow adverse, namely " m " for $10^{-3}$ and more important " n " for $10^{-9}$. It seems to me that the ease gained in reading and pronunciation justifies the necessary effort to get used to it. Here are a few examples:
for $0.0016 \mu \mathrm{~F}$ write $\ln 6$,
for $0.027 \mu \mathrm{~F}$ write 27 n ,
for $0.68 \mu \mathrm{~F}$ write 680 n ,
for $1000 \mu \mathrm{~F}$ write 10 m .
Exactly the same applies to the coils, these also often having values of fractions of the unit. Mogens P. Muller,
Copenhagen,
Denmark.

## Improper oscillations in transistors

D. B. Pitt describes "improper" oscillations on page 20 of the January, 1969 issue. Relaxationtype signals are obtained with an n-p-n planar silicon transistor in a simple $R C$ circuit.

Some years ago, I carried on similar experiments with $\mathrm{p}-\mathrm{n}-\mathrm{p}$ germanium transistors. See Fig. 1, which has two unusual features: (a) the base is not connected (b) the output is a sine wave-about 0.5 V at 7 kHz !

As $R_{2}$ is decreased to raise the current, an oscilloscope across $R_{1}$ or the transistor will indicate a sinusoid at approximately 0.4 to 0.6 mA . If the current is increased further, the sine wave will disappear. Not all transistors tested gave this unusual result. I used 2N112 and CK 768 (Raytheon) transistors. My experiments were described in RadioElectronics, August, 1959.

More recently, I found that various n-p-n silicon types seem to generate saw-tooth or pulse signals, and at much lower currents. I used Fig. 1 with reversed polarity. In all cases,


Fig. 1
the voltage across the transistor tends to remain at a peak value as $R_{2}$ is varied. For a 2 N112 this is approximately 20 volts, so a $22 \frac{1}{2}$ volt battery may be used. For a 2 N 2501 , it is about 26 volts, and for a 2 N 2712 it is about 48 volts.
I. Queen,

Radio-Electronics,
New York,
U.S.A.

## Do manufacturers really want to sell?

I am currently an undergraduate in electrical engineering and a radio amateur. One day, after graduation, I will perhaps be required to obtain some component or assembly in quantity for my employer. Because of my past experience I know even now to whom I shall turn. The odd thing is -almost all such places I can think of are American.

Example: A casual request for some information on a component resulted in the whole catalogue, plus reply-paid cards should I need more information on any thing else, being sent to my home address. I was not once asked if I were in business. The company was American.

An even more modest request for pamphlet, to an English firm resulted ir my being told that this prized documentwas not really available to the genera public, however, a special case would be made if I were prepared to pay 6 d plus postage.

These are not one-off examples, nor am I prejudiced (yet) but the facts are where public relations are concerned the Americans are our tutors and we are unwilling pupils.

Okay, so you can't supply the British Isles with firelighters-but you don't have to. All you have to do is generate goodwill, not only to your immediate market but also to the public at large.

Subsidies and tariff controls are like penicillin, one can become immune and trade protection is then lost, and it is ther too late to "get your finger out" because somebody will have cut off your hand.
L. Kennedy,

Southport,
Lancs.
'Vector' makes several points in his March article about 'Jim Bandstop', but at least Jim was able to start his business and doubtless Jim himself would agree wholeheartedly about the structuring of companies. Now as far as the structure of his own company was concerned, he at least had some choice. What is, however, quite intolerable is the degree of external interference from such people, for instance, as Vector mentions, the Inland Revenue.

Even these people, and all the other multitudinous Government agents, have at least the defence that they have no vested interest in the success of the business. Quite incomprehensible from any point of view is the attitude taken by the component suppliers in whose interests it surely must be that any business thrives.

May I relate my own experiences in starting a small business in my spare time, as most businesses start.

I have dealt direct with several manufacturers or agents, sometimes for single orders in the $£ 50-£ 60$ region and have had no suggestion of any difficulty in opening an account, with no preliminaries such as giving references. All bills have been paid within two weeks of receipt.

Not so happy however have been my dealings with the component wholesalers. Radiospares flatly refused to allow me to open an account unless I had a Registered Office open at least six hours a day,

Finally, I forwarded a 'cut-out coupon' from one of your advertisements for C.E.S. applying for a catalogue, and received in reply a duplicated letter, unsigned, asking me to give two trade references and the name of my bankers, so that, if my premises are correctly rated, I may receive a catalogue. What they would require if I wished to open an account, I hate to think!

As I mentioned earlier, my business is at present only part time. It does not seem to have occurred to any of these companies that I also have control of ordering thousands of pounds worth of goods for the company I am employed by.
J. C. TAYLOR,

Heywood,
Lancs.

## Negative feedback and hum

Whilst I must congratulate Mr. G. W. Short on his extremely ingenious circuit for reducing hum in class B single-ended push-pull outpui amplifiers (March issue), I suggest it is better to attack the problem at its root. This particular amplifier (Fig. 1) produces hum on its


Fig. 1. G. W. Shori's original amplifier


Fig. 2. Amplifier re-designed for common positive earth line


Fig. 3. Negative earth amplifier
output because the negative rail is used as the input "earth", and the positive rail as the output "earth". Since the liberal negative feedback ensures that there is negligible ripple on the output terminal, with respect to the negative rail, it follows that virtually the whole of the supply voltage ripple appears between the output terminal and the positive terminal. Fortunately it is very easy to redesign this amplifier so that the same rail is used for both input and output earth (positive), thus eliminating this problem (Fig. 2). If a negative earth amplifier is required, it is necessary merely to "invert" the circuit, using the same transistors in different positions (Fig. 3). D. Austin,

Birmingham, 24.
The author replies:
The most elegant solution to the hum problem is certainly to use a circuit which doesn't have it. One of my purposes in writing about my experiences with a particular amplifier circuit was to warn others of the problem, so that they could take avoiding action. When one gets down to actual cases, however, the solution may not be quite as simple as Mr . Austin's circuits suggest. For one thing, it is quite likely that the amplifier will be used with a pre-amp in a 'negative earth' configuration, in which case his Fig. 2 will be a non-starter. For another, it may not be permissible to swap $T r_{1}$ and $T r_{2}$ around to make possible Fig. 3. My own amplifier used a low-level p-n-p planar transistor type 2 N 4058 in the input stage and a medium power n-p-n planar type BFY51 as driver. Swapping these types around is not possible, because the 2N4058 won't handle the current needed in the driver stage, while the low gain of the BFY 51 makes it unattractive as an input transistor. This may seem a mere quibble, but when one looks for a p-n-p driver equivalent to the BFY 51 one discovers that it is expensive. If an extra smoothing capacitor can be obtained cheaply (they are much easier to find on the 'surplus' market than good p-n-p silicon driver transistors) then the 'swinging diode' smoothing circuit may be the most economical solution after all.

There is a further snag about Mr. Austin's circuits. This is that they may be found to exhibit an unexpectedly high hum level! Inspection of Figs. 1 and 2 shows that they both offer an entry point for ripple from the supply line. This is the emitter of the driver transistor, which goes straight to the unearthed side of the supply in each case.

Some readers have enquired about diode types for the smoothing circuit. Any silicon rectifier which will handle the current will serve. The reverse-voltage rating is of no importance. Selenium rectifiers will also work:
they start to conduct at about the same forward voltage but may have a greater forward drop at full current. A selenium bridge can be connected so as to be equivalent to two diodes in series.
G. W. SHORT

## High-quality TV sound

With regard to the comments in the April issue about high-quality television sound, I would agree entirely with Mr. Dinsdale about the position of the sound source.

Due to space considerations, anyone watching my set has to sit between it and the hi-fi speaker I use for the sound, thus the sound comes from behind the viewer. Everyone who has watched it has been quite amazed at the way the sound seems to come from the screen when actually watching it.

As regards extracting a high-quality sound signal, I simply earth all my equipment to the neutral side of the mains and take the sound from the output of the post detector stage as one would do with an ordinary radio. This is not as dangerous as it might appear since all the mains plugs are three pin and thus cannot be plugged in the wrong way round.

The quality of the sound thus obtained, when fed through a normal domestic hi-fi system can be surprisingly good. Although not as good as that of the Band II f.m. transmissions, it compares very favourably with that of the monitors used at the B.B.C. and I.T.A. transmitting stations I have visited.

On tape recordings made in this manner it is just possible to hear the 405 - and 625 -line scan whistles, but they are not normally noticeable.

I have tried this method of sound extraction with two sets and found in both cases that mains hum could be troublesome due to the slight voltage drop in the TV mains feeder. The cure for this is to connect the TV chassis direct to the hi-fi amplifier's earrh. Also, a significant improvement in treble response was obtained on removing the sound interference limiters on both sets.
B. Pollard (aged 18), Sheffield 10.

## Groove jumping on records

On both sides of the Atlantic one reads that a gramophone record has a "jumping groove", although what presumably is meant is that the cartridge needle jumps. The more important question is whether it is correct to speak at all of a "jumping" needle. Does the needle actually jump-that is, more correctly, is it thrown by the one groove wall over the opposite groove wall?-or does the groove wall, over which the needle is said to "jump", in fact pass under the needle? Or, again, is it sometimes the one, sometimes the other, and sometimes both occurring simultaneously? When I say that the groove wall passes under the needle-to me, the more likely cause of a needle missing one spiral of a groove-I mean that the one groove wall can undergo so violent an excursion that the groove moves out from under the needle, whichinertia and insufficient compliance hold more or less rooted to its original position.

It would seem that where the skating force is exactly neutralized, a needle should miss a spiral as often in the one direction as in the other, the only determining factor being (assuming that the needle, suspension, and damping material have exactly symmetrical characteristics in all directions of movement) whether the excursion causing the needle to miss moves towards or away from the centre of the disc. In the past, of course, owing to the skating force, it was usually the next groove inwards that came to be occupied by the needle.

Can any reader support or demolish my speculations?
Ronald Klett,

## Loerrach,

W. Germany.

## Folded exponential horn loudspeaker

I was delighted to read the abstract of J. Jecklin's article in February's Wireless World.

I do not feel, however, that Mr. Jecklin's high frequency arrangements represent the most satisfactory system. The power handling capacity of two Axiom 80s is far in excess of any domestic requirement and suitable arrangements give satisfactory distribution of sound from a single speaker.

My suggestion is to fit the high-frequency driver into a simple horn, mounted so as to reflect the sound off the corner of the room, or, if the ceiling be low, the ceiling. The horn loading restricts the movement of the cone ensuring negligible out-of-phase sound output from the rear of the cone. With Mr. Jecklin's arrangement this out-of-phase signal could be reflected off the walls to produce irregular response.

A further improvement, which I have made to my own speakers, is to cross over from the Lowther speaker at 4 kHz into a Decca-Kelly ribbon DK30 using the crossover details of which are given in Fig. 1 and the scheme of connection in Fig. 2. The crossover provides a transformer function increasing the drive to
the ribbon to bring its apparent sensitivity into line with the rest of the system. The ribbon unit is readily mounted on the outside of the horn of the mid-range speaker and similarly aimed so that its output too is reflected and dispersed. The Kelly acoustic lens should not be used in this arrangement.

The inclusion of the ribbon unit is well worthwhile as transient performance is improved and the smooth response minimizes listener fatigue, and background noise. For really noisy programme material the ribbons may be switched off-a filter far more effective than that in the amplifier.
Since Mr. Jecklin wrote his original article development has taken place in electrostatic mid-range speakers and readers should bear them in mind as a possible advantageous replacement for the p.m. unit. Mr. Peter Belt (Duode Ltd, Leeds) is marketing electrostatic speakers in which the matching transformer is replaced with advantage by a valve amplifier which also makes up for the lack of sensitivity of the electrostatic speaker. I have, however, found it necessary to retain the ribbon but to feed the h.f. range into the electrostatic panels and to feed the ribbon using the crossover as a high-pass filtertransformer only (see Fig. 3).

With the suggested arrangements the 16 ohm resistor can come out of Mr. Jecklin's crossover and the efficiency of the system rises to circa $40 \%$. This now gives rise to important considerations concerning the amplifier, a matter of milliwatts making a very pleasant sound level in a small room. The sizeable sum of money spent on the speaker can now be recouped on the amplifier.

The appended $2 \times 2$ watt circuit (Fig. 4) provides the audibly faultless quality and unconditional stability found only in the best professional studio amplifiers. Heat dissipation of 70 W is no greater than a large valve table radio and cost should not exceed $£ 8$. It has not been found possible to reduce the heat dissipation without degrading the sound but suggestions are very welcome as users of insensitive speakers would like to build more
powerful versions that are not at the same time central heating systems.

Readers having no constructional facilities might consult Mr. C. Telfer, Caverton, Kelso, Roxburghshire, Scotland, who specializes in horn speaker construction.
I. G. Abelson,

London N. 14.


Fig. 1. Crossover circuit supplied by Stanley Kelly. Cores: Mullard FX 1007 (E) and FX 1107 (I). Spacer 0.036 in.


Fig. 2


Fig. 3


Fig. 4 One channel and power supply for 2 -watt amplifier. RFC $_{1}=$ Radiospares 1 A television suppressor choke; RFC $_{2}$ $=2 \mathrm{~A}$ version.

## Modified Treble Filter for Bailey Pre-amplifier

In the pre-amplifier described by the author in the December 1966 edition of Wireless World, the presence of the treble filter affected the performance of the tone control in that the full boost and cut ranges were not available. In addition, ferritecored inductors of high " $Q$ " value gave unwanted ringing in the circuit.

These defects have only recently become clear, and a modified filter circuit has been designed to overcome them. This is shown in Fig. 1. The cut-off frequency of the filter is now dependent on only one capacitor, in that the cut-off frequency can be varied from 4 to 11 kHz merely by changing the value of the output terminating capacitor. The values given in Fig. 1 represent the limiting values of common usage, capacitor values between these limits giving intermediate values of cut-off frequency.

The inductor is damped by the series resistor to such an extent that variations in inductor " $Q$ " have little effect on the performance. Equally with the filter in the "out" position it is now removed completely from circuit and does not affect the amount of treble boost available. The overall transient response of the filter is quite satisfactory as can be seen from the square-wave response photograph shown in Figs. 3 and 4.


Fig. 1. Modified treble-filter circuit.


Fig. 2. Performance of modified circuit.


Fig. 3. Response to 1 kHz square-wave with $40,000 \mathrm{pF}$ capacitor


Fig. 4. As Fig. 3 but with 10,000 pF terminating capacitor

The inductor size was maintained identical to that in the original circuit so that modification entails a minimum expense.
A.R.B.

## Books Received

Solid State Electronics by G. Fournet, edited by S. Chomet. This book, translated from the French, investigates the laws governing the motion of electrons in a crystalline medium. It falls into four parts. The first part is a thorough treatment of quantum theory, from first principles, which should be followed without difficulty by anyone with no more than a grounding in the ideas of quantum physics. The second part deals more specifically with the theory of electrons in metals. The third and longest section deals with semiconductors, and with the detailed theory of the working of diodes and transistors. The last section is a discussion of magnetic phenomena including ferro- and anti-ferro-magnetism, and ferri-magnetism. Typical numerical examples are worked out to show what magnitudes may be expected in practice. Pp.308. Prices 70s hard-back and 38s limp. Iliffe Books Ltd., 42 Russell Square, London W.C.1.

Management of Research Development and Design in Industry by T. S. McLeod. The author is Company Technical Co-ordinator with the Plessey Company and responsible for the inauguration and control of much of their research. The creed of this book is that expenditure on research and development is wasted without planning and control and that the design process itself must be properly managed. Guidance is given in setting up objectives for industrial research. Details of budgeting, staffing and day-to-day control are described in practical terms. The book ends with four detailed case studies of research, development and design management in action. Pp.260. Price $\{3$. Gower Press L.td., 13 Bloomsbury Square, London W.C.1.

# Computer Aided Design 

A short interpretation

Computers have been used in engineering design ever since they became available to engineers, which has been for about twenty years. Why, then, all the excitement about this apparently new subject called "Computer Aided Design" (or "CAD" as it has become known, perhaps because it is not the gentleman's way of doing things)? It could be, of course, that those responsible for organizing conferences and publishing books and journals-the professional communica-tors-have only recently discovered what has been going on. Another reason may be that what started in a fragmentary way twenty years ago has only now gathered sufficient body to become autarkic. Yet another explanation could be that computers have suddenly become human, in the sense that the engineer can now conduct a "conversation" with them with the aid of verbal or graphical peripheral equipment.
The c.a.d. conference at Southampton Un -

> I.E.E.
provided a good opportunity to see what is being done in electronics design (the conference was concerned with computer aided design of almost anything, but electrical and electronic producis were predominant). There seem to be three main areas of application: (1) circuit analysis and synthesisusing computing techniques to find the circuit values necessary to uchieve optimum or specified performance or production yield; (2) physical layout-achieving the optimum spatial arrangements of circuit elements and connections in printed circuits, i.c. and I.s.i. devices, thin or thick film sub-assemblies, or conventional electronic equipment; (3) system design by simulation or testing-using the computer as a model on which to try out a likely system before construction, or to test a system already built.
In almost all c.a.d. projects the computer used is a digital machine. Analogue computers although particularly well adapted to certain jobs, such as system simulation in "real time", are restricted in range of ability because each piece of their hardware can perform only one specific operation (e.g. adding, multiplying, integrating).

What is perhaps rather mystifying is how a machine for handling numbers can deal with spatial and topological information, as in printed-circuit layouts or electronic circuit configurations. With spatial patterns the principle is simple: any point in space can be specified numerically in terms of Cartesian or polar co-ordinates within some arbitrary frame of reference; thus numerical descrip-
tions of points, lines, areas and volumes are possible. With electronic circuit topology the transformation is usually done by the use of nodes-that is, all the common connection points, or nodes, in a circuit are labelled with code numbers, then the position of each component in the circuit is specified by the code numbers of the nodes to which it is connected. This process, of course, can also be applied to the nodes of equivalent-circuit "models" of single devices such as the transistor. Branches (the paths containing components between nodes) are also used and similarly numbered.

By such techniques the computer can be made to do what the engineer normally does with diagrams and drawings in the design process, repeatedly recording and modifying. With straightforward calculations, e.g. using Ohm's or Kirchhoff's laws in circuits, the computer does essentially the same as the engineer with his slide rule-but more of it. Correct or optimum design is a matter of trying a succession of different arrangements in a systematic manner that approaches the desired result by degrees-very tedious and perhaps impractical for an unaided engineer to do exhaustively. Mathematically, however, it is an iterative, convergent process and therefore very suitable for handling by a mathematical machine such as a digital computer, which is ideal for repeating a given calculation with different sets of numerical values. For example, a typical electronics design process might call for calculating the steady-state response of a circuit at numerous frequencies for every possible value of every component in the circuit.

The following short descriptions of papers from the Southampton conference give some idea of current activity in c.a.d. as applied to electronic engineering.

## Circuit analysis and synthesis. Computer

 programme to solve the currents and voltages in a transistor-resistor network under steady applied voltage conditions (A. M. MacSwan). Determining circuit element nominal values and maximum allowable tolerances to achieve responses within specified constraints (G. J. Herskowitz, M. A. Murray-Lasso). A general d.c. analysis programme for non-linear circuits: allows the user to take the model provided or build up his own model (H. M. Davison). Worst-case a.c. analysis using signal-flow graphs (G. W. Zobrist). Specifying a circuit with the aid of an alpha/numeric/graphical display: the requirements of a given circuitanalysis programme are automatically met as the engineer is guided in a sequence of actions by instructions from the computer itself (J. A. Weaver). Obtaining optimum yield in production: finding the set of nominal component parameters, with given probability density functions, that gives the maximum number of satisfactory circuits (F. Jensen). Taking account of non-idealities of active devices in circuit analysis and applying corrections (J. I. Sewell, C. Nightingale).

Physical layout. Computer programming language for specifying layouts for i.c. masks: takes advantage of redundancies arising from parallel sides of shapes, repeated shapes in one circuit, patterns common to a range of circuits (J. Wood, et. al.). Programmes for designing layouts of circuit modules in large equipments (computers) to achieve minimum functions of the wiring, e.g. minimum total length of wire (J. Houghton). Trial layouts of thin-film microcircuits: programme deals with component dimensions, placement and interconnections and displays result on a digital incremental plotter (W. J. Cullyer et. al.). Programme using graphical display to allow intervention by the designer for semi-automatic design of printed circuit boards: placement of packages and arrangement of interconnections (D. F. A. Leevers). C.r.I. display and pat-tern-generating computer programme as an aid to designing i.c. masks: when a design is completed dimensional information is stored on magnetic tape to control a mask cutting machine (J. Atiyah). Programmes for automatic design of 1.s.i. two-layer interconnection patterns (P. E. Radley).

System design by simulation. Programme for simulating a digital processor of a doppler radar system (J. H. Blythe et. al.). "Conversational" programme for simulating logic sub-systems on a time-sharing computer: circuit description, input and required output are fed in as data and can be modified at will while the programme is running (J. S. Reynolds). Logic simulation programme capable of being expanded and modified according to experience with practical examples: includes TTL74 and DTL900 series of i.cs (P. C. Gorton, S. P. O'Byrne). Testing logic networks by simulation: system being developed is designed to reduce computing $\operatorname{costs}$ (A. A. Kaposi).
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## Personalities

Group Captain E. Fennessy, C.B.E., is the new chairman of the National Industrial Space Committee set up by the Society of British Aerospace Companies, the Electronic Engineering Assoc., and the Telecommunication Engineering \& Manufacturing Assoc. Grp. Capi. Fennessy is managing director of Plessey Electronics Group which he joined in 1965 after 20 years with the Decca organization, latterly as managing director of Decca Radar Lid. The N.I.S.C. is responsible for co-rdinating the views of this country's industries involved in space-vehicles and associated control and communications systems.

Douglas H. Bolton, M.B.E., who is 48 and joined Newmark Instruments Lid $3 \frac{1}{7}$ years ago as chief project engineer, is appointed manager of the company's Control Engineering Division. He was with Elliott Automation as a technical manager for eight years on de velopment of aircraft /missile control systems prior to which he was from 1956 to 1958 chief systems engineer with Sanders Roe Lid on "Black Knight" rocket development. During World War II, from 1939 to 1946, Mr. Bolton served in the Army and for $2 \downarrow$ years was a senior lecturer on radar and electronic control equipment at a R.E.M.E. Technical School. After the war he served as a civilian technical officer in the War Department and in 1951 was appointed an M.B.E. for his

D. H. Bolton
work on operational performance of radar and control equipment used for the air defence of Great Britain.
K. H. Kreuchen, O.B.E., D.Phil., F.Inst.P., appointed managing director of the newly formed EMI-Varian Lid., Hayes, Middlesex, studied physics, chemistry and mathematics at the universities of Kiel and Heidelberg. He started his career as a physicist at what is now the Max Planck Institute at Heidelberg. Five years later he joined the Development Laboratory of the Tube Factory of Siemens and Halske at Berlin-Siemenstadi. After the war, he was asked to come to England where he worked first on a government contract with S.T.C. In 1948 Dr. Kreuchen joined the staff of the Research Laboratories of EMI Limited, and specialized in research and development work on high-power velocity-modulated tubes, particularly klystrons. He has latterly been general manager of the Power Tube Division of EMI Electronics Lid.

Walter Marshall, B.Sc., Ph.D., who is 37, is appointed by the U.K. Atomic Energy Authority director of the Research Group (which includes the Culham Laboratory as well as Harwell). He will continue to be director of the Atomic Energy Research Establishment, Harwell. Dr. Marshall took his B.Sc. in mathematical physics at Birmingham in 1952, and his Ph.D. in 1954. He joined the Atomic Energy Research Establishment at Harwell in that year and from 1957 to 1959 spent two years in the United States at Berkeley and Harvard before returning to Harwell. In 1960 he was appointed head of the Theoretical Physics Division at Harwell, and in 1964 was made a member of the research group management board. In March 1966, Dr. Marshall was appointed deputy director of the A.E.R.E., Harwell, and a year later received the additional appointment of deputy director of the Research Group. He has been director of A.E.R.E., Harwell, since April 1968.

Michael Wadely, D.F.H., M.I.E.E., who has been development manager of Newmark Instruments since November 1966, has become chief engineer of the Control Engineering Division. He was with G.E.C. (Electronics) Lid, at their Applied Electronics Laboratory, Stanmore, as a project leader for 10 years. For the last three years with G.E.C. he was manufacturing manager of the Stanmore and Hemel Hempstead facilities. Mr. Wadely was educated at Brighton College and at Faraday House Electrical Engineering College, London.

M. Wadely

The new managing director of Veeder-Root Lid., the counter and pump computer manufacturers of New Addington, Croydon, is Lawrence Dilger, B.Sc., M.I.E.E. He succeeds B. E. Harry who is returning to the U.S.A. to take up the position of vice-president international with the parent company in Hartford, Connecticut. Mr. Dilger has been with Veeder-Root for five years, having joined them as technical manager from Honeywell Controls. The company has also announced the appointment of $\mathbf{E}$. S. Ashford, M.I.E.E., as technical manager. Mr. Ashford joined the company ten years ago as chief designer from E.M.I. Electronics Ltd. In his new capacity he will be responsible for $\mathrm{R} \& \mathrm{D}$ and design at New Addington.
R. W. Merrick, who has completed 41 years with Wright \& Weaire Ltd and the Ferrograph Company Lid, of which he was a founder in 1949, is retiring from active participation in the commercial affairs of Ferrograph, bur continues as a member of the board. He will continue to serve as an executive director of the Ferrograph subsidiary, Rendar Ltd. S. G. Griffiths has been appointed director of commercial affairs in succession to Mr. Merrick. Mr. Griffiths has been on the staff of Electric and Musical Industries Lid for 23 years, during the last five of which he has held the position of sales manager with responsibility for product planning and for worldwide marketing of professional tape recorders and associated equipment.
F. H. Townsend, a Londoner who has been in N. America since 1957, has been appointed manager, Electronic Tube Division of Canadian Westinghouse Co. Lid. I'rior to joining Canadian Westinghouse, Mr. Townsend served as manager, entertainment equipment sales, for the Westinghouse Electric Corporation, Electronic Tube Division. Mr. Townsend, who is 57, started his career with Cossors in 1931 where he remained in the research department until 1938 when be joined the vacuum laboratory of Pye. From 1946 until he went to the U.S.A. Mr. Townsend was chief vacuum engineer and manager of Cathodeon.

John Lockyer, chief designer, British Radio Corporation (Thorn Group), recently retired after 22 years service with the company. He started his career as an apprentice mechanical engineer in 1925 with Western Electric, which later became International Telephone and Telegraph. In 1931 he joined the B.B.C. to work on equipment for installation in the new Broadcasting House and later transferred to the Research Department as head draughtsman. Leaving the B.B.C. in 1946, Mr. Lockyer joined the Ferguson Radio Corporation at Enfield as chief mechanical designer.

Kenneth F. Gibson, B.Sc., has been appointed managing director of Computing Devices Company Lid, London. Mr. Gibson, aged 33 and a graduate of Queen's University, Belfast, joined Computing Devices of Canada Lid., Ottawa, the London company's parent organization, seven years ago. He became supervisor of the aerophysics department in 1964; manager of space sciences division 1965; and director, research and technology marketing just over a year ago.

Christopher R. Robinson, B.Sc., M.Sc., who is 38, has become chief engineer of Computing Devices Company Lid., London, following the recent death of Adrian Duguid. Mr. Robinson took his B.Sc. in electrical engineering at Nottingham University and an M.Sc. at the University of Tennessee. He later lectured in electrical engineering at the Ohio State University before returning to England in 1960 to join Hawker Siddeley Engineering Lid. After this he was a design engineer with Bendix Electronics Lid. In 1967 Mr. Robinson joined Computing Devices of Canada Lid, Ottawa, and has there been engaged on the planning of avionics products.

Peter Iddon, who has been with Multicore Solders L.td for more than ten years, has been appointed U.K. sales manager, consequent upon the resignation of G. A. Jarvis.

# Wireless World Colour Television Receiver 

## 13. Chrominance circuit adjustments

Before dealing with the adjustment of the chrominance circuits, it is necessary to complete the description of the colourdifference amplifiers and some other matters which lack of space prevented inclusion in last month's article. The circuit of


Fig. 1. Circuit diagram of the output stages of the colour-difference video amplifiers and black-level clamps.

Fig. 1 shows the colour-difference output stages. The grids of the three pentodes are connected through the resistors $R_{111}$, $R_{112}$ and $R_{113}$ to $P_{35}, P_{36}$ and $P_{37}$ on the main chrominance board. These three resistors are connected directly between the three pins of the main board and the pentode grid terminals of the valveholders and are shown dotted in the circuit diagram of Part 12.

The valves used are type PCL84 triode-pentodes; the pentode sections are used as the video amplifiers and the triode sections as black-level clamps. All three stages are identical and are self-biased by cathode resistors, $R_{1179} R_{118}$ and $R_{19}$; the by-pass capacitors $C_{68}, C_{69}$ and $C_{70}$, have values which give compensation for the effect of shunt capacitance on the anode loads.

Each pentode anode is connected to a triode anode through a capacitor and each triode anode in turn is connected directly to a grid of the colour tube. The triode anode loads are very high, $8.2 \mathrm{M} \Omega$ and the triodes are normally non-conductive. During line flyback, however, a $50-\mathrm{V}$ positive-going pulse from the line timebase is applied to each grid and makes each triode conduct. Because of the high anode load the voltage drop between anode and cathode becomes quite small, with the result that the anode potential drops to but little more than the cathode potential, which is set by the voltage divider, $R_{129}, R_{130}$ and $R_{\text {III }}$.

Because of this the coupling capacitors between the pentode and triode anodes are brought to a fixed charge once per line. The result is thus the same as if the conventional d.c. restorers were used on a normal signal. They cannot be used here, however, because the sync pulses, which normally control a d.c. restorer, are gated out of the signal at an early stage. Control has to be effected by pulses from the timebase, therefore.

The three valveholders are carried by a small metal panel measuring $3 \frac{1}{2} \times 2$ inches. The pentode bias resistors and by-pass capacitors are connected directly between the appropriate tags of these holders and the panel.

A second panel of Veroboard measuring $3 \frac{1}{2} \times 2 \frac{1}{2}$ inches is screwed to the metal panel with an overlap of $\frac{5}{8}$ inch, and on this are mounted the other resistors and capacitors as shown in the photographs of Fig. S. Three 2 B.A. clearance holes are drilled through both panels and the composite panel is screwed to the top of the framework holding the other boards. It is convenient to tap the holes in the framework, since nuts would be rather inaccessible. Spacers are needed to stand off the board from the frame and these can conveniently be a pair of 0 B.A. full nuts.

Fig. 2 shows the interconnections between the two main boards. Notice particularly that the connection between $P_{6}$ and $P_{26}$ is made by a $0.0022 \mu \mathrm{~F}$ capacitor.

Coil-winding details are given in the table, and a second table gives typical no-signal voltages.



Fig. 3. Details of the delay-line mounting board are given here, viewed from the rear. This is for the original model of the Mullard delay line.

## COIL WINDING DETAILS

| Coil | Turns | Winding | Frequency (MHz) | $\begin{aligned} & \mathrm{Lmin}_{(\mu \mathrm{H})} \end{aligned}$ | $L_{(\mu \mathrm{max}}$ | $\begin{aligned} & \text { Rdc } \\ & (S) \end{aligned}$ | Core |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: | :---: |
| L, | 60 | single layer | 4.43 | 11 | 29 | 2.35 | short |
| $L_{2}$ | 120 | scramble | - | 52 | 133 | 4.6 | long |
| $L_{3}$ | 55 | single-layer | 4.43 | 9.25 | 25.8 | 1.6 | long |
| $L_{4}$ | 1700 | scramble |  | 17.000 | 70.000 | 90 | Ferroxcube |
| $\mathrm{L}_{5}$ | 250 | scramble |  | 204 | 475 | 10.2 | long |
| $L_{6}$ | 70 | scramble | 4.43 | 15 | 40 | 2.8 | long |
| L, | 90 | scramble | 6 | 24.2 | 65 | 3.1 | short |
| $L_{4}$ | 30 | single-layer | 4.43 | 2.8 | 13.1 | 0.85 | long |
| L. Lio | 120 | scramble | 4.43 | 57.5 | 139 | 5 | short |

Except for $L_{4}$. all coil formers are Neosid type 722/1 with cans 7100. and terminal bases 5027. The long cores are Neosid $4 \times 0.5 \times 12.7$ and the shor cores Neosid $4 \times 0.5 \times 6 / 900$. For $L_{4}$ an Aladdin former is used of $\frac{1}{}$-inch diameter and 2 -inches long with a can $\frac{1}{2}$ inch square by $2_{k}^{3}$-inch long. All coils which are scramble-wound have cheeks fitted $t$-inch apart. All coils are wound with No. 42 gauge wire, which can be enamel or enamel-silk covered. The core of $L_{4}$ is Ferroxcube FX1068, wrapped with Sellotape to be an easy fit in the former


Fig. 4. This drawing shows the details of the board for the current Mullard-type DL1E delay line. With this line $T_{7}$ is not required and $R_{72}$ and $R_{95}$ should be changed to 100 ohms.

| Stage | Base | Emitter | Collector | Stage | Anode | Cathode |
| :---: | :---: | :---: | :---: | :---: | :---: | :---: |
|  | $\begin{aligned} & 0.65 \\ & 1.05 \\ & 0.45 \\ & 0.6 \\ & 2.7 \\ & 3.5 \\ & 2.4 \\ & 4 \\ & 2.2 \\ & 5.2 \\ & 0 \\ & 0 \\ & 0 \\ & 0 \\ & 0 \end{aligned}$ | 0 0.7 0.5 0.2 2.1 2.95 2.7 4 1.6 4.6 0 0 -0.65 -0.6 -0.65 | 12.9 <br> 14.1 <br> 14.25 <br> 8.6 <br> 11.6 <br> 11.6 <br> 13.2 <br> 13.3 <br> 1.3 <br> 12.5 <br> 5.5 <br> 5.5 <br> 15 <br> 17.6 <br> 13.5 | $\begin{aligned} & D_{1} \\ & D_{2} \\ & D_{3} \\ & D_{4} \\ & D_{3} \\ & D_{6} \\ & D_{3} \\ & D_{8} \end{aligned}$ | $\begin{gathered} -10 \\ -6.1 \\ 0.7 \\ 0 \\ 0 \\ 4 \\ 0 \\ 2.4 \end{gathered}$ | $\begin{gathered} 0 \\ 0.7 \\ 8 \\ 10.9 \\ 3.9 \\ 6.7 \\ 5.3 \\ 2.4 \end{gathered}$ |

Fig. 3 shows an under view of the board which carries the delay line and its connections. The delay line includes tuned circuits which are factory adjusted and should not be touched. There are in existence two types of line which can be distinguished with an ohmmeter. The connecting tags are in two groups of three and in the original pattern of line the outer pair of each three must be joined together, as shown in Fig. 3. An ohmmeter test between the tags of each pair before they are joined will show an open circuit. In the later model the test will show an internal connection between these tags. They must not then be joined together, but the connections shown in Fig. 4 must be adopted. This newer model, the Mullard type DL1E, has built-in auto-transformers at each end instead of plain coils. As a result, a push-pull output can be obtained directly from it and $T_{7}$ of Part 12 should not be used with it. At the input two different impedance levels are available. The higher impedance input provides a greater output and if this should be needed it is necessary to change $R_{T_{2}}$ to 390 ohms. However, normally the lower impedance is suitable and $R_{7}$ and $R_{98}$ should be each 100 ohms instead of the 150 ohms needed for the earlier model.

There are a good many adjustments needed in the chrominance circuits but nothing very complicated in the way of
apparatus is needed. A signal generator and an oscilloscope will do most things. It is advisable to use an isolating mains transformer, not merely to protect oneself, but to protect the test equipment. In addition a $0.002-\mu \mathrm{F}$ capacitor should be in series with the signal generator output.

The procedure is as follows:

1. Apply the output of the signal generator between the decoder input terminal, $P_{1}$, and chassis.
2. Set the saturation control $R_{f 0}$ to maximum.
3. Short-circuit $D_{8}$ (to render the colour-killer inoperative) and $R_{30}$ (to render the local oscillator inoperative).
4. Connect the oscilloscope to the base of $\operatorname{Tr}_{10}$.
5. With an input at 6 MHz tune $L_{7}$ for minimum output.
6. With an input of 4.43 MHz tune $L_{6}$ for maximum output.
7. Remove short-circuit from $D_{8}$ leaving that to $D_{30}$ in place.
8. Disconnect the inter-unit lead from $P_{3}$.
9. Join $P_{3}$ to the junction of $R_{48}$ and $R_{49}$ and also connect it to the chassis through 0.01 F .
10. Connect the oscilloscope to the cathode of $D_{1}$.
11. With an input of 4.43 MHz tune $L_{1}$ for maximum output.
12. Replace the connections altered under (8) and (9) to normal.
13. Connect the signal generator across $C_{9}$ and the oscilloscope


## across $R_{\text {\% }}$.

14. At 4.43 MHz adjust $L_{9}$ for minimum output.
15. Connect the signal generator across $C_{61}$ and the oscilloscope across $R_{\text {g }}$.
16. At 4.43 MHz adjust $L_{10}$ for minimum output.
17. Disconnect the signal generator and oscilloscope.
18. Connect the oscilloscope between $P_{6}$ and chassis.
19. Remove the short-circuit from $R_{30}$.
20. Adjust $L_{3}$ for maximum output which should be about 5.4 V p-p.
21. If possible, examine the waveform and if necessary readjust $L_{3}$ to make it more nearly sinusoidal. This will usually entail screwing in the slug a little. An output of 5 V p-p of good waveform should be obtainable.
22. Connect the oscilloscope to $C_{61}$.
23. Adjust $L_{8}$ for minimum output.
24. Connect the oscilloscope to $P_{6}$ and chassis, and take a separate lead from $P_{6}$ to the 'external sync' terminal of the oscilloscope.
25 . Use a $1-\mu \mathrm{s}$ sweep range and carefully lock the oscilloscope to the wave. Adjust the X -shift so that the top of a half cycle is exactly on a vertical line of the oscilloscope graticule.
25. Connect the oscilloscope to the junction of $R_{90}$ and $C_{579}$ but leave the 'external sync' terminal still joined to $P_{6}$.
26. Adjust $C_{5}$ so that the graticule line, which previously coincided with the top of a half cycle, now coincides with a zero of the sine wave. If this cannot be reached with $C_{5}$ at maximum, add $C_{56}$ of perhaps 20 pF . (Note. If a double-beam oscilloscope is available and it has the same phase shift in both channels, the two inputs can be connected simultaneously to $P_{6}$ and across $T_{6}$. Then $C_{57}$ can be adjusted for $90^{\circ}$ phase angle between the two traces.)
27. Restore all connections to normal.
28. Tune in a signal and lock line and field timebases to it. With saturation at minimum adjust for a good black and white picture. Adjust the tuning from a position of poor picture detail to one which is just short of the setting at which sound-channel interference appears.
29. Connect the 'external sync' terminal of the oscilloscope to a convenient point on the line timebase (a wire within a few inches of the line output valve will usually give enough pick-up).
30. Connect the oscilloscope input to $P_{1}$ and check that there is a colour burst on the waveform. If not, readjust the tuning, which may be critical.
31. Disconnect the lead from $P_{3}$ and connect the oscilloscope to $P_{3}$.
32. Adjust the X -shift to centre the colour burst on a vertical line of the graticule.
33. Connect the oscilloscope to $P_{25}$.
34. The trace should be a damped sinewave of perhaps three or four noticeable cycles. Adjust $L_{s}$ so that the first positive half cycle is centred on the vertical line of the graticule on which the colour burst was previously aligned. (Note. If a doublebeam oscilloscope is available connect it to display the burst on one trace and the damped sinewave on the other.) The amplitude of the first positive half cycle should be about 3.5 V .
35. Replace all connections to normal.
36. Set $R_{19}$ and $R_{2 g}$ at a little below maximum.
37. Remove the link between $P_{4}$ and $P_{5}$.
38. Short-circuit $D_{8}$.
39. Connect Model 8 Avometer on $25-\mathrm{V}$ range between chassis and the collector of $\operatorname{Tr}_{4}$ (i.e., $P_{4}$ ).
40. Adjust $R_{\vartheta}$ and $R_{r}$ so that the meter reads 7 V , and so that by adjustment of $R_{2}$ only the voltage can be varied from nearly zero to 12 V . This fixes the setting of $R_{\mathfrak{y}}$. Then set to 7 V by $R_{2 z}$
41. Turn up saturation. Horizontal colour bars should appear. Adjust for a moderate intensity of colour.
42. Adjust $L_{2}$ for a colour lock if possible; if not for the
slowest movement of the bars.
43. Replace the link between $P_{24}$ and $P_{25}$.
44. Adjust $R_{2 x}$ for a colour lock. This means that the horizontal bars will disappear and that the colour will be properly distributed over the picture. The colours, however, may be the wrong ones, but at this stage do not worry about this.
45. Adjust $R_{4}$ so that the setting of $R_{2 z}$ for a colour lock is not too critical.
46. Remove the short-circuit from $D_{8}$. If the colour killer is operating correctly this should have no effect.
47. Connect the oscilloscope across $R_{ \pm 4}$. An approximate sinewave of 7.8 kHz should appear. Adjust $L_{4}$ for the best sinewave. 49. Readjust the tuning. It will now be critical for colour. With quite small mistuning all colour should disappear, but at the proper setting not only should traces of colour appear but the reference oscillator should lock-in without any other adjustment.
48. Adjust saturation for a reasonable depth of colour. Avoid turning it up too much for this will produce colour streaking.
49. Examine the actual colours obtained. Test Card F is best for this. On this the background should be a pale blue and the girl should have a red dress with brown hair and the doll should be green. If the colours are wrong or nearly all wrong, transfer the lead to $P_{24}$ to $P_{23}$, thus changing the phase of the bistable. All colours should now be substantially correct, but may not be precisely right. Thus, reds should be red, greens green, and blues blue, but some may be too vivid and others too pale, while other colours, which are a mixture of these may have considerable errors of hue.
50. The controls $R_{98}, R_{106}$ and $R_{108}$ have now to be adjusted to put this right. The $R-Y$ channel gain is fixed, but the relative gain of the other two is adjustable as is also the matrixing of the $\mathrm{G}-\mathrm{Y}$ channel by $R_{98}$. Fortunately, these controls are not very critical. Adjustments are initially best carried out on the colour bar test pattern which is usually broadcast several times a day during the trade test transmissions. There is little that can be said about these adjustments beyond saying that they are done a little at a time until all colours look right.
53 . Since the delay line has not yet been brought into use the receiver is operating in the simple PAL mode. Under conditions of good reception it should give a good colour picture which at normal viewing distance may satisfy many people. Its main defect will be that in close viewing (how close depends on individual eyesight) alternate lines in a large area of colour may be of slightly different shades and the lines appear to move vertically. This is because in simple PAL the integration of successive lines is performed by the eye, and the eye cannot do this when it is too near the picture.
54 . With the receiver tuned to a signal so that the reference oscillator remains locked, connect up the delay line. Disconnect the lead to $P_{12}$ and disconnect the lead from $P_{6}$. Connect $P_{6}$ to $P_{12}$ through $10 \mathrm{k} \Omega$.
51. Disconnect the links $P_{29}$ to $P_{30}$ and $P_{31}$ to $P_{32}$.
52. Connect the oscilloscope to $P_{31}$. It will display the $4.43-\mathrm{MHz}$ output from the reference oscillator. Adjust $R_{75}$ for a minium. If no minimum setting can be found, transfer the oscilloscope to $P_{29}$. If there is now a definite minimum setting for $R_{\text {r }}$, reverse the leads to one end of the delay line. There should now be a definite minimum setting with the oscilloscope connected to $P_{3}$.
53. Ideally the minimum output should be zero. In practice, it is not. If it is not very small indeed, however, compared with the output at $P_{29}$, try adding capacitance across $R_{76}$ or $R_{\pi}$, across one there will be a phase lead and across the other a phase lag. Values of from $25-100 \mathrm{pF}$ should be tried.
54. Replace connections to normal and check on a picture. The crawling-line effect on areas of solid colour should now have disappeared. If it has not, slight readjustment of $R_{7}$ should make it do so.

This completes the adjustments to the chrominance circuits. The list appears to be a very formidable one, but in actual fact the adjustments are not at all difficult to carry out. No serious difficulty is likely to arise unless there is some gross defect. Unfortunately, the symptoms of a fault in the colour circuits can be very different from what one is inclined superficially to expect. Thus, for example, suppose that there is some defect which renders the $\mathrm{B}-\mathrm{Y}$ channel inoperative. One's first reaction is to expect that there will be no blue in the picture, but this is quite wrong. There will be too much blue! It is important to remember that this is a colour difference channel. For a fully-saturated blue signal, the $\mathrm{B}-\mathrm{Y}$ channel carries a signal of which the Y component is supposed to cancel the Y signal applied to the cathode and leave the B signal to operate the gun. However, if there is no signal at all applied to the blue grid there is still the Y signal applied to the cathode and this will operate the blue gun to produce blue.

The quickest way of checking in such cases is, of course, to use the oscilloscope to make sure that signals are in fact being applied to each grid of the tube. However, if it is necessary to diagnose from the symptoms the waveforms of Fig. 5, Part 10 will be found very helpful.

From this it can be seen, for instance, that on a blue signal the $Y$ signal is quite small and that the $R-Y$ and $G-Y$ signals are equal and opposite so that they cancel out to give no total signal on the red and green guns; the $B-Y$ signal is large, but its complete absence leaves the small $Y$ signal on the blue gun.

If the $R-Y$ channel were to fail, then with the same blue signal the cancelling signal on the red grid would be absent and the Y signal on the cathode would operate the red gun when it should be inoperative. The net result would be to give the blue a magenta cast.

It is possible to adopt this procedure in diagnosing colour troubles when the signal is the colour-bar test pattern for the colours are then known ones and include pure red, green and blue. It is almost impossible to do so on a general picture
where the precise colours are unknown and where pure primary colours are fairly rare.

In the development quite a number of colour faults were found and some of them through inexperience took quite a time to trace. In the end, however, they all proved to be simple electrical faults. Some, like reversed connections to a transformer winding or to the delay line, were a little puzzling at first. One which had devastating effects on the colours was a failure in the $G-Y$ channel. This was localized quickly enough for there was full h.t. voltage on the pentode anode, indicating that it was taking no current. A further check showed it to have no $g_{2}$ voltage and the problem then was, why? This took some time to find for the fault was a very rare one, an invisible break in a copper strip on the Veroboard! Once found, a touch with the soldering iron put matters right.

It may seem a statement of the obvious to point out that in order to obtain a colour picture one must have the proper chrominance input to the decoder, including the colour burst. This depends upon the bandwidth of the i.f. amplifier and they will not be obtained if this is insufficient.

In monochrome inadequate bandwidth does no more than reduce the horizontal definition and can pass unnoticed by the uncritical. In colour it may reduce the amplitude of the burst so much that a colour lock is difficult or impossible to obtain, but traces of colour and, in particular, horizontal colour bars, may still be evident. The chrominance signals are transmitted vestigial sideband below the sub-carrier in frequency. The higher modulation-frequency components of the chrominance signal may thus be within the i.f. pass-band even if the sub-carrier frequency itself is just outside it.

It is the normal current practice to make the $-6-\mathrm{dB}$ points of the i.f. amplifier 39.5 MHz and 35 MHz ; the burst comes at 35.17 MHz and so is attenuated only slightly less than 6 dB . As transmitted, the peak-to-peak amplitude of the burst is the same as that of a sync pulse. At the detector output of the receiver it will rarely be greater than one-half of this. It does

not take much misalignment of the i.f. amplifier to reduce the colour burst to a level which is inadequate for locking the reference oscillator properly.

Mistuning the receiver one way brings the vision carrier below 39.5 MHz , the upper modulation frequencies are cut-off, the definition becomes poor and, as the colour burst is cut-off, there is no colour. Mistuning the other way brings the vision carrier above 39.5 MHz , the upper modulation-frequency response is improved but a strong interference pattern from the sound channel occurs.

It might be thought that a bandwidth at 6 dB of 4.5 MHz is rather small when the transmitted bandwidth is 5.5 MHz . In practice, however, the results are good. It is not impossible to obtain a 5.5 MHz bandwidth but it is very difficult to do so and obtain the drop in response of at least 30 dB on a further 0.5 MHz change of frequency, which is necessary for soundchannel rejection. A bandwidth of 5 MHz is more practicable but even then the cut-off needed for proper sound-channel rejection is hard to obtain.

## Transient response

In television it is not so much the frequency response which is important as the transient response, and what is really required is a very short rise time without overshoot. A flat frequency response with a sharp cut-off, which is inevitable if the bandwidth is large, may give short rise time, but it inevitably produces overshoot. It is desirable for the response to fall off gradually towards and beyond the edge of the passband and so the edge is usually taken as the $6-\mathrm{dB}$ point.

The nearer this point is to the sound channel the more likely it is that objectionable overshoot will occur and the more difficult it is to secure adequate rejection of the sound channel.

There are two matters involved in deciding just where to place the cut-off point. One is performance and the other is cost. Current practice places it at 35 MHz and this is certainly the lowest practicable bandwidth and it is cheapest. To place it at 34 MHz would certainly greatly increase the cost of the i.f. amplifier and might make it too difficult to adjust and keep in adjustment. A limit at 34.5 MHz is certainly practicable but it is still a moot point as to whether it is desirable. The basic definition would certainly be improved; there would probably be more overshoot but it is not thought that this would be serious. However, the increased amplitude of the chrominance components around 4.43 MHz would certainly increase colour patterning effects and the net result might well be worse.

So much work has been involved in the development of this equipment that it has not been possible to explore all of the finer points of design. As a result we do not know just what is the optimum bandwidth when little regard is paid to cost. We have no doubt that for a monochrome transmission it should be at least 5 MHz but we are very doubtful whether with a colour transmission the increase of patterning would not more than offset the improvement in definition.

It is a very fortunate circumstance that colour improves the apparent definition and this in spite of the fact that the colour signals themselves are transmitted in a very narrow bandwidth and the true definition is produced by a monochrome signal, the Y signal. The reason is, of course, that the change between adjacent objects in the picture is not merely one of light and shade, as in monochrome, but of colour as well. This becomes obvious when it is remembered that two objects which are adjacent and of different colours are readily distinguished in a colour picture even when they are of precisely the same luminance, whereas in monochrome reproduction they could not then be distinguished at all whatever the bandwidth

In conclusion, we should mention that there has been a change in the A.B. Metal Products tuner. It is basically the same as the earlier model referred to in Part 7, but it no longer


The decoder section opened out and showing the PAL delay line.
has the printed-circuit board shown in Fig. 2, Part 8. Certain resistors are now mounted internally and have different values; also the case is now connected to the negative of the supply instead of being isolated from it.

In the i.f. board $R_{32}$ must be changed to $590 \Omega(120 \Omega+$ $470 \Omega$ ) and $R_{33}=0$. On the tuner itself $R^{\prime \prime}$ between the positive and negative supply terminals remains unchanged at $2.2 \mathrm{k} \Omega$. The other resistor $\left(R^{1}=470 \Omega\right)$ is now fitted internally and has the value of $1 \mathrm{k} \Omega$.

The chassis of the tuner will be at -20 V to all other chassis in the equipment and must be appropriately insulated. The aerial feeder can be connected as before through $0.001-\mu \mathrm{F}$ capacitors shunted by $1-\mathrm{M} \Omega$ resistors. The outer of the cable connecting the tuner to the i.f. board, however, must not be connected directly to the tuner case, but through $0.001 \mu \mathrm{~F}$. The coupling capacitor $C^{1}$, Fig. 2, Part 8, is still required and can be connected to the tuner case.

There is no longer an emitter connection of the mixer externally accessible to which a signal generator can be connected for alignment. The cover of the tuner is easily removable, however, by bending up two metal tags, one at each end of the cover. The mixer is at the shaft end and the emitter is joined to a $1-\mathrm{k} \Omega$ resistor shunted by 150 pF and is reasonably accessible.

This article concludes the series on the Wireless World colour television receiver. It is intended to reprint the whole series in booklet form and an announcement will be made when supplies are available.

# Test Your Knowledge 

Series devised by L. Ibbotson,* B.Sc., A.Inst.P., M.I.E.E., M.I.E.R.E.

## 13. Frequency Modulation

1. A sinusoidal carrier has an unmodulated frequency of 90 MHz . A particular modulating signal causes the carrier frequency to vary between 89.99 and 90.01 MHz 1000 times per second. If the amplitude of the modulating signal is doubled
(a) the carrier frequency will still vary between 89.99 and 90.01 MHz 1000 times per second
(b) The carrier frequency will vary between 89.99 and 90.01 Mhz 2000 times per second
(c) the carrier frequency will vary between 89.98 and $90.02 \mathrm{MHz} \quad 1000$ times per second
(d) the carrier frequency will vary between 89.98 and 90.02 MHz 2000 times $/ \mathrm{sec}$.
2. A sinusoidal carrier is frequently modulated in turn by two signals of the same amplitude, one having a frequency of 100 Hz , the other 1000 Hz . The amplitude of the phase variation of the carrier is
(a) zero in both cases
(b) the same for both signals
(c) larger for the lower frequency signal
(d) larger for the higher frequency signal.
3. A frequency modulated transmitter is radiating a modulated carrier, the modulation index being 2 radians. The amplitude of the modulating signal is doubled. As a result the total power radiated
(a) remains unchanged
(b) is doubled
(c) increases by $50 \%$
(d) increases by a factor of $\sqrt{ } 2$.
4. The amplitude of the carrier frequency component of the spectrum of a frequency modulated carrier is always
(a) the same as the amplitude of the unmodulated carrier
(b) less than the amplitude of the unmodulated carrier
(c) greater than the amplitude of the unmodulated carrier
(d) zero.
5. The spectrum of a carrier, frequency modulated with wide deviation by a single sinusoid, contains many side-frequency components. The number of components with significant amplitudes (assuming maximum deviation) is (a) the same whatever the modulating frequency

[^3](b) smaller the higher the modulating frequency
(c) larger the higher the modulating frequency
(d) greatest when the modulating frequency is equal to the square root of the deviation.
6. The carrier frequency of a f.m. signal may be increased either by multiplication or heterodyning. The result is
(a) no change in the frequency deviation in either case
(b) an increase in the frequency deviation in both cases
(c) an increase in the frequency deviation when multiplication is used; no increase when heterodyning is used
(d) an increase in the frequency deviation when heterodyning is used; no increase when multiplication is used.
7. The Armstrong method of generating a f.m. signal is based upon the generation of a pair of amplitude modulation sidebands (using a balanced mixer) and the subsequent addition of a carrier frequency signal lagging by $/ 2$ radians on the phase which the a.m. carrier would have had. The basic signal so produced is effectively
(a) frequency modulated with a wide frequency deviation
(b) f.m. with a narrow frequency deviation
(c) phase modulated with a large phase deviation
(d) phase modulated with a small phase deviation.
8. It is possible for a f.m. radio set to receive two transmissions within the bandwidth of its r.f. stage and, provided the amplitude of the unmodulated carrier of the stronger is at least twice that of the weaker, only respond to the stronger signal with negligible interference from the weaker. This effect can only occur if
(a) the maximum modulation index of the stronger signal is at least several radians at the highest modulating frequency
(b) the modulation index of the weaker signal is not greater than 0.5 radian at the lowest modulating frequency
(c) the two carriers are not closer together than the sum of the highest modulating frequencies of both
(d) the r.f. tuned circuit cuts off most of one sideband of the undesired signal.
9. The B.B.C. f.m. broadcasting system uses a maximum frequency deviation of 75 kHz and transmits an audio bandwidth of 15 kHz . The
i.f. bandwidth of a receiver should be at least
(a) 30 kHz
(b) 90 kHz
(c) 105 kHz
(d) 180 kHz .
10. If the i.f. bandwidth of a f.m. receiver is much narrower than it should be the main effect is
(a) removal of the higher audio frequencies from the output signal
(b) non-linear distortion in the output signal
(c) a large increase in the noise output from the receiver
(d) a reduction in the interference rejection effect.
11. Communications f.m. systems generally use a much narrower r.f. bandwidth than that required by the B.B.C. broadcast system; restriction of the a.f. bandwidth allows a much smaller maximum frequency deviation to be used. In addition to allowing more channels in a given frequency band, the result is that for a given transmitter power
(a) the service range is increased
(b) the output signal to noise ratio is improved
(c) the interference between stations broadcasting on adjacent channels is reduced
(d) the receiver i.f. gain required is less.
12. Many f.m. receivers have a stage at the end of the i.f. amplifier which "limits" the amplitude of the signal by cutting off the top and bottom of the waveform (those which do not have this stage use a demodulating circuit which incorporates limiting action). The purpose of limiting is
(a) to prevent the demodulator from being overloaded
(b) to provide a simple a.g.c. action
(c) to remove amplitude variations due to noise
(d) to improve the demodulator action by supplying it with a square waveform.
13. If we represent the signal presented to the demodulator in a f.m. receiver as:
$V \sin \left[w_{d}+(t)\right]$, the demodulator must produce an output voltage which is
(a) directly proportional to $\phi(t)$
(b) inversely proportional to $\alpha(t)$
(c) directly proportional to $d \phi(t) / d t$
(d) inversely proportional to $d o(t) / d t$
14. Following the demodulator in a receiver for the B.B.C. f.m. broadcasts is a circuit which consists of a resistor and capacitor arranged as a potential divider, the output being taken across the capacitor. The time constant of this circuit is specified as $50 \mu \mathrm{~s}$. Its purpose is
(a) to correct for frequency distortion which all f.m. demodulators introduce into the audio signal
(b) to correct for frequency distortion deliberately introduced into the audio signal at the transmitter
(c) to attenuate the higher audio frequencies because the receiver output stages cannot handle them
(d) to filter out any remaining carrierfrequency component in the output signal.
Answers and comments, page 295.

## A Transistor Multiplier Circuit

## A multiplier circuit and how it may be employed for modulation, mixing, detecting, a.g.c. and a.a.c. A circuit for a high-performance audio signal generator is described.

by A. F. Newell, M.I.E.R.E.

Many electronic circuits are basically nultipliers; some examples are detectors, requency changers, modulators, square aw voltmeters and analogue computer nultipliers. The physical realization of the nultiplication function can take many forms anging from a simple non-linear element uch as a diode, to the fairly complex :ircuits used in analogue computers. In ome circuits there is only one pair of input erminals, and the output consists of many :omponents besides the product of the nputs. While in other circuits separate erminals are available for each input, and he output is the product of the two inputs.
In this article a circuit will be described in which separate terminals are available for he inputs, and in which the output can be ither :

$$
k_{1} A+k_{2} A B
$$

re:

## $k A B$

there $A$ and $B$ are the two inputs and the $k$ s re constants which depend on circuit alues. Several examples will be given to -how how the circuit may be used to 'erform different functions.

## 3asic circuir

he basic circuit, Fig. I, consists of a longailed pair, the emitter current of which is upplied by a simple amplifier.
The linearity of the multiplier will of ourse be determined by the linearity of the

two amplifiers. The linearity of $T r_{3}$ is determined mainly by the ratio of the constant resistor $R_{3}$, and the varying emitter resistance of the transistor, which is approximately:

$$
r_{e}=25 / I_{E}\left(I_{E} \text { in } \mathrm{mA}\right)
$$

Now:

$$
I_{E}=V_{E} / R_{3}
$$

therefore:

$$
R_{3} / r_{e}=V_{E} / 25 \text { with } V_{E} \text { in } \mathrm{mV}
$$

This shows that if $V_{E}$ is large compared with 25 mV then the total emitter resistance is nearly constant, and the linearity is good. But at low emitter current where $V_{E}$ becomes comparable with 25 mV the linearity becomes poor. In practice this means that if the input $V_{2}$ is a.c. then it is possible to restrict the signal to the linear part of the amplifier characteristic. But if the input is d.c., additional circuitry will be required to linearize the characteristic.

To determine the linearity of the longtailed pair, a simplifying assumption will be made. This is that the relationship between the base-emitter voltage and emitter current of the two transistors is given by the diode equation:

$$
I=I_{o}[\exp (q V / K T)-1\}
$$

This is a good approximation provided that $r_{b} / h_{f e}$ is small, which is usually the case for a transistor with a high gain working at


Fig. 2. The test circuit employed.
(Right) Fig. 3. Characteristics of the longtailed pair.
currents of a few milliamperes or less.
It is easy to select transistors which most nearly satisfy this requirement by using the circuit of Fig. 2. If the relationship holds, then, when the emitter current is switched by a factor of ten, the change in $V_{B R}$ should be the same whether the switch is from $10 \mu \mathrm{~A}$ to $100 \mu \mathrm{~A}$, or from $100 \mu \mathrm{~A}$ to 1 mA .
Assuming that:

$$
I_{E}=I_{E B S}[\exp \cdot(q V / K T)-1]
$$

then:

$$
\begin{aligned}
V_{B E} & =(K T / q) \log _{e}\left(I_{E} / I_{E B S}\right) \ldots \\
V_{1} & =V_{B E_{1}}-V_{B E_{2}} \text { for } I_{E} \gg I_{E B S}
\end{aligned}
$$

and :

$$
=0.025 \log _{e}\left(I_{E_{1}} / I_{E_{2}}\right)
$$

From this equation the curve of $I_{E_{1}}$ and $I_{E_{8}}$ against $V_{1}$ can be drawn (Fig. 3). It can be seen that between $\pm 10$ and $\pm 15 \mathrm{mV}$ the relationship has good linearity, but beyond these points it is increasingly non-linear.
It is now possible to see how the circuit acts as a multiplier. From Fig. 3 the relationship between $I_{E_{1}}$ and the total emitter current $I_{E}$ over the linear part of the curve is:

$$
I_{E_{1}}=\frac{I_{E}}{2}\left(1+\frac{V_{1}}{V_{1} \max }\right)
$$

where $V_{1_{\text {max }}}$ is the voltage for $I_{E_{1}}=I_{E}$.


Now $V_{1 \text { max }}=50 \mathrm{mV}=1 / 20$ of a volt which makes:

$$
\begin{align*}
I_{E_{1}} & =\frac{I_{E}}{2}\left(1+20 V_{1}\right) \\
& =\frac{I_{E}}{2}+10 V_{1} I_{E} \tag{1}
\end{align*}
$$

similarly:

$$
\begin{equation*}
I_{E_{2}}=\frac{I_{E}}{2}-10 V_{1} I_{E} \tag{2}
\end{equation*}
$$

and:

$$
\begin{equation*}
I_{E_{1}}-I_{E_{2}}=20 V_{1} I_{E} \tag{3}
\end{equation*}
$$

but:

$$
\begin{align*}
I_{E} & \approx \frac{V_{2}}{R_{3}} \\
\therefore \quad I_{E_{1}} & \approx \frac{V_{2}}{2 R_{3}}+\frac{10 V_{1} V_{2}}{R_{3}} .  \tag{4}\\
I_{E_{2}} & \approx \frac{V_{2}}{2 R_{3}}-\frac{10 V_{1} V_{2}}{R_{3}} .  \tag{5}\\
I_{E_{1}-I_{E_{2}}} & \approx 20 \frac{V_{1} V_{2}}{R_{3}} \tag{6}
\end{align*}
$$

If the output is taken across $R_{1}$ :

$$
\begin{equation*}
V_{\text {out }} \approx \frac{R_{1}}{2 R_{3}} V_{2}+\frac{10 R_{1}}{R_{3}} V_{1} V_{2} \tag{7}
\end{equation*}
$$

If the output is taken across $R_{2}$ :

$$
\begin{equation*}
V_{\text {out }} \approx \frac{R_{2}}{2 R_{3}} V_{2}-\frac{10 R_{2}}{R_{3}} V_{1} V_{2} \tag{8}
\end{equation*}
$$

If the output is taken between the collectors, assuming that $R_{1}=R_{2}$, then:

$$
\begin{equation*}
V_{o u t} \approx \frac{20 R_{1}}{R_{3}} V_{1} V_{2} \tag{9}
\end{equation*}
$$

The graph of Fig. 3 was checked experimentally (at $I_{E_{1}}+I_{E_{2}}=1 \mathrm{~mA}$ ) with transistors selected using the circuit of Fig. 2, and confirmed within the limits of measurement accuracy.

## Temperature dependence

Equations I to 9 and Fig. 3 are based on the assumption that $K T=25 \mathrm{mV}$ which is correct for $17^{\circ} \mathrm{C}\left(=290^{\circ} \mathrm{K}\right)$. The temperature coefficient of $V_{1}$ in the region of $17^{\circ} \mathrm{C}$ is $1 / 290=0.00345$. In some circuits it may be desirable to compensate for this by using a resistance between the bases, which has a similar temperature coefficient.

## Zero drift due to differential power dissipation

If the long-tailed pair is unbalanced (as will happen, for example, if the input is d.c.) then there will be a difference in power dissipation between the two transistors which will result in unequal junction temperatures.

To minimize this effect the thermal resistance between the transistors, and the dissipation in them, should be as small as possible.

For a given mean dissipation, the differential dissipation can be minimized by designing the circuit so that the mean collector to emitter voltage is equal to the mean voltage across the collector resistor. In this case an unbalance in collector currents will reduce the dissipation in both transistors by the same amount.

## Frequency dependence

The linearity of Fig. 3 for $V$, between about $\pm 15 \mathrm{mV}$ depends on the $h_{f e}$ of the transistor being so large that the base resistance (internal and external) can be neglected. The cut off frequency of $h_{f e}$ is approximately $f_{1} / h_{f e}$, and at frequencies above this distortion may become apparent. Also the impedance presented by the long-tailed pair at the base terminals will decrease and cease to be resistive at frequencies of the order of $f_{1} / h_{f e}$ and above. However with high frequency transistors the circuit should be usable up to several MHz .

## Modulation

Amplitude modulation is a process whereby the amplitude of a carrier is made to vary in
accordance with the modulating signal.
Consider the case of a carrier ( $V_{c} \sin \omega_{c} t$ ) applied between the bases of $T r_{1}$ and $T r_{2}$ in Fig. I, and a modulating signal:

$$
\left(V_{d c}+V_{m} \sin \omega_{m} t\right)
$$

applied to the base of $T r_{3}$ : then from, equation (7):

$$
\begin{align*}
& V_{3}=\frac{R_{1} V_{d c}}{2 R_{3}}+\frac{R_{1} V_{m}}{2 R_{3}} \sin \omega_{m} t+ \\
& \quad+\frac{10 R_{1} V_{d c} V_{c}}{R_{3}} \sin \omega_{c} t+ \\
& \quad+\frac{10 R_{1} V_{m} V_{c}}{R_{3}} \sin \omega_{m} t \sin \omega_{c} t \\
& =\frac{R_{1} V_{d c}}{2 R_{3}}+\frac{R_{1} V_{m}}{2 R_{3}} \sin \omega_{m} t+ \\
& +\frac{10 R_{1} V_{d c} V_{c}}{R_{3}} \sin \omega_{c} t+\frac{5 R_{1} V_{m} V_{c}}{R_{3}} \times \\
& \times\left[\cos \left(\omega_{r}-\omega_{m}\right) t-\cos \left(\omega_{c}+\omega_{m}\right) t\right] \tag{10}
\end{align*}
$$

The output $V_{3}$ thus consists of a d.c. component, a component at modulation frequency, the carrier and the upper and lower sidebands. A simple $C R$ coupling can be used to eliminate the d.c. and modulation-frequency components, provided that there is a sufficient difference between carrier and modulation frequency.

The output $V_{4}$ is the same as $V_{3}$ except that the polarity of the carrier and the sidebands is reversed. $V_{5}$ which is the difference between $V_{3}$ and $V_{4}$ is therefore:

$$
\begin{aligned}
V_{5} & =\frac{20 R_{1} V_{d c} V_{c}}{R_{3}} \sin \omega_{c} t+\frac{10 R_{1} V_{m} V_{c}}{R_{3}} \times \\
& \times\left[\cos \left(\omega_{c}-\omega_{m}\right) t-\cos \left(\omega_{c} t+\omega_{m}\right) t\right]
\end{aligned}
$$

i.e. just the carrier and the two sidebands.

It is sometimes necessary to suppress the carrier leaving only the two sidebands, one of which may then be filtered out to give single-sideband transmission. A method of achieving carrier suppression is shown


Fig. 4. Modulator with suppression of carrier and modulation frequencies.

Fig. 5. Circuit to give up to $100 \%$ modulation.


Fig. 6. Output of Fig. 5 versus modulating waveform.


Fig. 7. Square law voltmeter.
schematically in Fig. 4. Provided that the collector current of $\mathrm{Tr}_{8}$ is the same as the d.c. component of $\operatorname{Tr}_{3}$ current, then the carrier frequency component due to $T r_{1}$ and $T r_{2}$ is cancelled by that of $T r_{1}$ and $T r_{3}$. The sideband components appear only in the output of $\operatorname{Tr}_{1}$ and $T r_{2}$ and are therefore not cancelled. By having a small unbalance in d.c. currents in $T r_{3}$ and $T r_{\text {f }}$ it is possible to leave a small component of carrier frequency, which may sometimes be required.

The curve of Fig. 3 shows that good linearity is obtained up to about $\pm 15 \mathrm{mV}$, and the carrier input should be restricted to this value if the following circuits are simple amplifiers. However if the amplifiers are tuned so that harmonics will be rejected, a larger input is permissible.

As stated earlier the linearity of a simple amplifier, such as $\operatorname{Tr}_{3}$ in Fig. 1, is quite good provided that the maximum input signal does not cause the emitter current to approach zero. This means that it is suitable for modulation depths up to, say, $80 \%$. But if good linearity is required with modulation depths of near $100 \%$ then a circuit such as Fig. 5 should be used. A current feedback pair, $\operatorname{Tr}_{3}$ and $T r_{4}$, is used in place of $T r_{3}$ in Fig. 1. The current amplification of the circuit is quite accurately given by $\left(R_{3}+R_{4}\right) / R_{3}$, provided that the actual gain is not too large.

The biasing network of $T r_{1}$ and $T r_{2}$ is arranged so that the preset resistor $R_{11}$ can be used to balance the long-tailed pair. The carrier voltage developed across the bases of $T r_{1}$ and $T r_{2}$ is

$$
\left(R_{i}+R_{8}\right) /\left(R_{6}+R_{7}+R_{8}\right)
$$

times the input. The value of $R_{7}+R_{B}$ should be small if the assumption of an exponential relationship between the baseemitter voltage and the emitter currents is to be a good approximation.

A circuit was constructed using the values


Fig. 8. An analogue multiplier.
shown in Fig. 5, and with BCIO7 transistors. Fig. 6 shows the output gaveform (between the collectors) with nearly $100 \%$ modulation, and with the modulation waveform applied to the X input, to check linearity.

## Detectors and mixers

The use of the multiplier circuit as a detector or mixer is similar to its use as a modulator, and therefore need not be considered at length.

By applying the signal to one input and an oscillation of carrier frequency to the other, the circuit can be used as a synchrodyne, homodyne or single-sideband detector.

## Square law voltmeter

Multiplier circuits can be used to give the square, cube or higher power of an input. A practical application would be an a.c. voltmeter with an indication proportional to the square of the input. Such a voltmeter is useful because it indicates the true r.m.s. value regardless of waveform; also a doubling of the reading corresponds to a change of 3 dB .

Fig. 7 shows one form of circuit. It has the advantage of simplicity; but since the long-tailed pair operates with a standing current, and the f.s.d. of the meter can only be a fraction of this, there may be difficulty in maintaining a stable zero. Also unless the meter is very sensitive, it may have a comparatively small ratio of (peak)/(r.m.s.) before distortion occurs. A high ratio is desirable if the voltmeter is used to measure noise, or other "peaky" waveforms.

Since the main drawback of the circuit of Fig. 7 is due to the standing current, a better alternative would be to effectively rectify the input to give the modulus. In this case no standing current is required.

## Analogue multiplier, reciprocal and divider circuits

With analogue circuits it is usually desirable that all inputs should be referred to the same zero level. Fig. 8 shows how this may be done, in the case of the multiplier circuit. The diodes $D_{1}$ and $D_{2}$ compensate for the base-emitter voltages of the transistors $\mathrm{Tr}_{3}$ and $T r_{3}$, so that with the input voltages at zero the emitter current of $\operatorname{Tr}_{4}$ is zero and the emitter current of $\mathrm{Tr}_{6}$ is that required to balance the long-tailed pair. The use of current feedback pairs ensures good linearity.

The linearity of the analogue multiplier circuit is determined almost entirely by the characteristic of the long-tailed pair (see Fig. 3). The two input amplifiers use considerable amounts of negative feedback and are thus very linear.
With the circuit values shown in Fig. 8, the maximum departure from linearity was about $3 \%$ (corresponding to $V_{1}=15 \mathrm{mV}$ ). It would be possible to improve on this by restricting $V_{1}$ to a lower value. Another method, using feedback is shown schematically in Fig. 9. An additional long-tailed pair is used to provide negative feedback. The characteristics of the long-tailed pairs are the same, so that the non-linearity caused by the feedback tends to cancel the nonlinearity of the multiplier.

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The quotient $A / B$ may be obtained by multiplying together $A$ and $1 / B$. A circuit for obtaining an output proportional to the reciprocal of an input is shown at the left of Fig. 10, this together with the multiplier circuit at the right of the figure forms a divider circuit.

The recciprocal circuit consists of a multiplier circuit, ${T r_{1,2,3} \text { and } 8 \text {, a feedback }}^{\text {a }}$ amplifier, $T r_{4}$ and ${ }_{5}$, and constant current sources $\operatorname{Tr}_{6}$ and 7 . The tendency of the constant current source $T r_{7}$ to unbalance the collector voltages of $\mathrm{Tr}_{1}$ and $\mathrm{Tr}_{2}$ will be compensated by the feedback circuit; this will result in the collector voltages being nearly in balance, and a voltage between the bases to give:

$$
I_{c_{2}}-I_{c_{1}}=I_{c_{7}}
$$

It has already been shown (Fig. 3) that, over the range of about $\pm 15 \mathrm{mV}$, the voltage between the bases is related to the collector currents by the expression:

$$
\frac{I_{c_{1}}-I_{c_{2}}}{I_{c_{1}}+I_{c_{2}}} \propto V_{1}
$$

But $I_{e_{1}}-I_{c_{2}}$ in Fig. 10 is a constant and $I_{e_{1}}+I_{c_{2}}$ is proportional to the input, therefore $V_{1}$ is proportional to the reciprocal of the input.

The characteristics of Fig. 3 show that as the divisor input in Fig. 10 is reduced the voltage $V_{1}$ will depart from the relationship above, and the more the input is reduced the greater will be the discrepancy. However this non-linearity is exactly that required to cancel the non-linearity of the multiplier $T r_{9}$ and $T r_{10}$. So the permissible minimum value of divisor input is fixed by limiting in $T r_{8}$ and $T r_{10}$ rather than by non-linearity in $V_{1}$. It is of course not possible to obtain useful results with the divisor input near zero, as the reciprocal of zero is infinity.

The relationship between divisor input
and $V_{o}$ was checked for inputs between I and 10 V (at intervals of 1 V ), it was not possible to detect any departure from the relationship $V_{0} \propto 1 / V_{i n}$. The input was then reduced to 0.4 V , the departure from the correct relationship was then about $1 \%$. At an input of 0.2 V the discrepancy was about $2 \%$, no further reduction in input was possible because of limiting in $\mathrm{Tr}_{9}$, $\operatorname{Tr}_{10}$.

## Automatic amplitude control and automatic gain control

The controls a.a.c. and a.g.c. are virtually the same thing; in both cases the gain of an amplifier is controlled. In a.a.c. the amplifier is part of an oscillator. The gain is controlled so that the amplifier is linear and a constant amplitude output is obtained, without the distortion that would result from limiting on a nonlinear part of the characteristic. On the other hand a.g.c. is used to keep the output of an amplifier approximately constant for a changing input, or to make the output change in proportion to the logarithm of the input.

Fig. II shows schematically how a.a.c. and constant output a.g.c. may be achieved. For low inputs where $V_{0}$ is less than $V_{d} T r_{2}$ is cut off, and the full gain is available. When the rectified voltage across $C_{2}$ approaches $V_{d}$ current starts to flow in $T r_{2}$ thus reducing the gain in proportion to the reduction of current in $\mathrm{Tr}_{1}$.

By eliminating the delay voltage (connecting the anode of $D_{2}$ to the base of $T r_{1}$ ) and compensating for the diode voltages, the output can be made approximately proportional to the logarithm of the input.

## Wien network signal generator with

 a.a.c.With $R C$ oscillators some form of amplitude control is virtually essential as the effective


Fig. 9. Adding negative feedback to the multiplier circuit.
maximum phase shift of $90^{\circ}$ in the modulating frequency and a single time constant smoothing circuit will cause a maximum shift of another $90^{\circ}$. But these shifts will occur at zero gain, so that it would seem that squegging would be avoided. However at high frequencies there are stray impedances, which are not shown in the circuit diagram, and these may provide sufficient extra phase shift to cause the $180^{\circ}$, unity gain condition to be met.

One way of curing the squegging is to switch to a low value of $C_{4}$ on the highest
range. This will still give good smoothing of the oscillator frequency, but the phase shift of the possible modulating frequencies will be sufficiently low to prevent squegging.

The circuit of Fig. I2 has been kept simple, as its purpose is to show how the multiplier can be used to provide automatic amplitude control. However additional facilities may easily be provided. For example, by placing a resistor in the collector circuit of $\mathrm{Tr}_{4}$ a constant amplitude output may be obtained, which may be used to synchronize an oscilloscope or feed a
frequency meter. A square wave may be obtained by feeding a limiter or trigger circuit from the collector of $T r_{6}$, as a constant load at this point will not affect the amplitude stability. An antiphase output may be obtained by feeding a currentfeedback pair from the emitter of $T_{7}$

## Reference

1. W. A. Edson "Intermittent Behaviour in Oscillators", Bell System Technical Fournal, Vol. 24, No. 1, Jan. 1945.


Fig. 10. An analogue divider circuit.


Fig. II. Automatic gain control.


Fig. 13. Amplifier to reduce effect of rectifier ripple in Fig. rI.


Fig. 12. Wien network signal generator with a.a.c.

## Letter from America

When commenting on last year's I.E.E.E. Show in New York I questioned whether the handful of British exhibitors was really representative of Britain's electronics capability. This year (Mar. 24-27) there were 31 British exhibitors-a big improvement.

As usual the Show spread over four floors in the Coliseum Building although the total floor space was $4 \%$ down on the 1968 Show. More important was the absence of some of the larger firms like Raytheon, Philco and the semiconductor companies. The number of exhibitors was 720 minus 1 (which I will explain later). Probably the most significant development (at least I thought so) was the enormous increase in automated test systems. As Abraham Bluestone, sales manager of Teradyne, put it "While the number of leads on a device has grown linearly, the number of tests has grown exponentiallv. The diode, first semiconductor, has two leads and requires about four tests. The transistor with its three leads requires about nine or ten tests. After transistors, the industry started making i.cs and now large arrays with many, many leads and the number of tests that have to be performed have grown enormously. A human operator could not perform them all quickly and efficiently."

Automated i.c. test systems were shown by many companies. The Microdyne automatic i.c. tester is quite compact measuring some 19 in by 20 in deep and only 7 in high. When the instrument is set up the operator merely inserts the i.c. devices and watches pass or reject lamps. A third lamp gives an indication if proper connections are not being made. This go-no-go instrument will test d.t.l., h.n.i.1., m.e.c.l., r.t.1. and t.t.l. logic, gates, flip-flops, binary counters, etc. Programming is performed by a plug-in matrix card and it is stated that
upwards of 5,000 devices can be tested in a day. The Model 1000 test system made by AAI is much more complex featuring computer operation with built-in analogue-todigital convertor, testing with a.c., d.c., pulse, r.f. and thermal conditions. It can test all kinds of microcircuits, thin or thick film devices, analogue, linear and non-linear logic devices. Provision is made for a data logging option which allows the operator to arrange test results under programme control and $\log$ them on a teletypewriter. Modular construction is used and the test rate is quoted as 180 double limit tests per second. Another tape-programmed i.c. tester is Aviens Model 2400 which comes in the form of a fairly large console. All tests and measurements are on Mylar tape 82 -bits wide and it is claimed that 3000 i.cs can be tested per day. Performance can be tested, measured, displayed and recorded under a wide range of conditions. Failures can be analysed in detail and data logging can be made of each measurement or switched to record failures only.

General Radio had an automatic capacitor bridge which selects range, balances capacitance and loss simultaneously, generates coded digital output data and displays the measured values on illuminated indicators -all in half a second or so! This is Model 1680 and the useful range is 1 pF to $1000 \mu \mathrm{~F}$. Accuracy is quoted as $0.1 \%$ and the 1680 can also measure parallel conductance from 1 nanomho to 1 mho.

How about the other test equipmentoscilloscopes, generators, meters-and the computers? Well, it would probably take more than one complete issue of Wireless World to do justice to the vast array of equipment displayed so I will mention just a few of those I found interesting. For exam-

ple, Wavetek had several unusual instruments on show-all well styled with an eye to function. Model 141 is a voltage controlled generator which can provide sine, square or triangular waveforms from 0.5 Hz to 5 MHz . External frequency control is possible over a $1000-1$ range and there is an audio sweep option to cover the range from 20 Hz to 20 kHz . Overall accuracy is very high and the output is 10 volts peak-topeak into 50 ohms. Model 710 is a Dialomatic Herzmeter and this instrument measures frequency from 5 Hz to 100 MHz with an accuracy of $0.1 \%$. It combines the resolution of a digital device with differential voltmeter circuitry and crystal control. Exact Electronics were showing what they claimed to be the smallest multiple waveform generator on the market. This was Model 100 and it measures just under $7 \frac{1}{2}$ in by 3 in by $8 \frac{1}{2}$ in and has a continuously variable frequency range from 0.001 Hz to 3 MHz . It features a choice of nine different waveforms and is very moderately priced at $\$ 445$ ( $(145)$. I liked the new Krohn-Hite variable bandpass filter unit which has independently controlled low and high cut-off frequencies.
Telephone facsimile transmitters have been available for some time and there is now a wide choice of equipment. Among those shown was the Dex I made by Graphic Sciences. It is an attractively styled machine and it can transmit photographs, letters, documents, etc., up to 11 in by 8 in via any telephone. Transmission time is six minutes. No electrical connection is made to the telephone lines-coupling is purely acoustical. I was quite impressed with the clarity and definition obtained with the Dex I ( 88 lines per inch). Printing is non-contact and no chemicals are used.
CSI had an 'Acoustic Data Coupler' which is another device for use with a telephone. This one is intended for computer links and only frequencies in the $1-2 \mathrm{kHz}$ range are used.

Colour TV cameras and equipment were well in evidence. Sony were demonstrating a two-tube camera which employs what is called a 'Colour dissector optical system' to separate luminance and chrominance components. Also being demonstrated were TV sets using the controversial 'Trinitron' tube which has three beams and a single gun with a common eleciron lens system. A pair of electron 'prisms' give colour convergence. Also shown were Trinitron systems combined with an 'Aperture Grille' which is said to give twice the brightness of conventional sha-dow-mask tubes. I understand Panosonic were showing their new flat television receiver, which uses an electroluminescent image display system, but unfortunately I missed this exhibit.

One stand that did intrigue me had the splendid title of "The Orient International (USA) Inc.". This turned out to be a tailor's business and here two cheerful Chinese gentlemen could be seen busily measuring up diffident but smiling engineers for Hong Kong suits! I understand the stand had to close down the next day as the organizers had misunderstood the precise business of Orient International (USA) Inc.; hence my reference earlier to 720 minus 1 stands! I only hope they made enough to pay the expenses!
G. W. Tillett

## New Products

## Uni-junction Transistor

A low-voltage device for pulse triggering voltage and current sensing circuits, tuning circuits, flipflops and pulse timers has been announced by Motorola. It is a silicon uni-junction transistor type 2N5431 which is constructed by the surface-passivated, diffused annular process giving high uniformity and improved characteristics. Peak point current is only $0.4 \mu \mathrm{~A}$ at a $V_{B 2 B 1}$ of 25 V and $4 \mu \mathrm{~A}$ at 4 V , critical parameters in long-time-delay, low leakage circuits. The very low emitter leakage current of 10 nA is claimed by the makers to be 100 times better than cube-alloy uni-junctions. Maximum emitter voltage is 30 V , maximum emitter current 50 mA r.m.s., power dissipation 300 mW , and maximum emitter saturation voltage 3 V . The 2 N 5431 is hermetically sealed in a TO-18 case. Motorola Semiconductors Lid., York House, Wemuley, Middlesex.
WW 328 for further details

## Double-beam Oscilloscope with Signal-delay

Philips PM3231, marketed by Pye Unicam, is a double-beam oscilloscope employing signal-delay lines on both inputs. It is a d.c. to 15 MHz generalpurpose instrument but is specially suitable for the pulse measurements required when checking lowand medium-speed computers and desk calculators. The vertical amplifier's sensitivities are adjustable from $10 \mathrm{mV} / \mathrm{div}$ using $1: 2: 5$-sequence switches with continuous adjustment between settings by vernier controls. Sensitivity can be extended to $1 \mathrm{mV} / \mathrm{div}$ via a $\times 10$ switch but on this setting the bandwidth is reduced to 5 MHz . Measurement accuracy on all ranges is $3 \%$. The inputs are protected against overloads up to 500 V d.c., and d.c. drift is $0.5 \mathrm{div} / 24$ hours. Triggering can be either automatic or continuously variable level triggering. Sweep speeds cover $0.2 \mu \mathrm{~s} /$ div to

$0.5 \mathrm{~s} /$ div with continuous adjustment of selting Sweep can be expanded up to five times. The input selector switch features a "0" position which earths the Y amplifier input enabling the d.c. reference level to be found without disconnecting the probe. Pye Unicam Lid., York Street, Cambridge.
WW 313 for further details

## Coaxial Attenuator Kit

A versatile attenuator kit available in both 75 and $50 \Omega$ impedance has been introduced by Greenpar Engineering of Harlow. The kit comprises seven attenuators of $1,2,3,6,10,14$ and 20 dB . These are made with " $T$ " rod and disc networks designed to accept Greenpar inter-series adaptors allowing the user to fit

the required coaxial interfaces. A male and female series " $N$ " interface is supplied with the kit and when this is used in conjunction with the attenuators the specification is as follows: Frequency range d.c. to 4 GHz ; resistance tolerance $\pm 1 \%$ or 0.1 dB (whichever is least); v.s.w.r. less than 1.05 at 1 GHz ( 1.2 at 4 GHz ); maximum power $1 W$ continuous. Price of the $50-\Omega$ version (GE83500) or the $75-\Omega$ version (GE83700) is $£ 48.3 \mathrm{~s}(\mathbb{4 8 . 1 5 )}$. Greenpar Engineering Lid., Station Works, Harlow, Essex.
WW 338 for further details

## Aero-band Monitor

A crystal-controlled monitor, model 60SS, for a.m. 25 or 50 kHz channelling on frequencies between 118 and 156 MHz is announced by Park Air Electronics. Six-channel capability is provided with dual-gate f.e.ts for r.f. amplifier and mixer circuits, and linear i.cs for the i.f. amplifier. Each circuit function occupies a separate printed circuit sub-assembly, interconnected by plug and socket. Single-frequency conversion is employed and the i.f. is the standard 10.7 MHz . Sensitivity at 130 MHz is $2 \mu \mathrm{~V}$ for 2 W audio output power, and signal-to-noise ratio with $2 \mu \mathrm{~V}$ input is $>15 \mathrm{~dB}$. Rejection at 50 kHz (adjacent channel) is -80 dB . Suitable 3rd overtone crystals are supplied with the equipment, each crystal being individually trimmed to frequency. Frequency stability is $0.003 \%$ in the temperature range $-10^{\circ}$ to $+50^{\circ} \mathrm{C}$.


Details of a.g.c. performance state that for a change of input from $2 \mu N$ to 200 mV it will produce a change of output not greater than 3 dB with reference to 1 W . Operation is from a.c. mains $100-115 \mathrm{~V}$ and $200-250 \mathrm{~V}$. Size is $407 \times 305 \times$ 178 mm . A number of optional extras are available including interchangeable block filters for changing channel spacing. Park Air Electronics Ltd., Red Lion Square, Stamford, Lincs.
WW 315 for further details

## Conductive Tapes

Two new pressure-sensitive tapes introduced by the 3 M Company are claimed to provide low-cost shielding against electromagnetic and r.f. interference. These two additions to the range of Scotch electrical tapes are type X-1181, a copper foilbacked tape and type X-1170, which is aluminium foil-backed. Both employ an electrically conductive adhesive which allows the tapes to be, what the makers call "three-dimensionally conductive", with no corrosive reaction between the adhesive and the material to which the tape is applied. Conductivity and adhesion is said to remain good in conditions of high ambient temperature and humidity. 3M Company, Wigmore Street, London W. 1 .

WW 318 for further details

## Switch without Contact Bounce

A push-type switch incorporating a t.t.l. flip-flop was shown at the recent Paris components exhibition by SECME. The switch, which provides a true and a complementary output, has two modes of operation: asynchronous or synchronous. In the asynchronous mode the equipment operates when the button is pushed and released. In the synchronous mode the equipment switches on at the first clock pulse after the button is pressed and switches off on the clock pulse following the button's release. Société d'Etudes et de Construction de Matériel Electronique, 13 bis, rue des Envierges, Boite Postale 26, Paris 20e.
WW 335 for further details

## S.S.B. Communications Receiver

Model LSR8-B by Labgear is a single sideband a.m./c.w. receiver which provides instant sideband selection on eight crystal-controlled channels within the $2-20 \mathrm{MHz}$ band. Normally operated from a $100-240 \mathrm{~V}$ a.c. mains supply, the receiver can be powered from a 12 V battery; the changeover from mains to battery in the event of mains

failure is automatic. Any aerial with a 75 Stransmission line may be employed with the receiver or a long wire in conjunction with an aerial tuning unir. A socket is provided for the connection of headphones or an external loudspeaker. When this facility is in use the internal loudspeaker is muted. A second socket terminated at $600 \Omega$ allows an a.f. signal to be fed to external equipment such as an amplifier or teleprinter. Price $\ell 190$. Labgear Lid, Cromwell Road, Cambridge.
WW 301 for further details

## Portable Colour V.T.R.

A portable colour video tape recorder developed by the Victor Company of Japan will be available for export later this year. In the U.S.A. it will cost $\$ 2000$. The technique employed is called d.f.c (direct and f.m. combined) system and, although the recorder is designed to accept N.T.S.C. colour signals, the system can be applied to any broadcasting standards. When recording, the video signal is divided into two bands of low and high frequencies. The l.f. component is frequency modulated and the f.m. signal is then combined with the h.f. component and recorded on the tape. On playback, the f.m. signal is demodulated and added to the h.f. component to reproduce the original signal. By adopting this method the makers

claim to make the bandwidth $50 \%$ wider than a normal v.t.r. Tape width is 12.7 mm and its length 915 m . Speed is $240 \mathrm{~mm} / \mathrm{s}$. Two video heads are used and horizontal resolution is 350 lines for black and white; 250 lines for colour. The recorder measures $480 \times 480 \times 250 \mathrm{~mm}$ and weighs 25 kg . Victor Company of Japan Ltd., 12,3-chome, Moriyacho, Kanagawa-ku, Yokohama, 221, Japan.
WW 332 for further details

## Transducer Scanners

Low-level transducer scanner modules designed specifically for data logging and alarm scanning applications have been announced by IDM Electronics, of Reading. Costing from $\mathcal{\beta 2 5}$, three

models in the range are 25 -, 50 -, and 100 -channel units each with three alternative rates of scanning provided by an internal clock. Flexibility of design allows the connection of different types of equipment. Use with an existing digital voltmeter provides multi-channel measurement and the addition of a printer will give complete data logging facilities. A visual indication of the channel being sampled is provided by neon number tubes and a b.c.d. output is supplied for printout purposes. Internally generated thermal e.m.fs are less than $1 \mu \mathrm{~V}$ in normal operating conditions. All of the modules are self-contained and mainsoperated. The 25 - and 50 -channel units are 133 mm high and 241 mm wide; the 100 -channel unit is 482 mm wide. IDM Electronics Ltd., Arkwright Road, Berkshire, RG2 0LH.
WW 311 for further details

## Solid-state Relays

Solid-state relays that can operate at frequencies up to several hundred MHz using photon coupling are announced by Mullard. They can be used in a range of applications varying from simple on/off switches to r.f. modulators and demodulators. Complete electrical isolation exists between input and output stages thus allowing the devices to be used as coupling elements between circuits at different voltage levels but still allowing the transfer of d.c. signals. Each relay comprises a gallium arsenide diode and photo-transistor or photo-diode inside the same encapsulation. When a forward current flows through the gallium arsenide diode, it emits infrared radiation that applies a bias to the other diode or transistor so that current in the g.a. diode controls the conducting state of the output diode. Unlike mechanical relays, the output is proportional to the input making the photorelays suitable for use as noiseless automatic or manual volume controls. The transfer ratio (input current to output current) is typically 10:1. Rise and fall times for the output current are 1 ns. The two semiconductors in a relay are linked only by the infrared radiation: the voltage breakdown rating can be as high as 20 kV between input and output stages. Mullard Ltd., Torrington Place, London W.C.1.
WW 303 for further details

## P.C. Edge Connectors

Connectors for printed circuit boards with contacts pitched at 3.96 mm are announced by Ultra Electronics. The type of construction enables any length of connector to be specified by the circuit designer within the range 5-62 contacts per side, and the contacts can be single-sided or doublesided as required. Phosphor-bronze contacts are gold-plated and set in diallyl-phthalate mouldings which are claimed to provide high physical and dielectric strength. High conductivity is obtained at low contact pressure. The new series, type 5124, is offered with a full range of ancillaries including nylon or metal mounting clips, terminations for solder and solderless connections and polarizing and reference keys. Ultra Electronics (Components) Ltd., 419 Bridport Road, Greenford, Middlesex.
WW 307 for further details

## Advance Timebase Module

A sweep delay plug-in for their OS2000 and OS2100 oscilloscopes has been introduced by Advance Electronics. When used with either of these normal sweep, variable delay sweep or gated delay sweep modes of operation can be selected. Twin timebases and special triggering characteristics are featured. Timebase A has 19 calibrated sweep speeds from $200 \mathrm{~ms} / \mathrm{cm}$ to $0 . \mu \mathrm{s} / \mathrm{cm}$ and a continuously variable $3: 1$ fine control which provides the sweep for normal and "A intensified by B" modes of operation. It is also used together with

a 10 -turn calibrated potentiometer to provide the delay of $0.2 \mu \mathrm{~s}$ to 2 s . Timebase B , with 18 calibrated sweep speeds from $100 \mathrm{~ms} / \mathrm{cm}$ to $0.2 \mu \mathrm{~s} / \mathrm{cm}$ provides the sweep in the delay mode. The gate and ramp waveforms from timebases A and B are available at sockets on the front panel. A $\times 5$ magnifier expands the sweep length to effectively five screen diameters and provides a maximum sweep speed of $40 \mathrm{~ns} / \mathrm{cm}$. Advance Electronics Ltd., Roebuck Road, Hainault, Essex.
WW 327 for further details

## Fibre-Optic Vidicon

E.E.V. has introduced a new vidicon camera tube with a fibre-optic faceplate. Essentially the same as the EEV type P831 ruggedized vidicon, which has separate mesh construction, magnetic deflection and focusing; the P831F has a 25 mm diameter faceplate constructed from 9 -micron diameter fibres. When used with a 7735B type photosurface and 10.8lux illumination on the faceplate, a signal current of at least $0.15 \mu \mathrm{~A}$ is

attainable with the target voltage set to produce $0.02 \mu \mathrm{~A}$ dark current. This new fibre-optic vidicon is ideal for applications involving coupling to other devices having fibre-optic window outputs, such as image intensifiers. By using fibre-optic windows on both devices and coupling them together in direct optical contact, the optical efficiency can be improved by as much as 50 times compared with a normal lens system. Finglish Electric Valve Co. Ltd., Chelmsford, Essex.
WW 319 for further details

## Lightweight Accelerometers

Miniature piezo-electric accelerometers for vibration and shock measurements have been introduced by Environmental Equipments Lid. Measuring 11 mm in diameter and 9.5 mm high the accelerometers weigh 4.5 g and have a charge sensitivity of $3.5 \mathrm{pC} / \mathrm{g}$. The two basic types in the
range are designed for adhesive mounting, or fixing by means of an integral mounting stud. All models in the range have a flat response from 0.05 Hz to 12 kHz , a resonant frequency of 60 kHz , and an operating temperature range of $-75^{\circ}$ to $+250^{\circ} \mathrm{C}$. These devices are constructed from either stainless steel or titanium and the use of adhesives is avoided in the crystal assembly to prevent problems at high temperature. Environmental Equipments Ltd., Denton Road, Wokingham, Berkshire.
WW 337 for further details

## Power Supply for Valve Circuits

While most solid-state power supplies described in these columns are designed to power semiconductor circuits, Hewlett-Packard has brought out a new power supply unit which, although in itself is solid-state, its purpose is to power valve circuits. The new unit, model 712 C , provides a variable output 0 to +500 V d.c., 200 mA max.; a fixed output of -300 V d.c., 50 mA max.; a variable bias output of 0 to -150 V d.c., 5 mA max.; and a heater supply output of 6.3 V a.c. centre-tapped,


10A max. The output voltage changes less than $0.1 \%+5 \mathrm{mV}$ with a change from no load to full load and the transient recovery time is such that the output returns to within 25 mV of the selected voltage within $50 \mu$ s of the step change from no load to full load or vice versa. Dimensions: $16 \times$ $42 \times 33 \mathrm{~mm}$. Weight: 10 kg . Price: $\{240$. HewlettPackard Ltd., 224 Bath Road, Slough, Bucks.
WW 322 for further details

## Variable Filter

Barr \& Stroud variable filter consists of two similar active low-pass/high-pass sections which can be used separately and together to give highpass, low-pass, band-pass and band-stop facilities. The low-pass range is in five decades from $0-100 \mathrm{kHz}$ with lowest cut-off at 0.1 Hz . The highpass range is in five decades from $0.1 \mathrm{~Hz}-500 \mathrm{kHz}$ with highest cut-off at 100 kHz . In all modes the pass-band insertion loss of each filter is low and the stop-band attenuation is at least $36 \mathrm{~dB} /$ octave. Critical damping can be switched in for pulse and step waveforms. A narrow band amplifier mode can be selected with a voltage gain of 20 dB . The input impedance is nominally $1 \mathrm{M} \Omega$ in parallel with 30 pF capacitance while the output impedance

is approximately $5 \Omega$ The case measures $320 \times$ $225 \times 245 \mathrm{~mm}$. Barr \& Stroud Limited, Kinnaird House, 1 Pall Mall East, London S.W.1. WW 329 for further details

## I.C. Memory System

A family of $500-600 \mathrm{~ns}$ core memories with all the electronic functions performed by integrated circuits is announced by Honeywell. The new ICM-500 system is designed for use as main or

auxiliary memory within standard or custom digital systems. It has a 600 ns full cycle-time and an access time under 300 ns . Capacities range from 4,096 to 32,768 words. The i.c. replaces a number of discrete transformers and transistors and it performs both current switching and logic functions in the system. In a typical 8,192-word capacity memory of 24 -bit words, 112 flat-packs perform the functions formerly requiring 2,000 discrete components. Honeywell Ltd., Great West Road, Brentford, Middlesex.
WW 309 for further details

## Hall Probe Magnetometer

Model D11 magnetometer by Scientifica \& Cook Electronics is a self-contained instrument with internal cells supplying the power requirements. It has four ranges of $0.1,0.3,1$ and 3 tesla full scale with manual selection by front panel switch. The same switches also provide battery check and polarity reversal. Additional controls are for "zero" and "calibration" with a coaxial socket output for

recorder operation. Supplied with the magnetometer is a calibration magnet and two Hall probes; one for transverse field and the other for axial field measurement. Accuracy is quoted as $\pm 2 \%$. The unit measures $229 \times 152 \times 127 \mathrm{~mm}$ and weighs 1.95 kg . Price 198. Scientifica \& Cook Electronics Ltd., 40-48 High Street, Acton, London W. 3.
WW 314 for further details

## Temperature Controllers

A new range of temperature controllers by SK Instruments combines in one mode the features of three-term control (proportional, reset and rate control) without complications. These controllers employ a form of non-linear proportional mode control which the makers describe as deviation dependent sensitivity or d.d.s. In operation, the correction force derived from deviation is linearly proportional for small values but at the limits of deviation the control loop is de-sensitized logarithmically. This results in a narrow proportional band operating around the control point which,
at large deviations, operates smoothly to an almost infinite proportional band. This overcomes several disadvantages inherent with proportional control. Series-nine controllers are available for operation with resistance thermometers and with thermocouples with integral cold junction compensation. Common mode a.c. rejection is up to 250 V , and series mode up to 50 mA . Operation is from 240 V $50-60 \mathrm{~Hz}$ single phase supply with optional ratings of 8,12 or 24 A . The front panel measures $92 \times$ 92 mm and it contains a scale with a calibration accuracy within $1 \%$. SK Instruments Ltd., Greenhey Place, Gillibrands, Skelmersdale, Lancashire.
WW 325 for further details

## Double-beam Storage Oscilloscope

Featuring double-beam storage facilities the Telequipment oscilloscope, model D53S, costs f495. It offers a choice of three display modes: as a normal oscilloscope; as a long-persistence instrument with a continuously variable persistence of

more than a minute; and as a storage oscilloscope capable of storing traces for periods of up to ten minutes. Variable sweep delay is also provided and a choice of plug-in Y amplifiers is available. Display area is $6 \times 10 \mathrm{~cm}$ and 22 calibrated sweep speeds range from 5 s to $0.5 \mu \mathrm{~s} / \mathrm{cm}$. Telequipment Ltd., 313 Chase Road, Southgate, London N. 14. WW 336 for further details

## Compact D.C. Supply

A power supply measuring only $38 \times 76 \times 50 \mathrm{~mm}$ can provide up to four output rails with a total capability of 30 V at up to 40 mA . It is Adretta's model P1015, initially developed as a stabilized d.c. source to drive this company's tuning fork oscillator/tuning units and now marketed as a product in its own right. Operation can be from $100-125 \mathrm{~V}$ or $200-250 \mathrm{~V} 50-60 \mathrm{~Hz}$ mains supplies without adjustment. Up to four outputs can be provided in series if required, provided that the sum of the output voltages should not exceed 30 V and the current 40 mA . The zero volt connection may be earthed or isolated as required and a second screen may be connected to minimize spurious noise when an isolated supply is required. Prices range from $£ 816 s(\{8.80)$ to $£ 12$ according to quantity. Adretta Letd., Station Approach, Fleet, Hampshire.
WW 302 for further details

## Character-generating C.R.T.

 A 30 mm electostatic character-generating monoscope for use in data display units, in which a c.r.t. is used to provide input and output information for a computer, or for displaying remotely printed information initiated on a typewriter keyboard, is announced by E.M.I. Designated Printicon Tube 9788, it provides up to 64 charac-ters in an $8 \times 8$ array. The number and style of symbols can be changed to meet users' requirements. Principal feature is all-electrostatic operation giving fast access to any character. E.M.I, Electronics Ltd., Hayes, Middlesex.

WW 308 fier further details

## Low Output, High Input Impedance Potentiometer

The limitations of precision potentiometers when circuit designers require low output impedance and high input impedance are met by a new potentiometer introduced by Computer Instruments Corp. which incorporates a solid-state isolation circuit. The low output impedance means that low-impedance devices such as meters and sensitive relays requiring high current levels can be directly driven. Any load from infinity to $1 \mathrm{k} \Omega$, fixed or variable in magnitude up to 30 mA , can be driven by a standard unit. Wiper current is virtually eliminated providing improved noise performance and, with the need for impedance matching removed, the potentiometer can be treated as a simple shaft-to-voltage converter. Standard model 202-30 is available with terminal resistance of $10 \mathrm{k} \Omega$ or $25 \mathrm{k} \Omega$ and maximum output impedance of $0.5 \Omega$. Electrical function angle is $350^{\circ}$. The applied voltage can be from 10 to 30 V d.c. (polarity must be observed) and the permitted power dissipation at $25^{\circ} \mathrm{C}$ is 2 W . Computer Controls Lid., 19 Buckingham Street, London W.C. 2 .

WW 333 for further details

## Transmitter Analyser

A transmitter output analyser, model TG2400 by Green E.C.E. Ltd., features an oscilloscope which displays directly the r.f. modulation envelope at any frequency up to 500 MHz . Absorption load units of $50 \Omega$ and $75 \Omega$ contained in the analyser can handle up to 1 kW mean r.f. power at any frequency between 2 and 500 MHz . The absorption load units are connected to a wattmeter with full scale ranges of $10,30,100,300$ and 1000 W mean, and an accuracy of $5 \%$. Indicators of v.s.w.r. are

included. Single- and two-tone signals are provided for driving the microphone input of a.m. and s.s.b. transmitters. Price $\int_{290}$. Green Electronic and Communication Equipment Lid., 79-91 Braemar Road, London N. 15.
WW 304 for further details

## Shock Accelerometer

A transducer for use in very high $g$ shock applications has been announced by Kistler Instruments. It is the quartz shock accelerometer type 805A which has a resonant frequency of 60 kHz and is suitable for the measurement of shock accelerations up to $100,000 \mathrm{~g}$. Deviation is only $5 \%$ at 12 kHz and the low lower frequency limit allows measurements of long duration shocks to be made. A tri-axial accelerometer (see illustration) comprises three shock accelerometers mounted on a special adaptor with which accelerations up

to $20,000 \mathrm{~g}$ in three axes can be measured. Kistler Instruments Ltd., The Ridges, 2 Clockhouse Road, Farnborough, Hampshire
WW 323 for further details

## I.C. Test Clip

A device comprising a spring-loaded test clip and a "contact comb" has been introduced by Guest Electronics for testing dual-in-line integrated circuits. The comb can be attached to 14 - or 16 -lead packages where it functions as an attachment

guide and prevents the short-circuiting of adjacent leads. The test probe can then be clipped to the comb. The makers claim that this solves oscilloscope probe attachment problems and facilitates testing. Gold-plated contacts are employed and the capacitance effects on h.f. transitions are quoted as negligible. Price $\mathbb{L}^{2} 10 \mathrm{~s}(\mathbb{2} .50)$ each with reductions for quantity. Guest Electronics I.t., Nicholas House, Brigstock Road, Thornton Heath, Surrey, CR 4 7JA.
WW 317 for further details

## Power Frequency Changers

Although the primary purpose of power frequency changers by Valradio is to allow operation of $50-\mathrm{Hz}$ equipment from non-standard frequencies, or for operating $60-\mathrm{Hz}$ equipment from a $50-\mathrm{Hz}$ supply, the range comprises $100-\mathrm{W}$ and $200-\mathrm{W}$

units working from any input voltage and providing a variety of output voltages. The conversion principle is static and noiseless in operation. Frequency stability is claimed to be better than $\pm 1 \%$. The two types available are FCA230/100W at $\quad 32.6 \mathrm{~s} .9 \mathrm{~d}$. ( $\{32.34$ ) and FCB230/200W at $\{52$. Special units providing $400-1000 \mathrm{~Hz}$ for testing marine and aircraft equipment can be supplied to order. Valradio Ltd., Browell's Lane, Feltham, Middx.
WW 331 for further details

## Short-circuit Detector

Rapid location of short-circuits in telephone and signalling cables, distribution wires and power cables is the claim made for the Swiss-made ITT short-circuit detector now available in the U.K. from ITT Electronic Services, of Harlow. The instrument also enables particular cables to be identified from among others, concealed wiring to be traced and the run of cable pairs to be followed even through concrete to a depth of 300 mm . Two separate units are employed: one comprising a probe, amplifier and headphones and the other an oscillator unit generating a fixed frequency at about 1.4 kHz . The short-circuited cable is first energized by the oscillator, then the probe is moved along the cable. Initially a tone is heard in the headphones which falls to a minimum when the short-circuit is reached. Price is $\{2517 \mathrm{~s}$ 6d $\left(\left\{25.87 \frac{1}{2}\right)\right.$ for the detector and $\AA 1212 \mathrm{~s}(\Omega 12.60)$ for the oscillator. ITT Electronic Services, Edinburgh Way, Harlow, Essex.
WW 316 for further details

## Pulse Generator

A general purpose pulse generator, type TF2010, has been introduced by Marconi Instruments. It provides positive and negative outputs, single or double pulse. Double pulse outputs are delivered from 2.5 Hz to .2 MHz and single pulse outputs up to 2.5 MHz . Features include continuously variable amplitude up to 20 V , variable pulse width from 100 ns to 10 ms , and 10 ns rise time. Internal or external triggering may be used; the internal trigger frequency is adjustable over the range 2.5 Hz to 2.5 MHz . External triggering can be

achieved by the application of a sine, square or pulse waveform. In addition to the main output waveform, a positive or negative "pre-pulse" is delivered from a separate socket. Dimensions of the instrument are $100 \times 360 \times 270 \mathrm{~mm}$ deep. Price: $£ 135$. Marconi Instruments Ltd., St. Albans, Hertfordshire.
WW 326 for further details

## Magnetic Memory

Utilizing a miniature reed switch and designed for printed circuit mounting, a compact memory element announced by F. R. Electronics is suitable for applications such as the retention of information in the event of power failure, or the replacement of conventional relays in portable equipment. Designated type RSC68, the memory is small ( $35.6 \times 17.8 \times 16.5 \mathrm{~mm}$ ) and has good vibration and shock characteristics. Price is about $\Omega 110 \mathrm{~s}(\Omega 1.50)$. F. R. Electronics, Wimborne, Dorset.
WW 321 for further details

## Answers to "Test Your Knowledge'"-13

## Questions on page 284

1. (c). The amplitude of the modulating signal determines the frequency deviation of the carrier, the frequency of the modulating signal determines the number of cycles of variation of the carrier frequency per second.
2. (c). Mathematical analysis show's that if a carrier $A \sin \omega_{\rho} \ell$ has its frequency varied by a signal of the form $\cos \omega_{m} t$ so that the frequency deviation (maximum frequency excursion) is $d f$, then the modulated carrier can be written $A \sin \left(\omega \ell+\frac{\Delta f}{f} \sin \omega_{m} t\right)$.
3. (a). The mean power output of a frequency modulated transmitter is constant whatever the modulation.
4. (b). It must be so since the mean power output is unchanged.
5. (b). The number of components with significant amplitude decreases as the modulating frequency increases, but the frequency separation between components increases so that the total bandwidth required to include all significant side frequencies is about the same for all modulation frequencies.
6. (c). A combination of the two is used in transmitters where it is most convenient to generate f.m. of small deviation at a low carrier frequency and then increase the carrier output and the deviation to those required at the output.
7. (d). In phase modulation the modulation index (or phase deviation) is independent of modulating frequency; in frequency modulation it is inversely proportional. Hence in the Armstrong system the modulating signal is first passed through a network which produces attenuation proportional to frequency before it is applied to the balanced mixer. This method cannot produce a phase deviation greater than about $\frac{1}{4}$ radian without introducing significant distortion.
8. (a). The weaker signal modulates the phase of the stronger signal (amplitude variations are removed by the receiver limiting action). The phase variation of the stronger signal due to this cause cannot exceed 0.46 radian, whatever the carrier frequency or modulation index of the weaker signal.
9. (d). The "rule of thumb" for wide frequency deviation systems is that a range of frequencies equal to the maximum deviation plus maximum audio frequency on either side of the carrier must be passed.
10. (b). For a sinusoidal modulating signal the carrier phase at the output of the i.f. amplifier will not vary sinusoidally.
11. (a). Provided that limiting still occurs in the receiver the extent of the service range is determined by the distance from the transmitter at which the unmodulated carrier amplitude is about twice the mean noise amplitude. With a narrower bandwidth system the mean noise amplitude will be smaller.
12. (c). a.g.c. is usually incorporated as well
13. (c). For a sinusoidal modulating signal
$\varphi(t)=\frac{d f}{f} \sin \omega_{m^{t},} \Delta f$ being proportional to the modulating signal amplitude.
Hence $\left.\frac{d \phi(t)}{d t}=2 \pi\right\lrcorner f \cos \omega_{m}$.
14. (b). Since with f.m. the noise suppression is least at the highest audio frequencies, components of the input signal at these frequencies are deliberately "preemphasised" at the transmitter. The circuit referred to is the "de-mphasising" circuit.


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+ K. 515 Knob
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A Moulded body toggle operated D.P.C.O. 8 contact switch for double switch for double pole alternative circuit switching. Replacing the popular laminated body type $S .277$ to which it has dimensional conformity but improved performance.

Switched legend indicator unit with D.P.C.O switch rated 2 A .250 V . A.C. and holders accepting L.E.S. lamps. Legending to order


Knob dial and escutcheon assembly. dial legending is only visible through window in escutcheor and is carried out to customers re quirements. Whole unit is colle fixing to $\frac{1}{}^{\prime \prime}$ dia shafts

Two, three pole side entry jack plugs The 'third 'Ring contact between the 'Sleeve" and 'Tip' can serve as a guard-ring or as a third pole, or 'Sleeve can carry screening continuity of 2 pole + screen cable. The design matches that of our popular model P.535-6. P. 538 Gold


Further addition to the D.P.C.O. Moulded Switch range. Key operated rated at 2 A .250 V A.C. N.I.

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## World of Amateur Radio

## Direct-conversion "Homodyne" Receivers

Increasing interest is being shown by amateurs in the development of relatively low-cost receivers in which the incoming signal is heterodyned directly, by means of a balanced linear detector, to audio frequency. This form of "straight" receiver was described, in a valve version, by James White, (W2WBI) of Princeton, N.J., in QST, May 1961, but has attracted more attention since it was revived, using transistors, by the Dutch amateur K. Spaargaren (PA0KSB) in Electron (Jan. 1967) and by R.S.G.B. Bulletin. An interesting design, in which the linear derector comprises four hot-carrier (Schottky) diodes using wideband ferrite toroid transformers, has also attracted considerable attention.

The basic requirements for such direct conversion or simple synchrodyne receivers are a well-balanced linear detector, a stable variable-frequency-oscillator on the signal frequency, an audio filter and a high-gain, low-noise a.f. amplifier. The oscillator can also form the basis of a simple transceiver. For the reception of broadcast or other a.m. transmissions, the oscillator requires to be phaselocked to the incoming signal as in the Tucker synchrodyne, but this refinement is unnecessary for the reception of s.s.b. or c.w. signals, for which the current receivers are generally intended. Provided that the detector is linear and accurately balanced, selectivity can effectively be determined by the characteristics of the audio filter without incurring cross-modulation or blocking. The use of hotcarrier diodes or beam deflection valves (types 7360 or 6 JH 8 etc ) can result in excellent noise figures without requiring any r.f. stage. An inherent problem-unless a more complex phasing type detector were used-is the presence of the audio "image" which can be eliminated by the i.f. selectivity of singlesignal superheterodyne receivers. Nevertheless, good audio selectivity can minimize this disadvantage. Several simple receivers of this general type, using either semiconductors or valves, are known to have been built by British amateurs, with generally satisfactory results.

## Ionospheric "Openings" on 50 MHz

Despite the earlier belief that Solar Cycle 20 was already on the decline, 50 MHz conditions this year appear better than at any other time during the current sunspot cycle. M. Waters, G3JVL, of Portsmouth, heard the south-west

African station, ZS3B, at very good strength for $1 \frac{1}{2}$ hours from 13.50 G.M.T. on April 4th, almost certainly due to $\mathbf{F}$ 2 layer ionospheric propagation. Don Hayter, G3JHM, of Worthing, similarly recieved the 40 -watt Rhodesian beacon station ZE1AZC from 16.30 to 17.15 G.M.T. on April 14th, with signals peaking RST99. One suggestion, being mooted in amateur circles, is that Solar Cycle 20 may be following precedents in having two main peaks, spaced roughly one year apart, and offering the prospect that higher maximum usable frequencies may occur this year, than those of 1968.

## "Top Band" DX

The current world "wanderings" of Gus Browning, W4BPD, have brought several new countries briefly on to "Top Band" (1.8 MHz ). His expedition to Rodriguez, in conjunction with VQ8CC, however, resulted in only one two-way contact being made on this band; this was with the British station G3XAQ. Gus Browning's 1.8 MHz operation as ZD3A produced no two-way contacts, though his signals were heard in the U.K., and he heard veteran top-bander, Stewart Perry, W1BB. Incidentally, Stewart Perry recently achieved his DXCC ( 100 confirmed countries) on this band following a contact with HK0TU, Malpelo Islands-despite trouble, during the contact, with his coaxial feeder. He later lifted his total worked to 104 countries with a contact with VP2KK, the St. Kitts' expedition.

## Chordal Hop Theories Gaining Support

 There is a growing feeling among some British amateurs that throughout the h.f. and v.h.f. spectrum (and possibly also at m.f.) long distances are often covered by means of "chordal hop" and related modes not requiring intermediate ground reflection points. The chordal hop theory, now attracting increasing attention in professional research and communications, was originally put forward by Hans Albrecht, following the careful measurements made by him and a large number of other Australian amateurs in the early 1950 s , on $3.5,7$ and 14 MHz signals received in Australia from amateurs in West Europe. Albrecht subsequently returned to Europe and suggested the name "chordal hop" to explain his idea that signals could be reflected more than once from ionospheric layers without returning to earth each time. Theapparent absence of intermediate ground reflection points is now also recognized as occurring during transequatorial (TE) propagation, which was first investigated as a result of amateur long-distance openings on 50 MHz , at times when this band should have been well above the maximum usable frequency. Such mechanisms have more recently been suggested by M. Hall of the Radio and Space Research Station, Ditton Park, Slough, as playing a significant role in v.h.f. propagation. Possibly as a result of ionosperic tilts and/or "whispering gallery" layer entrapment, it now seems likely that many of the amateur DX contacts, previously thought to be due to conventional multi-hop F2 propagation, are in fact made without intermediate ground reflection, accounting for the low path losses and high m.u.f. often observed. More precise knowledge of such propagation modes could have considerable importance for radio communication and broadcasting.

## National Field Day

The R.S.G.B. National Field Day, with all participating stations operated from tents by amateur radio clubs and R.S.G.B. groups, is being held this year over the period 17.00 G.M.T. June 7th to 17.00 G.M.T. June 8th. For many years, this event-first held in June 1933-has been the most keenly contested of all British portable events, and involves the largest number of operators. At the first event, 34 stations were operated by 18 groups; last year, when Cannock Chase Amateur Radio Society gained the coveted shield, some 150 stations were entered by about 100 groups and clubs. Contacts, on c.w., can be on any three bands from 1.8 to 28 MHz .

## Other June Events

A mobile rally organized by the Amateur Radio Mobile Society is being held on June 1st at the Shuttleworth Aircraft Museum, Biggleswade.

The Bristol R.S.G.B. Group, assisted by the Bristol Amateur Radio Club, are organizing for June 29th the Longleat Mobile Rally at Longleat Park, near Warminster.

A Midlands VHF/UHF Convention and Dinner-including a lecture on "a new approach to vhf/uhf receiver design" is being held at Wolverhampton on June 14th (details from P. G. Wright, 20 James Road, Kidderminster, Worcester, enclosing foolscap stamped addressed envelope).

In Brief: A new beacon station, GB3SU, operating on 70.695 MHz is located at the University of Sheffield . . . Latest F.C.C. figures put the number of amateur operators in the United States at 256,546 , down very slightly on a year ago . . A.R.R.L. reports its full membership down $1 \%$ to 80,012 with worldwide membership given as 97,678 . . Membership of the International Amateur Radio Union, following the admission of societies representing Mauritius and Surinam, now stands at $80 \ldots$ U.S. amateurs, as a result of changes in the Bell System telephone regulations, can now legitimately operate "phone patches" connecting overseas stations to telephone subscribers.

Pat Hawker, g3ya

# AMPLIFIER SUPPLEMENT 

# The Vital Statistics of an Audio Amplifier 

by R. Williamson

A definition of the term "high fidelity" would be a logical opening to a discussion on high-quality amplifiers (yes, I'm sufficiently old fashioned to prefer high quality to the imported term-but high fidelity, or "hi-fi", is here to stay and I have no intention of starting a revolution to change it back again). A precise definition is quite impossible, since there is no clearly defined boundary at which "low fidelity" (sic) ends and high fidelity begins.*

In the final analysis, a purely subjective judgement by the listener will decide one way or the other and so long as the human element is involved in assessing reproduced sound quality, the boundaries will continue to remain blurred. I much regret that in recent years there has been no real progress towards a more precise definition. Anyone may slap a label "high fidelity" on an amplifier despite a frequency response which, if reproduced graphically, would look something like the hind leg of an arthritic donkey.

The amplifier is the "heart" of any sound reproducing system and I intend to discuss its vital statistics, to examine the facilities one expects to find and finally, to draw attention to typical and particularly interesting design features.

## Distortion level and distortion figures

At the head of my list of vital statistics for good sound quality is the degree of non-linear distortion up to the maximum rated output. By non-linear distortion I mean any spurious harmonic and intermodulation products in the amplified signal. For these to be negligible the dynamic input/output transfer characteristic should be linear within clearly defined limits up to maximum output at all frequencies within the accepted audible range.

In the U.S.A. intermodulation products are often quoted and although some authorities might justifiably attach equal or even greater weight to this information, the practice of quoting i.m. products is not usual in the U.K.

It is here that it might be worthwhile examining a very thorny problem-that of evaluating the figures quoted. Just prior to the transistor amplifier era, valve designs had reached a very high standard, and at levels up to the rated power generated harmonics were at a very low level, and usually of a low order. The magical figure was a total harmonic distortion (t.h.d.) of below $0.1 \%$ and one could literally assume that with the best on the market, the amplifier was the strongest link in the reproducing chain. Almost, one might say-and here I cannot resist quoting my favourite advertising blurb-a "straight wire with gain".

When the change to transistors began, and using the germanium devices available at that time, designers were to some extent obliged to take advantage of the high efficiency possible with them. Not only were the early circuits virtually "transistorized" valve amplifiers, but class B output stages came back, *Does "fidelity" need qualifying? Fidelity or infidelity!-ED.
too, sometimes with driver transformers which had long since disappeared from the valve amplifier scene! Small wonder, then, that soon there were complaints that not only was the sound "different" to the best valve amplifiers, but that in most cases it was very much inferior.

However, the rapid development of semiconductor technology began to yield its own circuit techniques, and, following the concept of complementary symmetry and the publication of the well-known circuit by H. C. Lin in 1956, $\dagger$ transistor amplifiers began to improve. But the so-called "transistor" sound persisted and it began to be appreciated that it was primarily due to minute amounts of crossover distortion arising from the inherent asymmetry of a quasi-complementary output stage operating in the class B mode. A new generation of designers and listeners were re-discovering that there are two kinds of harmonic distortion; the even harmonic (nice) sort and the odd harmonic (nasty) sort; furthermore, the nasty sort could be extremely objectionable when caused by even minute discontinuities in the transfer characteristic at the transition point and consisted of very high order odd harmonics. It had been well understood for some time that these high order harmonics can provoke a degree of discomfort and have an unpleasant aural effect out of all proportion to their actual level in ratio to the fundamental, even though as low as the long accepted $0.1 \%$. At least one manufacturer has suggested that this type of distortion must be as low as $0.003 \%$ if the "transistor" sound is to be eliminated.

## Frequency response

An audio amplifier is required to handle the audible spectrum from say 20 Hz to 20 kHz . Wait! Before the "let's entertain the bats as well" fraternity rush for their pens and paper, let me make a plea for sweet reason in this. We are, after all, considering high quality sound reproduction in the home and there isn't the slightest doubt that for you and me, the programme sources that are available are going to have bandwidths that are very much less than this for most of the time. Limits to the bandwidth are being imposed all along the chain to the listener's loudspeaker, and wasn't it Capt. P. P. Eckersley who wisely remarked, apropos audio bandwidth that "the wider you open the window, the more the dirt flies in!'?

Fortunately, in the present state of the art of amplifier design, an acceptable bandwidth at normal power levels presents no problem and our specification can easily be met within $\pm 1 \mathrm{~dB}$ and with no more than 3 dB loss at an octave above and below the prescribed limits.

## Power bandwidth

Rather more important is power bandwidth; the amplifier must be able to handle comfortably this frequency range at or near full power without measurable degradation of the signal. This + H.C.Lin, "Quasi-Complementary Transistor Amplifier," Electronics, Sept. 1956.
requirement is not quite so stringent at the extreme high end of the passband, and in a practical amplifier it would be acceptable for the power bandwidth to fall above 15 kHz . A typical specification will indicate the limits of power bandwidth at -3 dB points. Again, with modern design techniques, this modest requirement should be met without difficulty and in a typical product, the -3 dB points will be well beyond these limits-although some early germanium designs might fall short of these standards.

## Transients

The ability of an amplifier to handle without degradation wavefronts with a fast rise time is referred to as its "transient" response and will be related to the upper limits of its frequency response and inherent stability. The rise time of a modern transistor design is likely to be very much faster than that occurring in the waveforms of programme sources accessible to the domestic user.

## Damping factor

For good frequency response and transient handling ability the speaker system must be well damped electrically. Movement of the cone of a moving-coil loudspeaker is restricted by its suspension stiffness and resistance, by air loading and electromechanical damping. While it could be argued that with a modern 'infinite baffle' speaker the inherent damping of the system is already very high and that further electromechanical damping would be superfluous, I would suggest that it is still of importance because of the large number of speaker systems that do not fall neatly into this category.

Typically, in a modern feedback amplifier, the source impedance will be a fraction of an ohm and substantially resistive. The damping factor is usually derived by dividing the actual source $Z$ into the nominal load $Z$. Values of quoted damping factor vary from 20 to 150 , although there is little point in deliberately aiming for values as high as this, since the speakers own resistance has to be taken into account and is effectively in series. In fact, there are good grounds for suggesting that a damping factor of not less than 15 is adequate for all practical purposes. Nevertheless, one must deplore the increasing practice of actually adding quite large amounts of passive resistance in series with the speaker circuit on some recent commercial designs, ostensibly to limit the current in the output stage when low-impedance speaker systems are used. One such model recently reviewed had a measured source $Z$ of nearly 5 ohms at the 4 - ohm speaker terminals. The measured frequency response was markedly degraded.

## Power rating

It is perfectly true that a mere one watt of power into an efficient speaker will generate a very healthy noise and probably more than enough for most domestic users. However, commercial speakers seem to get less and less sensitive as designers trade efficiency for quality. It is a purely personal view that to take this into account, and yet to preserve at all times the capacity of the system to handle the maximum possible dynamic range, the power rating should not be less than 10 watts per channel in a stereo system.

And this is, I feel, an opportune moment to discuss the highly deplorable bandying about of figures that seems to be the current advertising practice when referring to power handling ability. Almost any subterfuge goes, it seems, if that highly important figure in watts can be inflated. We have peak watts, music power and I.H.F. rating to mention but three popular methods of enchancing the power, and no doubt these ratings would carry some validity if everyone fully understood what they meant; unhappily, the vast majority of the lay public haven't the faintest idea what they mean.

I have one such advertisement before me at this moment and
by virtue of what it omits to say it is quite misleading. The product is variously described as a 12 -watt amplifier, with 24 watts peak power, 15 watts music power and 30 watts peak (music?) power. We are also furnished with the information that power requirements can be met by using batteries if so desired.

This juggling with figures can only but utterly confuse the less knowledgeable reader, who is likely to purchase the product, attempt to use it with an inefficient 15 -ohm loudspeaker and a $6-V$ battery supply and then wonder why it sounds like his younger sister's transistor portable with its honest 500 mW power rating. One can only hope that recent legislation will offer some means of regulating this sort of advertising.

I would suggest that a straightforward measurement of the power dissipated in a specified load under continuous sine wave input and taken at the onset of symmetrical clipping, has the merit of being the least equivocal method of assessing power rating.

## Input sensitivity

The sensitivity of each of the inputs provided on an amplifier is usually expressed as the r.m.s volts "in" for maximum power "out"; but the manner of expressing sensitivity in this way can be a little misleading, as indeed can be the method of quoting the signal-to-noise ratio.

Take, for example, a 10 -watt amplifier with a pickup input typically rated at 2 mV for maximum output. What will not be obvious to the uninitiated is that a 20 -watt amplifier with the same sensitivity and $\mathrm{s} / \mathrm{n}$ ratio is actually twice as sensitive as, and has a $\mathrm{s} / \mathrm{n}$ ratio 3 dB better than, the 10 -watt model. The reason for the increase in sensitivity is probably quite clear (the 20 -watt model will need only 1 mV to produce the same volume of sound from the same speaker as the lower powered amplifier) but the apparent improvement in $\mathrm{s} / \mathrm{n}$ ratio might not be quite so obvious. Since the noise generated in an amplifier usually originates in the earlier low-level stages, it follows that for the 20 -watt amplifier to produce 10 watts for a $2-\mathrm{mV}$ input, the volume control will have to be adjusted to reduce the signal level by 3 dB ; and, of course, the generated noise is also attenuated by the same amount.

## Stability

The final requirement one expects of a well-designed amplifier is that it should be unconditionally stable, bearing in mind the complex load conditions presented by some modern speakers, such as those with multiple drive units and crossover networks.

In a feedback amplifier the loop gain must be tailored so that it falls below unity at frequencies where the phase shift reaches $180^{\circ}$. Whilst with silicon planar transistors the unrestricted passband could extend well into the megahertz region, such a range is neither necessary nor desirable.

Such an amplifier could be unduly sensitive to small reactive components in the load and even if not going into sustained oscillation, the performance could be severely degraded if the amplifier were provoked into "ringing" by steep transients in the signal.

## 'Facilities'

What facilities does one expect to find in a modern high-fidelity amplifier? While it is idealistically the aim of amplifier designers as well as the manufacturers of pickups and loudspeakers for their product to have a linear frequency response over the audible range, somewhere in the programme chain, something or somebody will let the side down and there will be introduced some imperfection that will mar the quality of the sound that emerges from the loudspeaker.

Nevertheless, the facilities we have now come to expect as a

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200 WATT AMPLIFIER．Can deliver its full audio power at any frequency in the range of 30 $\mathrm{c} / \mathrm{s}-20 \mathrm{Kc} / \mathrm{s} \pm 1 \mathrm{db}$ ．Less than $0.2 \%$ distortion at $1 \mathrm{Kc} / \mathrm{s}$ ．Can be used to drive mechanical devices for which power is over 120 watt on continuous sine wave．Input 1 mW 600 ohms．Output $100-120 \mathrm{v}$ or $200-240 \mathrm{v}$ ．Additional matching transformers for other impedances are available．

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CP50 AMPLIFIER．An all silicon transistor 50 watt amplifier for mains and 12 volt battery operation， charging its own battery and automatically going to battery if mains fail．Protected inputs，and overload and short circuit protected outputs for 8 ohms－ 15 ohms and 100 volt line．Bass and treble controls fitted．
Models available with 1 gram and 2 low mic．inputs． 1 gram and 3 low mic．inputs or 4 low mic．inputs．
100 WATT ALL SILICON AMPLIFIER．A high quality amplifier with 8 ohms－ 15 ohms and 100 volt line output for A．C．Mains．Protection is given for short and open circuit output over driving and over temperature．Input 0.4 v on 100 K ohms．

20／30 WATT MIXER AMPLIFIER．High fidelity all silicon model with F．E．T．input stages to reduce intermodulation distortion to a fraction of normal transistor input circuits．The response is level 20 to $20,000 \mathrm{cps}$ within 2 db and over 30 times damping factor．At 20 watts output there is less than $0.2 \%$ inter－ modulation even over the microphone stage at full gain with the treble and bass controls set level．Standard model 1－low mic．balanced input and Hi Z gram．

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## Sanswi


permanent feature of a typical high-fidelity amplifier have fallen into a set pattern, and I propose to take each in turn, to describe its function and illustrate with extracts from the circuits of currently available commercial amplifiers.

## The amplifier stages

Probably the most important stage is the so-called "front end", the point at which the often minute signal from the programme source is amplified to a level which raises it well above the inherent noise of the system. It also carries out one other important function, that of equalizing the signal from the gramophone pickup.

To all intents and purposes, the signal on a modern LP disc is recorded at constant amplitude and with a velocity proportional to frequency. So when the system includes a velocity sensitive pickup, and this means the majority in use today (moving magnet, moving coil and variable reluctance dominating the field) the voltable at its output terminals will be proportional to the frequency on the disc.

The shape of this voltage curve has long been determined to an international standard, and the input stage has to introduce an inverse of this curve within close tolerance. A particular two-transistor circuit has become popular with designers-the d.c. feedback pair which I believe can be accredited to J. Somerset Murray (British Patents 80927 and 83245 ). Originally developed with germanium transistors to give tight d.c. "sit" points under conditions of varying temperature and using transistors with a wide production "spread" it has passed into use with modern silicon planar types. The input stage of the Heathkit TSA-12 is typical of the many variants of this type of circuit, and not only compensates for the replay curve but provides for a sensible amount of overall gain (Fig. 1).

That the input stage should contribute negligible noise to the signal is a basic requirement generally appreciated, and to this end it is common practice for the first transistor to be run at less than 0.5 mA . The second transistor is normally run at a higher $I_{c e}$ and a figure of $1-2 \mathrm{~mA}$ is again typical. The collector load is chosen to take into account the shunting of the feedback network and a low-noise working condition is here of rather secondary importance. Suffice to say, that in respect of $\mathrm{s} / \mathrm{n}$ ratio, most modern designs are satisfactory, and on the most sensitive input a -65 dB figure or better should be attainable, even using modern low-output magnetic cartridges.

Since it is in overload capability that there is some variation in the standards achieved, let's examine the problem and see what is involved. Consider a typical magnetic pickup with a sensitivity of $1 \mathrm{mV} / \mathrm{cm} / \mathrm{sec}$, which will generate from the average LP disc a signal in the region of 5 mV . Allowing for the dynamic range possible on a modern recording, one must cater for peak velocities of up to $20 \mathrm{~cm} / \mathrm{sec}$ and this means the peak terminal voltage from the pickup may reach 20 mV . With a midband overall gain for our "front end" of, say, 150, the peak signal level at the collector of the second stage will be up to 3 V . The designer has to ensure that the input stage is able to handle signal levels of this magnitude without distortion, at all frequencies over the audible band and it has come to be accepted that such an input stage must be able to handle not less than +20 dB over the rated input level and preferably very much more.

An alternative to the simple two-transistor pair, and representative of a sophisticated design philosophy, is that adopted by Radford in their SCA30. Here (Fig.2) an additional buffer stage in the common collector mode has been added to the conventional pair as an impedance conversion device. This offers certain advantages, in that the second common emitter stage can now be tailored for the maximum possible gain, having now been relieved of the loading of the feedback network, and can operate at low $I_{c e}$.

Cambridge Audio bring a highly individual approach to the problems of input stage overload. They have abandoned the
traditional concept of a feedback equalizing pair at the input, and substituted instead a straightforward linear amplifying stage with overall variable parallel feedback-the variable element being the volume control. By using a "virtual earth" amplifier in this way, a number of virtues are claimed, including a better than +60 dB overload factor and a $\mathrm{s} / \mathrm{n}$ ratio that is independent of the source $Z$ (Fig.3). The function of equalization is delegated to a later stage.

Inputs that are already at a suitably high level and equalized (such as from a tuner) are usually selected by switching, and are injected across the volume control. An alternative is to convert the front end from an equalizing stage to one of fixed linear gain, and feed the high level signal in at the same point via a passive, sometimes variable, attenuator.

On many imported models, and on some British designs conceived with an eye on the healthy export market, the volume control is sometimes replaced by, or can by switching be converted to, the controversial loudness control. This feature is guaranteed to arouse passionate feelings whenever discussed by the true apostles of the hi-fi religion, as readers will be well


Fig. 1. Input stage of the Heathkit TSA-12.


Fig. 2. Input stage of Radford SCA-30.


Fig. 3. Input stage of Cambridge Audio P40 and P8O.
aware from Letters to the Editor published some months ago. The principles on which the action of the loudness control is based, is that the ear becomes disproportionately less sensitive to low frequencies and, to a lesser degree, high frequencies as the loudness (volume) of the sound source diminishes.

Unfortunately, its staunchest protagonists refuse to recognize the simple fact that it just doesn't always make a low-level sound more natural; for example one has only to listen to the reproduced male voice while manipulating a loudness control.

On the other hand, there is another side of the argument that should be recognized. Hi-fi is no longer the cult of the few but big business, and its products are subject to the dictates of consumer demand and market research. If evidence derived from such sources indicates that the consumer regards some form of loudness control as a desirable feature, then who are our experts and, even more important, British manufacturers to wrinkle a fastidious nose and ignore the demand? Audio amplifiers are going to be used in the home for background music, and the loudness control takes the effort out of making a pleasant noise at low volume level. Foreign competitors are aware of this, and laugh at our conservative attitudes all the way to the bank. . . . If it helps to sell the product, then put the loudness control in, so long as it can be switched out by the pure at heart; and above all, spare us the scientific evidence of its desirability. Fig. 4 shows the loudness control in the Sansui AU-777 and is typical.
Une expects the well-dressed amplifier to have tone controls, of course. These permit some adjustment to the treble and bass ends of the spectrum relative to a midband point-which may be anywhere from 500 Hz to 1 kHz . The degree of variation is usually up to $\pm 15 \mathrm{~dB}$ at 15 kHz and of a similar amount at 40 Hz . There are, basically, two modes in which these controls operate. Broadly speaking they are related to whether the designer has opted for passive equalization or the adjustment of reactive elements in a feedback network. The feedback


Fig. 4. Sansui loudness control circuit.


Fig. 5. Tone control stage of Leak 'Stereo 30 Plus'.
type, especially that due to Baxandall, appears to enjoy the greatest popularity and that used in the Leak "Stereo 30 Plus" is a well tailored version (Fig. 5).

Whilst tone controls have a maximum slope that does not exceed 6 dB /octave, it is frequently desirable, one might say almost essential, to have low-pass filter facilities that operate at a far greater rate than this and particularly at the high end of the spectrum. Objectionable noises and harmonic and intermodulation products are likely to appear in an imperfect signal above, say, 5 kHz , and it is useful to be able to attenuate these rapidly. The rate of slope for these steep cut filters should not be less than $-12 \mathrm{~dB} /$ octave and to achieve these higher attenuation rates, designers either adopt a two-section $R C$ network or in a more sophisticated approach, will use bridged-T networks in a feedback configuration. Curiously enough, designers seem to fight shy of using combinations of $L$ and $C$, although Leak have included a basic half section in their "Stereo 30 Plus" with one switched turnover frequency at 6 kHz . Quad, on the other hand, have gone in for a full-blooded version, very comprehensive, with three switched turnover points at 5,7 and 10 kHz (by means of a tapped inductor) and the facility of being able to vary the slope on a calibrated control up to a maximum of 25 dB /octave.

It is regrettable that many amplifier manufacturers seem to regard a really effective low-pass filter as less than essential.

At the low end of the spectrum a high-pass filter is either permanently included or switchable, to limit the response below 20 or 30 Hz in order to attenuate mechanical noise or "rumble" produced by the record turntable.

Paradoxically, inexpensive amplifiers which might be complemented in a budget system by a turntable of comparable cost, invariably omit this feature and response is likely to be unrestricted down to subsonic levels.
The power amplifier: Both at home and abroad, a small number of manufacturers eschew completely the principle of complementary working, possibly because originally, suitable high-voltage complementary pairs of driver transistors were somewhat thin on the ground and carried a price tag that reflected their scarcity. This inhibiting factor applied equally to n-p-n types in the germanium era and later, with silicons, p-n-p's were in short supply and somewhat costly. Rogers, for example, have opted for a driver transformer in both their Ravensbourne and Ravensbrooke. By employing a carefully designed quadrifilar wound component, it is claimed that most of the inherent disadvantages usually associated with transformer drive have been overcome. Incidentally, without exception in my experience, output transformers have disappeared entirely and designers have opted for the series push-pull transformerless output stage, irrespective of the method of phase inversion adopted. But broadly speaking, the quasi-complementary class B transformerless circuit is highly favoured.

However, right from the introduction of the first transistor amplifier, there began to be complaints (and sometimes, even approval) of the so-called "transistor sound", and discounting some of the highly subjective reasons advanced one can justifiably argue now that the main cause can usually be attributed to the inherent asymmetry of the Lin-type quasicomplementary configuration. The principal "cure" has been, so far, to rely upon the high overall negative feedback that has come to be regarded as almost mandatory with this type of amplifier. During a recent evaluation of a very expensive amplifier there was, at low listening levels, some crossover distortion audible. Yet the reproduced sine wave at approximately the same level, 200 mW , showed not the slightest sign of this defect and the sum of the distortion products when measured on a distortion factor meter hardly reached our hitherto acceptable figure of $0.1 \%$.

We are faced, then, with the problem of how to equate the subjective effects with the degree of aural "objectionable-ness" that this form of distortion provokes, and to express it in

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Three different models of the Uher 'Report' are now available.
4000 Report - L Specification. 2 Tracks conforming to international standards. Tape reels diam. $-5^{\prime \prime}$. Tape speeds (ips) $\frac{18}{16}, 1 \frac{7}{8}, 3 \frac{3}{4}, 7 \frac{1}{2}$. Frequency range (cps) 40-4, 500/40-10,000 and 40-16,000/40-20,000. Dynamic volume range (db) 40 at $\frac{18}{18} \mathrm{ips}, 46$ at $1 \frac{7}{8} \mathrm{ips}, 50$ at $3 \frac{3}{8} \mathrm{ips}, 52 \mathrm{at}$ $7 \frac{1}{2}$ ips. Wow and flutter ( $\max \pm \%$ ) 0.2 at $7 \frac{1}{2}$ ips. Recording mono. Half-track. Playback mono half-track. Power output one watt.
Monitoring via headphones or speaker. VU meter + three digit tape counter. Tape stop-start remote control, collectorless motor controlled by 8 transistors. Power supply from $6 \mathrm{~V}, 12 \mathrm{~V}, 24 \mathrm{~V}$ car battery, from rechargeable accumulator or 5 type L.P. U2 batteries or mains unit. 17 transistors. Inputs : Microphone :$\cdot 1 \mathrm{mv}$ at 200 ohms. Radio :- 2 mv at 47 K ohms. Pick up :-30mv at 1 megohm. Weight 6 lbs (approx). $125 \mathrm{gns} .+10 \%$ tax surcharge.
4200 Report Stereo Affording all the advantages of the successful 4000 Report-L in size, style and specifications-plus stereo. 152 gns.
$+10 \%$ tax surcharge.
4400 Report Stereo Again with all the advantages of the 4000 Report-L -plus stereo and maximum economy of tape on four tracks without deterioration of reproduction quality. $152 \mathrm{gns} .+10 \%$ tax surcharge.

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To capture the sounds of history being made.

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doesn't reckon he can do any better than that.

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quantitative terms. Fortunately, this is a problem that may be esolved by the adoption of techniques in transistor circuitry hat will eliminate once again this particularly objectionable lefect. The obvious line of attack is to try to overcome the inherent asymmetry of the orthodox quasi-complementary class B output stage, although there has developed a strong "back to zlass A" movement as exemplified by the two commercial models produced by the Richard Allan company.

While one cannot deny that a good class A design will eliminate crossover distortion completely, in my view this is design by expediency and metaphorically speaking, simply sweeping the difficulties under the carpet of the $R$ and $D$ department. The many disadvantages of class A working in a transistor amplifier, its low efficiency for example, far outweigh the short-term advantage of freedom from just one aberration in the performance of an audio amplifier.

I emphasize short-term, because already, there is evidence that designers with a more imaginative approach are developing ways to eliminate the asymmetry of the class B stage, the use of complementary "triples" as adopted in the Quad 303 being well to the fore in sophisticated elegance (Fig. 6).

Aside from the technique developed by Quad, the orthodox remedy is likely to be the adoption of full complementary working following the increasing availability of pairs of $n-p-n / p-$ n-p silicon power transistors and whilst they are still not too plentiful, the Radford SCA30 employs this technique. Models P40 and P80 from Cambridge Audio also use a complementary pair of silicon transistors in the output stage with the added refinement of constant current drive. It is claimed that this technique reduces even further the effects of any asymmetry that remains in the complementary output'stage.

While the increasing use of silicon devices improved the robustness of high-quality amplifiers under a wide range of expected working conditions, it is an inescapable fact that transistors have not yet the inherent resistance to short-term overload of valves and most leading manufacturers might, in an unguarded moment, admit to some unhappy experiences following an initial attempt to introduce a transistor model.

Possibly the most important problem that designers have had to contend with, is that of "second breakdown" in transistors and principally those of the large chip area power types. This is not just simple voltage breakdown, but a thermally and electrically regenerative process initiated by certain levels of voltage and current being coincident for finite lengths of time, and is produced in the output stage of an audio amplifier by undesirable reactive load conditions. Transistor manufacturers have not been slow to develop chip construction techniques to minimize the possibility of second breakdown, but the problem is still very much with the amplifier designer and some measures of circuit protection are now regarded as essential.

Protection on a short-term basis can only be achieved by comparatively fast operating electronic circuitry. Broadly speaking, the techniques being adopted fall into two categories. First, the latching-type overload trip whereby the power supply to the output stage is cut instantly under conditions of overload and has to be reset manually. This is employed in some Japanese designs, such as the Sony TA1120 and the Sansui AU777.

Most British and European designers, on the other hand, tend to favour non-latching protection and incorporate limiting circuitry into the amplifier and/or the power supply, again employing sensing techniques either with diodes as simple voltage operated switches as in the Quad 303 or as in the Radford SCA 30 which uses transistors to monitor the emitter current of each output transistor.
Power supplies. In the low and medium price ranges, the designer has usually to be content with a straightforward silicon diode bridge rectifier, plus a single electrolytic smoothing capacitor. At the other end of the cost spectrum, we have the complex thyristor regulated system of the Radford which
even includes a separate zener regulated supply for the pre-amplifier stages (Fig. 7). Power supplies of such sophistication go a long way towards rendering unnecessary any need for the advertising dept. to manipulate the power rating figures. Amplifiers of this calibre are clearly in the "professional" class and invariably carry a price tag to match.

It is safe, at least, to assume that circuit techniques will continue the process of refinement, with the increasing use of integrated circuits and correspondingly fewer discrete components, especially in the small signal stages. Whilst it is an open secret that at least one familiar name in the amplifier field is seriously considering the advantages of an integrated power amplifier and loudspeaker combination, market trends indicate that "separates" in the traditional form of tuner plus preamplifier, plus power amplifier are falling out of public favour. Preamp. and power amp. combined, in one unit, are dominating the market and eventually, the stereo receiver-all three in one-will be the favoured choice, as indeed they already are in the U.S.A. and on the Continent.


Fig. 6. Output section of Quad 303 power amplifier.


Fig. 7. One half of the power supply in the Radford SCA-30.
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## Amplifier Data <br> Audio

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information to illustrate，by example，the particular facts and figures referred to in Mr．Williamson＇s survey article．On examining the details given，the


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# richardson 

## announce the forthcoming release of their SCP 2-SIA 100 units.



The SCP 2 is similar in appearance to the SCP 1, but has plug in circuit boards and an overload factor up to +36 dB . Distortion at $+30 d B$ is less than $0.1 \%$.

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## - RADFORD

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The SCA 30 uses a true complementary symmetry output circuit using balanced npn and pnp transistors completely eliminating "crossover" distortion with its attendant listening fatigue.

The amplifier is completely stable on any input waveform and any output load and will deliver full power from 15 Hz to 80 kHz . It is proof against damage by any output load from open circuit to short circuit and load characteristics of any phase angle. Its protection is automatic without the need for replacing fuses or re-setting a cutout.

Its high sensitivity and signal/noise ratio make it ideal for use with low output high quality cartridges such as the ADC 10E, etc.

One of the weaknesses of conventional transistor integrated amplifiers and preamplifiers is the very low input signal handling capacity to transients. This has been overcome in the SCA 30 by the use of 40 Volt transistors of exceptionally low noise factor in a feedback triple circuit in the preamplifier. The 1.5 mV disc input will accept more than 100 mV before overloading!

## FM TUNER FMT 3

The FMT 3 is a transistor tuner with high sensitivity and performance of matching, presentation with the SCA 30 amplifier. It is available as a standard model FMT 3M (Mono) or FMT 3.S (Stereo).

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\begin{tabular}{|c|c|c|c|c|c|c|c|c|}
\hline Model \& Mono or stereo \& Valve or transistor \& \begin{tabular}{l}
Recommended speaker impedance \\
( \(\Omega)\)
\end{tabular} \& Maximum r.m.s. power/channel into recommended load (W) \& \[
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\] \& Power bandwidth \(\left(\begin{array}{l}( \pm 3 \mathrm{~dB}) \\ (\mathrm{Hz}-\mathrm{kHz})\end{array}\right.\) \\
\hline \multicolumn{9}{|l|}{\multirow[t]{2}{*}{}} \\
\hline \& \& \& \& \& \& \& \& \\
\hline \& \& \& \& 25 (41) \& 45 (88) \& \& \& \(20-30\) \\
\hline AUフิ77 \& S \& T \& 4 to 16 \& 25 (168) \& 24 (88) \& < 0.5 \& - \& 20-50 \\
\hline 250 \& s \& \(v\) \& 8 or 16 \& 10 (168) \& \& 1.5 \& \& 35-15 \\
\hline 350 \& s \& \(T\) \& 4 to 16 \& 18 (89) \& 34 (88) \& \(<1.0\) \& \& 30-20 \\
\hline 400 \& 5 \& T \& 4 to 16 \& 20 (88) \& 24 (8) \& \(<1.0\) \& \& 20-50 \\
\hline 2000 \& 5 \& \(T\) \& 42016 \& 32 (898) \& 24 (89) \& < 0.8 \& - \& 20.40 \\
\hline 3000A \& \({ }_{5}\) \& T \& 4 to 32 \& 48 (8) \& is (812) \& < 0.8 \& \& 20.40 \\
\hline 5000 \& 5 \& \(T\) \& 4 to 16 \& 55 (80) \& 50 (89) \& <0.8 \& \& 15-30 \\
\hline \& 5 \& \(T\) \& 4 to 16 \& 22 (8S) \& 60 (89) \& \(<0.8\) \& \& 2040 \\
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Sanyo Service and Sales, Marubeni-lida House, 164 Clapham Park Road, London, S.W. 4 \\
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Sony (U.K.) Letd., Ascot Road, Bedfont, Feltham, Middx. \\

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\hline TAli20 \& 5 \& T \& 8 \& 50 \& \(>70\) \& \(<0.1\) \& \(<0.03\) \& 10-100 \\
\hline STR6050FW \& 5 \& \(T\) \& 8 \& 30 \& \(>40\) \& < 0.2 \& \& 30-50 \\
\hline STR6060fW \& 5 \& T \& 8 \& 45 \& \(>70\) \& <0.2 \& <0.08 \& 20.60 \\
\hline \multicolumn{9}{|l|}{\begin{tabular}{l}
Solvsuper 1070 M Hybrid \\
Tandberg (Elstone Electronics Litd., Templar Street, North Court, Leeds \(\mathbf{2 )}\)
\end{tabular}} \\
\hline Sglvsuper 1071 \& 5 \& Hybrid \& 4 \& 6 \& \& - \& - \& 30-16 \\
\hline Sglvsuper 1072 \& 5 \& Hybrid \& 4 \& 6 \& - \& - \& \& 30.16 \\
\hline Huldra 9 \& 5 \& Hybrid \& 4 \& 15 \& \& \& 二 \& 30.16 \\
\hline \multicolumn{9}{|l|}{Telefunken (A.E.G. (Great Britain) Led., 27 Chancery Lane, London, W.C.2.) -} \\
\hline Allegro 101 \& \& \& \& \& \& - \& \& \\
\hline Rondo \& 5 \& T \& 4 \& 4 \& \& \& \& \\
\hline Concertino 101 \& 15 \& T \& 4 \& 10 \& \& \(\leqslant 1\) \& - \& 2020 \\
\hline \(\checkmark 201\) \& 5 \& T \& 4 \& 25 \& \& \(\leqslant 1\) \& \& ( \({ }_{17}^{17.58}\) \\
\hline V250 Hi Fi \& s \& \(T\) \& 4 \& 35 \& 30 \& 0.5 \& - \& \(10-20\) \\
\hline \multicolumn{9}{|l|}{\multirow[t]{2}{*}{Trio (B. H. Morris \& Co. (Radio) Ltd., 84-88 Nelson Street, London, E.1)}} \\
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\hline Trio Supreme I \& 1 S \& T \& 8 \& \[
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\hline Trio TK-250T \& s \& T \& 8 \& 15

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\hline Trio TK+150T \& $s$ \& T \& 8 \& 13 \& 20 \& 0.5 \& - \& 20-60 <br>

\hline \multicolumn{9}{|l|}{\multirow[t]{2}{*}{| Tripletone Manufacturing Co. Led., 241a The Broadway, Wimbledon, London, S.W. 19 |
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\hline \& \& \& \& \& \& \& $<0.2$ \& 30-20 <br>
\hline \& \& \& \& \& \& \& \& 30-20 <br>
\hline \multicolumn{9}{|l|}{Yortexion Led., $257 / 263$ The Broadway, Wimbledon, London, S.W.19} <br>
\hline 120/200 wate \& M \& \& 70/100S or $200 \Omega$ \& 200 ( 100 ) \& $20+$ \& 0.1 \& $<0.1$ \& $20-40$ <br>
\hline 100 Watt \& M \& $T$ \& $100 \Omega$ line \& 100 \& \& \& \& <br>
\hline 30/50 watt \& M \& $v$ \& $4,7.5,15 \Omega$ or 100 volt line \& 50 \& $20+$ \& 0.15 \& $<0.1$ \& 20-50 <br>
\hline 5.50 watt \& M \& $v$ \& $15 \Omega$ and 100 \& 50 \& 20 \& - \& - \& - <br>
\hline 50/70 wate \& M \& $T \quad \mathrm{~B}$ \& Bal. 100 vole \& 70 (100 vols line) \& $20+$ \& \& $<0.1$ \& 30-20 <br>
\hline CP50 \& M \&  \& ine 7.5-15 $\Omega$ and loov line \& 50 \& 10 \& (i.m.d.) \& < 0.1 \& 25-20 <br>

\hline 20/30 watt Mixer/amplifier \& M \& T \& 7.5 and 158 \& 30 \& $30+$ \& < 0.1 \& <0.15 \& $$
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\hline \& \& \& \& is (8R) \& 30 \& 0.1 \& $<0.1$ \& 30-20 <br>
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\hline \multicolumn{9}{|l|}{| Wye Electronics Ltd., Queen Street North, Whittington Moor, Chesterfield |
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\end{tabular}

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Freq. $85 \mathrm{Kc} / \mathrm{s}-25 \mathrm{Mc} / \mathrm{s}$ in 8 ranges. Incremental $:+1-1 \%$ at $1 \mathrm{Mc} / \mathrm{s}$. Output: continuously variable 1 microvolt to 1 volt. Output Impedance: 1 microvolt to 100 millivolts, 10 ohms $100 \mathrm{mV}-1$ volt52.5 ohms. Internal Modulation: $400 \mathrm{c} / \mathrm{s}$ sinewave $75 \%$ depth. External Modulation: Direct or via internal amplifier. A.C. mains $200 / 250 \mathrm{~V}, 40-100 \mathrm{c} / \mathrm{s}$. Consumption approx. 40 watts. Measurements: 19$\} \times 124 \times 10 \mathrm{in}$. The above come complete with Mains Leads, Dummy Aerial with screened lead, and plugs. As New, in Manufacturer's cases, $£ 40$ each. Carr. 30/-. DISCOUNT OF $10 \%$ FOR SCHOOLS, TECHNICAL COLLEGES, etc.

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COMMAND TRANSMITTERS, BC-458: 5.3-7 Mc/s., approx. 25 W output, directly calibrated. Valves $2 \times 1625$ PA; $1 \times 1626$ osc.; $1 \times 1629$ Tuning Indicator; Crystal $6,200 \mathrm{Kc} / \mathrm{s}$. New condition- $£ 3 / 10 /-$ each, $10 /-$ post.
(Conversion as per "Surplus Radio Conversion Manual, Vol. No. 2," by R. C. Evenson and O. R. Beach.)

AIRCRAFT RECEIVER ARR. 2: Valve line-up $7 \times 9001 ; 3 \times 6$ AK5; and $1 \times 12 \mathrm{~A} 6$. Switch tured $234-258 \mathrm{Mc} / \mathrm{s}$. Rec. only E 3 each, $7 / 6$ post; or Rec. with 24 v . power unit and mounting tray $£ 3 / 10 /=$ each, $10 /$ - post.

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COSSAR 1035 OSCILLOSCOPE, $£ 30$ each, $30 /$ - carr.
RELAYS: GPO Type 600,10 relays (a) 300 ohms with 2 M and 10 relays (a) 50 ohms with 1 M ., $\mathrm{E2} 2$ each, $6 /-$ post.
12 Small American Relays, mixed types $£ 2$, post 4/-
CALIBRATION TACHOMETER Mk. II: Maxwell Bridge Type 6C/869, £25 each, $£ 2$ carr.
ROTAX VARIAC \& METER UNTT: Type 5G. 3281. Reading 0-40 v., 0-40 mA and 0.5 amps ., all on 275 deg. scales, $£ 30$ each, $£ 2$ carr.
HEWLETT PACKARD TYPE 400C: $115 \mathrm{v} \cdot 230 \mathrm{v}$. input $50 / 60 \mathrm{c} / \mathrm{s}$. Freq. range $20 \mathrm{c} / \mathrm{s}-2 \mathrm{Mc} / \mathrm{s}$. Voltage range: 1 mV - 300 v . in 12 ranges. Input impedance 10 megohms. Designed for rack mounting, $£ 30$ each, carr. 15/\%.
TCS MODULATION TRANSFORMERS, 20 watis, pr. 6,000 C.T., sec. 6,000 ohms. Price $25 /-$, post $5 /$.
AUTOMATIC PILOT UNIT Mk. 2. This complex unit of diodes and valves, relays, magnetic clutches, motors and plug-in amplifiers, with many other items, price $87 / 10 /-$, 11 carriage.

FOR EXPORT ONLY: B. 44 Trans-ceiver Mk. III. Crystal control, $60-$ $95 \mathrm{Mc} / \mathrm{s}$. AMERICAN EQUIPMENT: BC-640 Transmitter, $100-156$ $\mathrm{Mc} / \mathrm{s}$., 50 watt output. For 110 or 230 v . operation. ARC 27 trans-ceivers, 28 V. D.C. input. Also have associated equipment. BC-375 Transmitter. BC-778 Dinghy transmitter. SCR-522 trans-ceiver. Power supply, PP893 GRC 32A ; Fltcr D.C. Power Supply F-170 G Cables CY 728/GRC; Mast
 CM.23; Directional Conirol CRD.6, 567/CRD and 568/CRD; Azimuth Control Units, $260 / \mathrm{CRD}$. Test Set URM.44, complete with Signal Generator TS.622/U.

VARIABLE POWER UNIT: complete with Zenith variac 0-230 v., 9 amps.; 2 tin. scale meter reading $0-250 \mathrm{v}$. Unit is mounted in 19 in . rack, $£ 16 / 10 /-$ each, 30/-carr.
SOLENOID UNIT: 230 v . A.C. input, 2 pole, 15 amp contacts, $\mathbf{£ 2 / 1 0 / - ~ e a c h ~}$
CONTROL PANEL: 230 v . A.C., 24 v. D.C. @ 2 amps., $£ 2 / 10 /-$ cach, carr, $12 / 6$.
AUTO TRANSFORMER: 230-115 v.; 1,000 w. £5 each, carr. 12/6. 230-115 v.; 300VA, $\& 3$ each, carr. $10 \%$.
OHMITE VARIABLE RESISTOR: 5 ohms , $5 \| \mathrm{amps}$; or 2.6 ohms at 4 amps . Price (either type) $£ 2$ each, $4 / 6$ post each.
POWER SUPPLY UNIT PN-12B: 230 v. A.C. input, 395-0-395 v. output @ 300 mA . Complete with two $\times 9 \mathrm{H}$ chokes and 10 mfd . oil filled capacitors. Mounted in 19in. panel, $\mathbf{1 6 / 1 0 / - \text { each, } £ 1 \text { carr. }}$
TX DRIVER UNIT: Freq. $100-156 \mathrm{Me} / \mathrm{s}$. Valves $3 \times 3 \mathrm{C} 24$ 's; complete with filament transformer 230 v . A.C. Mounted in 19in. panel, $£ 4 / 10 / \mathrm{m}$ each, $15 / \mathrm{c}$ carr.
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DE-ICER CONTROLLER MK. III: Contains 10 relays D.P. changeover heavy duty contacts, 1 relay $4 \mathrm{P}, \mathrm{C} / \mathrm{O}$. ( 235 ohms coil). Stud switch 30 -way relay operated, one five-way ditto, D.C. timing motor with Chronometric governor $20-30 \mathrm{v}$. ,

MODULATOR UNIT: 50 watt, part of BC-640, complete with $2 \times 811$ valves, microphone and modulator transformers etc. $£ 7 / 10 /-$ each, $15 /$ carr.

ADVANCE TEST EQUIPMENT: VM76 Valve Voltmeter, 788 each; VM78 A.C. Millivoltmeter (transistorised) $£ 55$ each; VM79 UHF Millivoltmeter (transistorised) £125 each; J1B Audio Signal Generator $£ 30$ each; TT1S Transistor Tester (CT472) $£ 37 / 10$ each. 10 per cent Discount for schools, colleges, etc. on the above items. Carr. 10/-, extra per item.

INDICATOR UNIT TYPE CRT.26: complete with CV1526 Cathode Ray Tube (3EG1). ( $3 \times$ CV138; $3 \times$ CV $329 ; 1 \times$ CV858; $2 \times$ CV261; $6 \times$ Crystals). Complete with brilliance and focus controls. Sultable for converting Into a small oscilloscope ( $10 \times 8 \times 6$ in., wt. 15 lb .) 85 each. Post $10 /-$.
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FUEL INDICATOR Type 113R: 24 v . complete with 2 magnetic counters $0-9999$, with locking and reset controls mounted in a 3 in . diameter case. Price
$30 /-$ each, postage $5 /-$.
UNISELECTORS (ex equipment): 5 Bank, 50 Way, 75 ohm Coil, alternate wipe, £2/5/- each, post 4/-

FREQUENCY METERS: BC-221, meter only ©30 each, BC-221 complete with stabilised power supply $£ 35$ each, carr. $15 /$. LM13, $125-20,000 \mathrm{Kc} / \mathrm{s}$, $£ 25$ each, carr. 15/- TS.175/U, 75 each, carr. $£ 1$. TS $323 /$ UR, $20-450 \mathrm{Mc} / \mathrm{s}$, 875 each, cart directly in digital form. Counting rate : $20-100,000$ events per sec. Time Base Crysta Freq.: $100 \mathrm{Kc} / \mathrm{s}$. per sec. Power supply: $115 \mathrm{v} ., 50 / 60 \mathrm{c} / \mathrm{s}$., $£ 100$ each, carr. $£ 1$

CT. 49 ABSORPTION AUDIO FREQUENCY METER: freq. range $450 \mathrm{c} / \mathrm{s}$ $22 \mathrm{Kc} / \mathrm{s}$., directly calibrated. Power supply 1.5 v.-22 v. D.C. $£ 12 / 10 /-$ each, carr. 15/-.
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SYNCHROS: and other special purpose motors available. British and American ex stock. List available 6d.

MARCONI NOISE GENERATOR TF-987/1; Used to determine noise factor of a.m. and f.m. receivers. Designed for 230 v. a.c. operation. In used condition, £ 20 each, carr. £1.

MARCONI TF-956 (CT.44) AUDIO FREQUENCY ABSORPTION WATTMETER; Large clear 6 in. scale. 1 microw. to 6 W . 225 each. Carr. 15/-. MARCONI DIVERSITY RECEIVERS; Consisting of $2 \times$ CR. 150's and associated equipment. \&175 each. Carr. £5.

MARCONI DEVIATION TEST SET TF-934: Freq. $2.5-100 \mathrm{Mc} / \mathrm{s}$. Can be extended to $500 \mathrm{Mc} / \mathrm{s}$. Deviation range $0-5,0-25$ and $0-65 \mathrm{Kc} / \mathrm{s}$. $£ 35$ each, carr. \&1

CANADIAN C52 TRANS/REC.: Freq. $1.75-16 \mathrm{Mc} / \mathrm{s}$ on 3 bands. R.T., M.C.W. and C.W. Crystal calibrator etc., power input 12 V . D.C., new cond., complete set $£ 50$. Used condition working order $£ 25$. Carr. on both types $£ 2 / 10 /-$ Transmitter only $£ 7 / 10 /-$ (few only) Carr. $15 / \%$. Power Unit for Rec., new $£ 3 / 5 /$-. Used power units in wirking order $£ 2 / 5 /-$. Carr 10/-.
AVOMETERS: Model 47A, 110 each, $10 /$ post. Model 7, $12 / 10 /$ - each, $10 /-$ post. Excellent secondhand cond. (Meters only-batteries and leads extra, at cost.)
DECADE RESISTOR SWITCH: 0.1 ohm per Rep. 10 positions. 3 Gang, each 0.9 ohms. Tolcrance $\pm 1 \% £ 3$ cach, $5 /-$ post.
total value 900 ohms per step. 10 positions, 3 Gang. Tolerance $\pm 1 \% \quad £ 3 / 10 /-$ each, $5 /-$ post.

TELESCOPIC ANTENNA: In 4 sections, adiustable to any height up to 20 ft . Closed measures 6 ft . Diameter 2 in . tapering to 1 in . $£ 5$ each $+10 /-$ carr. Or £9 for two $+£ 1$ carr. (brand new condition).

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## a complete stereo system for 28 gns



The new Duo general-purpose 2-way system is beautifully finlshed in polished teak veneer. with matching whalr grille. It is ideal for wall or shelf mounting either upright or horizontally
SPECIFICATION:
Impedance 10 ohms. If incorporates Goodmans high flux $6^{\prime \prime} \times 4^{\prime \prime}$ and $2 子^{\prime \prime}$ tweeter. Teak finish $12^{\prime \prime} \times 61^{\prime \prime} \times 51^{\prime \prime} .4$ guineas each. $7 / 6 \mathrm{~d}$. p \& p.
Garrard Changes from $£ 7,19.6 \mathrm{~d}$. p \& p 7/6d. Cover and Teak finlsh Plinth $£ 4.15 .0 \mathrm{~d}$. 7/6d. $p$ \& $p$.
THE DUETTO Integrated Transistor Stepeo Amplifier 9 GNS.
The Duetto is a good-looking quality amplifier, attractively styled and finished. It glves superb reproduction previously associated whith amplifiers costing far more.
SPECIFICATION:-
R.M.S. power output: 3 warts per channel imo 10 ohms speakers.

INPUT SENSITIVITY: Sultable for medium or high ourput crystal cartridges and tuners. Cross. talk better than 30 Ma at $1 \mathrm{Kc} / \mathrm{c}$
CONTROLS: 4 -position selector switch 12 pos. mono \& 2 pos. stereol dual ganged volume
TONE CONTROL: Treble lift and cuf. Separate on/off switch. A preset balance control.


THE RELIANT Solid State General Purpose Amplifier
SPECIFICATION:-
OUTPUT: 10 watts into a 3 ohms speaker.
INPUTS: (1) for mike ( $10 \mathrm{~m} . \mathrm{v}$.). Input (2) for gram. radio (250 m.v.) individual bass and treble control.
TRANSISTORS: 4 silicone and three germanium.
MAINS INPUT: $220 / 250$ volis.
SIZE: $10 \frac{1}{1}^{\prime \prime} \times 4 \frac{t^{\prime \prime}}{} \times 2 \frac{1}{2}$
PRICE: $6 \frac{1}{4}$ guineas in teak finished case. Less teak case $5 \frac{1}{\frac{1}{2}}$ guineas. $7 / 6 \mathrm{~d}$. p \& p MIKE TO SUIT (CRYSTAL): $12 / 6 d+1 / 6 d$. p \& p.
$8^{\prime \prime} \times 5^{\prime \prime}$ speaker $14 / 6 d+3 / p B_{1} p$. $8^{\prime \prime} \times 5^{\prime \prime}$ speaker $14 / 6 \mathrm{~d}+3 /-\mathrm{p}$ \& $\mathrm{p}^{+}$.


THE VISCOUNT $\qquad$

## Stereo Amplifier

$13 \frac{1}{2}$ GNS.
SPECIFICATION:-
integrated High Fidelity Transistor

OUTPUT: 100 watts per channel into 3 to 4 ohms speakers ( 20 watts monaural).
INPUT: E-position rotary selector switch 13 pos. mono and 3 pos. stereo). P.U.. Tuner. Tape and Tape Rec. Sensitivities: All Inputs 100 mV into 1.8 M ohm.
FREQUENCY RESPONSE: $40 \mathrm{~Hz}-20 \mathrm{KHz}+2 \mathrm{db}$
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External $50 \mathrm{c} / \mathrm{s}$ to $10 \mathrm{kc} / \mathrm{s}$ ．Outpu $0-100 \mathrm{db}$ below 200 mV from 75 ohm source．E85．DITTO but 801／A1／with additional high level output． $\mathbf{P} 8$ ．Both nectors，plugs，and instrucsion manual BROADBENT MICROWAVE SIGNAL GENERATOR TYPE 903. Frequency range $6,800-11,000 \mathrm{mc} / \mathrm{s}$ cis and $x$ multiplyer delay $3-300$ U／sec．Wideh 05 to $10 \mathrm{U} / \mathrm{sec}$ ．Input for external syncronisation and modu－ lation．Ourput delayed and undelayed syncronised directly calibrated attenu ator．685．Carraige 30／
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As above but frequency $3,830-11,050$ $\mathrm{mc} / \mathrm{s}$ ，counter read out，pulse delay XI ， $\times 10$ and $\times 100$ at 2.20 microsecs．Pulse
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2163

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is required to join the Group responsible for the development ans operation of the Synchrotron. He should be prepared to undertake development work on various projects and carry out this work with a high degree of personal responsibility. He should also be prepared to spend some of his time (at present $50 \%$ ) as a member of the operating crew on a three shift basis.
Applicants should be at least 26 years of age and must have served a recognised engineering apprenticeship or have had comparable training. They must also possess an O.N.C. or equivalent in Electrical Engineering or Applied Physics and have experience in electro-mechanical and electrical work. Some electronic and high vacuum work would be an advantage.
Starting salary will be assessed according to age, qualifications and experience on the scale $£ 1,347-£ 1,565$ (this scale is under review). A shift allowance (at present $14 \frac{1}{2} \%$ of salary) is paid in addition to salary.
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The current expansion programme of our Flight Simulator Division entails the consolidation of a newly-formed Standards policy. We need a

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[^4]
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The ability to plan and negotiate high grade networks for speech, telemetry and data transmission is required together with a thorough knowledge of the associated G.P.O. terminal equipment.

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## BATH EDOCATIONAL TELEVISION SERVICE OPERATIONAL AND MAINTENANCE ENGINEER

Applications are invited from suitably qualified and experienced candidates for a post as Operational and Maintenance Engineer with the B.E.T.S. Duties will include the operation, testing and maintenance of a comprehensive range of video and audio equipment at the Studio centre in Bath.
Further information and forms of application can be obtained from: The Secretary, Bath Educational Television Service, Northgate House, Bath, BAI 5AL.

2171

## RADIO TECHNICIANS

Vacancies to be filled by October, 1969
A number of suitably qualified candidates are required for unestablished posts, leading to permanent and pensionable employment (in Cheltenham and other parts of the UK, including London). There are also opportunities for service abroad.

Applicants must be 19 or over and be familiar with the use of Test Gear, and have familiar with the use of Test Gear, and have
had practical Radio/Electronic workshop experience. Preference will be given to such candidates who can also offer "O" Level GCE passes in English Language, Marhs and/or Physics, or hold the City and Guilds Telecommunications Technician Intermediate Certificate or equivalent technical qualificacions. A knowledge of electro-mechanical equipment will be an advantage.
Pay according to age, e.g. at 19- $\mathbf{2 8 6 9}$; at 25-fl, 130 (highest age pay on entry) rising by four annual incremenes to $\{1,304$.

Prospects of promorion to grades in salary range $\{1,217-\{2,038$. There are a few posts range $\{1,217-£ 2,038$. Th
carrying higher salaries.
Annual Leave allowance of 3 weeks 3 days rising to 4 weeks 2 days. Normal Civil Service sick leave regulations apply.

Application forms available from:
Recruitment Officer (RT 3),
Government Communications Headquarters.
Oakley, Priors Road.
CHELTENHAM, Glos, GL52 5 AJ.

## TEST ENGINEERS

Engineers are required for final test of solid state $R / F$ prototype and pre-production equipment operating at U.H.F. and microwave frequencies.

These positions would be ideally suitable to ex-service radio/radar personnel, television service engineers, etc., with experience of transistorised circuitry.

- The Company offers first-class holiday. sick payment and welfare facilities. including an excellent group pension and insurance scheme. The two modern establishments are located at Bushey and Hemel Hempstead. Herts., within easy access of the M. 1 .


Apply in writing,
quoting reference WWRM2 to:
Personnel Officer,
Ether Engineering Ltd.,
Park Avenue, Bushey, Herts.


Engine ving [fd]

## PRODUCTION TEST ENGINEERING

Due to our successful Research and Design work many exciting new projects are entering a production phase and we require Engineers and Technicians to participate in this work.
Minimum qualifications required are a basic understanding of Transistor circuitry enabling testing to specification to be carried out on our Data Processing and Servo Control Systems, etc.

Electrical Engineering Certificates an advantage, but not essential if experience in a similar activity can be offered.

## Apply:

Personnel Officer
RECORDING DESIGNS LTD.
Blackwater Station Estate
Blackwater, Camberley, Surrey
Telephone Camberley 24622

## SENIOR FIELD ENGINEER

Required for Computer and Data Processing Peripheral units, to operate from London, there are excellent prospects for a man with good electro-mechanical practice who can show initiative and can write clear factual reports. A car and operating expenses and good salary are offered to the right man.

## DRAUGHTSMANCHECKER

Required for electro-mechanical work. Promotion prospects are good for a man with proved ability and initiative.

## AUDIO EQUIPMENT DEVELOPMENT ENGINEER

Required for work connected with Public Address, sound recording and reproducing and Cinema Projection Equipment. Applicants must have a good experience of Technical Audio work.

> Apply in writing to
> The Chief Engineer, Westrex Co. Ltd.,

152, Coles Green Road, London, N.W.2.
or telephone
01-4525401 Extension 12.


A DIVISION OF LITTON INDUSTRIES

## POST <br>  SERVICES

Our POST DESIGN SERVICES SECTION at Wandsworth has a vacancy for a man with a basic theoretical and practical knowledge of radio. He would also need the ability to prepare written technical leaflets from laboratory information and a knowledge of M.O.T. Post Design procedure would be an advantage.
Applications in writing please to:-
The Personnel Officer, REDIFON LIMITED.
Broomhill Road, Wandsworth, London, S.W.18.
REDIFON:
A Member Company of the Rediffusion Organisation

# Radiomobile CAR RADIO DeSGIGERS 

## Do you:-

Have a Degree or HND/HNC in electronics? Have experience in radio receiver design, not necessarily car radio?
Like the idea of working with a dynamic design team and seeing your project through to production?
Have ideas for using microcircuits?
IF YOUR ANSWER TO MOST OF THESE QUESTIONS IS YES

WHY NOT TELEPHONE ME, Peter Wilding
(Engineering Manager) on 01-452 0171-
(Reverse charges of course).
On any weekday
or send me your career details-
We need people like you-and will pay well for the right men-or women


COMMISSIONING ENGINEERS OR TECHNICIANS
Experienced in servicing or testing digital equipment. Training on Equipments given where necessary.

## PROTOTYPE WIREMEN

Experienced on electronic rack wiring, but desiring more varied work.

These vacancies are in a team commissioning an advanced system of machine tools on line to a computer. They involve installation, test, evaluation and maintainance of machine tools and automatic conveyors.

Please write for Company brochure and application form to Mr. K. Oxenham, Head Office Personnel Officer,

## TECHNICAL AUTHORS

A Technical Publications Contractor has vacancies in their Home Counties offices and on site for personnel to be engaged in the preparation of manuals for a wide range of electronic and alfied equipment to Ministry and Commercial require ments. Appllcation arelevant experience. Box No 5052.

## ELECTRONIC SERVICE ENGINEERS

required by OLYMPIA BUSINESS MACHINES for their London workshops to work on a range of electronic calculators. A good salary and working conditions are offered.

Also required: Young Men with strong interest in electronics but without complete experience will be trained. Courses are available through this company. Day release for selected trainees. Please apply in writing to:
D. H. Smith,

Olympia Business Machines
Company Ltd.
299a Edgware Road, London, W. 2

## TECHNICIAN

Applications are invited for the post of technician to maintain computer systems, to construct computer hardware, and to assist in the general running of a small electronics laboratory.

Suitable qualifications are experience in electronic equipment, construction and maintenance of electro-mechanical devices and an interest in the subject generally.

Salary range £847-£1,400. Superannuation scheme.
Apply in first instance by letter, stating briefly personal details and relevant experience, to Mr. J. A. Payton, Centre for Computing and Automation, Imperial College, London, S.W.7.

2201

## CHIEF SOUND RECORDIST

required by the CENTRAL OFFICE OF INFORMATION for its Radio Division which is responsible for the production and fast transmission of radio programmes on magnetic tape and disc or by circuit for use by broadcasting stations overseas. Programmes vary from brief interviews to half an hour in length and total output is about 50 hours per week, in some 30 languages.
The Chief Sound Recordist will have control of a staff of maintenance engineers and sound recordists and will be responsible for all sound recording operations. His duties will include the management of recording studios and copying channels, and the servicing of static and portable equipment. He will supervise recording by outside contractors and liaise closely with the GPO about and line facilities to overseas territories. He will be responsible for the planning, design and installation of such new facilities as may be required by the development of the service and by technical advances in the medium. Salary $£ 1,850-£ 2,355$ per annum.
Please send postcard for application form to Manager (PE/A/185/EW). Department of Employment and Productivity, Professional and Executive Register, Atlantic House, Farringdon Street, London, E.C.4. Closing date for completed
2207 application forms 4 June 1969

## Tradesmen and Technicians

Applications are invited from competent men who are attracted by the opportunity to work overseas for a year or two (with generous leave and free air passages), earn an attractive salary and qualify for tax concessions.

Our immediate vacancies are as follows :-

FITTERS INSTRUMENT
(Ref. FTI)

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WIRELESS
(AIR)
(Ref. FTW/A)

FITTERS RADAR (AIR)
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FITTERS
RADIO/RADAR
(Ref. FTR/R)

FITTERS
ELECTRICAL
(GROUND)
(Ref. FTE/G)

LABORATORY TECHNICIAN
(Ref. LTN)

Suitable applicants would be ex-RAF or civilian trained fitters with Flight Instrumentation experience in 1st and 2nd line servicing associated with Lightning and Jet Provost aircraft

Suitable applicants would be ex-RAF or RN trained fitters with 1st and 2nd line servicing experience of Airborne communication equipment, P7R 175, ARC 52, TACAN and IFF.MK 10.

Suitable applicants would be ex-RAF or RN trained fitters with 1st and 2nd line servicing experience of Airborne Radar equipment, AI 23B, TACAN and IFF.MK 10.

Suitable applicants would be ex-RAF or RN trained fitters who have received a formal course on TACAN, IFF, VHF/UHF and PTR 175 and are experienced at 1st and 2nd line servicing level.

Suitable applicants would be ex-RAF or RN trained fitters with experience of servicing and maintaining Airfield ground servicing vehicles and equipment.

Suitable applicants would be ex-Service or civilian trained technicians who are familiar with the use of electronic, radio and radar test equipment. They would be required to assist Electronic Instructors in the laboratory.

Please apply, quoting the appropriate reference, to :

THE PERSONNEL MANAGER AIRWORK (OVERSEAS) LIMITED BURLINGTON ARCADE BOURNEMOUTH . HANTS

## ELECTRONIC ENGINEERS

Service Engineers required for Offices, throughout the United Kingdom, of well-known Company manufacturing Electronic Desk Calculating Machines. Applicants should possess a sound knowledge of basic Electronics with experience in Electronics, Radar, Radio and T.V. or similar field. Position is permanent and pensionable. Comprehensive training on full pay will be given to successful applicants. Please send full details of experience to the Service Manager, Sumlock Comptometer Ltd., 102/108 Clerkenwell Road, London, E.C.1.

## ITT Marine

## MARINE RADIO ENGINEER

Due to our expanding business in the South Wales area, we urgently require an additional engineer to work from our Cardiff Depot on service and installation of marine radio and associated equipment.

Candidates must be ex-Merchant Navy Radio Officers with a minimum of three years"sea-service and preferably previous experience of installation and maintenance of equipment.

Apply to Head Office Personnel Manager, giving brief details of qualifications and experience.
International Marine Radio Co. Ltd., 1 Peall Road, Croydon, Surrey, CR9 3AX.

## NORWICH CITY COLLEGE DEPARTMENT OF

ELECTRICAL ENGINEERING

The Department of Electrical Engineering of the Norwich City College offers students who have studied Physics and Mathematics at Advanced level in the G.C.E. and passed in one subject, a modern sandwich course for the Higher National Diploma in Electrical and Electronic Engineering. Subjects studied include Computation, Statistics, Economics and Law, Electronics, Control, Telecommunications, Power and Machines. Well balanced and interesting industrial training with pay will be arranged as required. The course is approved for major grant awards by Local Authorities.

Accommodation will be arranged by the College if desired.

Enquiries about the course starting in September 1969 should be made to:
E. Jones, B.Sc., Ph.D., C.Eng., M.I.E.E. Head of Department of Electrical Engineering,
Norwich City College,
Ipswich Road, Norwich, Norfolk. NOR 670.

## Computer Engineering

NCR requires additional ELECTRONIC, ELECTRO-MECHANICAL ENGINEERS and TECHNICIANS to maintain medium to large scale digital computing systems in London and provincial towns.
Training courses will be arranged for successful applicants, 21 years of age and over, who have a good technical background to ONC/HNC level, City and Guilds or radio/radar experience in the Forces.
Starting salary will be in the range of £900/ $£ 1150$ per annum, plus bonus. Shift allowances are payable, after training, where applicable. Opportunities also exist for Trainees, not less than 19 years of age, with a good standard of education, an aptitude towards and an interest in, mechanics, electronics and computers.
Excellent holiday, pension and sick pay arrangements. Please write for Application Form to Assistant Personnel Officer NCR, 1,000 North Circular Road, London, N.W.2, quoting publication and month of issue.

## Electronic Technicians

Ampex Quality Control Department now has vacancies for electronics technicians. Successful applicants will be responsible for fault finding and testing a complete range of sophisticated magnetic recording equipment.

Experience gained in the electronic industry or radio or television servicing would be an advantage or a qualification of O.N.C. standard.

Attractive salary based on qualifications and experience will be paid and the company operates an excellent range of Life Assurance and Pension Schemes, etc.

Please write or telephone for application form to the Personnel Officer, Ampex Electronics Limited, Acre Road, Reading, (Tel.: Reading 84411).

AMPEX

## MAINTENANCE ENGINEER

(Salary up to $£ 1600$ )

The rapidly expanding Echo and Post Limited, a member of the progressive Thomson Organisation, has a vacancy for an engineer to maintain the equipment in the Teleprinter and Type Setting departments.

Applicants should preferably have served an apprenticeship with a light engineering company, and have had experience in the maintenance of Teleprinters and Printer equipment. A working knowledge of electronics would be an advantage.

The many attractive features of employment include: $37 \frac{1}{2}$ hour week. 3 week holiday, Contributory Pension Scheme, subsidised canteen and pleasant working contions in the most modern newspaper office in Britain.

Apply in writing giving brief details of age and experience to:
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Echo and Post Ltd,

## Mark Road,

Hemel Hempstead,

## Herts,

or
Telephone Hemel Hempstead 2211 extension 340

# Looking for a change? <br> TECHNICAL AUTHORS 

We are one of the world's leading designiers and manufacturers of flight simulators. We are looking for authors with a sound knowledge of electronics and who preferably have some knowledge of-basic digital computer operation. They will produce operating and maintenance manuals. They must be able to write literature in a clear and concise style. Formal qualifications are desirable but not essential. Our product is a highly sophisticated one and incorporates both analogue and digital computers. Simulation is based on novel applications of known techniques. Authors have ample opportunity to employ a measure of creative expression. This work is definitely not of a monotonous. routine nature.
Conditions of employment are good and include a contributory pension scheme coupled with free life assurance. There is a paid sick scheme and other benefits.
Please apply in writing, giving brief details of career quoting ref. WW/469.
Apply to: H. C. Hall,
Personnel Manager, REDIFON LIMITED, FLIGHT SIMULATOR DIVISION, Gatwick Road, Crawley, Sussex. Telephone: Crawley 28811. REDIFON:
A Member Company of the Rediffusion Organisation

## GOVERNMENT OIF ZAMBIA

# Department of Civil Aviation requires <br> <br> RADIO ENGINEERS 

 <br> <br> RADIO ENGINEERS}

Salary in scale up to $\mathbf{E 2 7 8 2}$. Tour of 36 months offered.
Generous leave on full salary.
25\% End-of-Tour Gratuity.

Commencing salary according to experience in scale $K$ wacha 2736 ( £Stg.1596) rising to Kwacha 3216 ( (Stg.1876) a year, plus an inducement Nllowance of ESig. 568 - LSig. 615 . A Direct Payment of $£ \operatorname{Stg} .268$ - CStg. 291 is also payable direct to an officer's U.K. Jank account. Both gratuity and direct payment are normally TAN FREE. Free passages. Quarters at low rental. Cliildren's education allowances. Gencrous leave on full salary or terminal payment in lieu. Pension scheme available under certain circumstances.

Candidates must be under 55 years of age and should possess 8 years relevant experience following:-
i) an apprenticeship of 5 years, or
ii) possession of a Service ryade Certificate, or
iii) possession of an A.W.O.A. or I.C.A.O. certificate of competency or its equivalent.
In addition, candidates must have a sound knowledge of the theoretical principles of and experience in the maintenance of at least FOUR of the following groups of Communications, CM, Navigational and Surveillance Systems.

1. Medium powered H.F. Transmitters and associated Receivers;
Frequency Shift Keying, S.S.B. and D.S.B. Equipment,

Medium Frequency Non-Directional Radio Beacons.
2. Low and High powered V.H.F., I.M. Equipment.
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4. Instrument Landing System.
5. Radar X and S Band Terminal and P.P.i Talk Down Rquipment.
6. Audio and Remote Control Equipment; Public Address Equiprnent; Airport Magnetic Tape Recorders; Inter Office Communication; Underground Control Cables; Impulse and D.C. Switching Systems.
7. Teleprinter Telegraphy (torn tape) and associated Page Printers; Pape Recorders (autoheads); Printing Reperforators and Associated Switching Equipment.
Duties include the maintenance, overhaul and installation of ground terminal radio communication equipment and navigational aids at Airports and Flight Information Centre.

Possession of a valid driving licence will be an advantage.
Apply to CROWN AGENTS, M. Division, 4 Millbank, London, S.W.I., for application form and further particulars, stating name, age, brief details of qualifications and experience and quoting reference $M_{2} Z / 690315 / \mathrm{W}$ F

## OXLEY ${ }^{\circ} \oplus$ TEChNICIAN

Hrogressive Electronic Component Manufacturers, situated in the Lake District, require a Techniciah to work in close conjunction with Electronics Engineers and Physicists, in the development, and subsequent production, of precision glass components.

The successful applicant should be capable of working on his own initiative. A knowledge of Laboratory workshop practise and basic physics would be advantageous.
Assistance given in finding local accommodation.
Applications, stating age, experience etc., to be sent to:
The Personnel Manager,
Oxley Developments Company Limited,
Priory Park, Ulverston, North Lancashire.

A CAREER IN ELECTRONICS WITH THE AIR FORCE DEPARTMENT<br>VaCANCIES AT RAF SEALAND, NEAR CHESTER<br>RAF HENLDW, BEDFDROSHIRE<br>AND RAF CARLISLE, CUMBERLAND<br>INTERESTING AND VITAL WORK ON RAF RADAR AND RADIO EQUIPMENT FOR:<br>RADIO TECHNICIANS<br>MINIMUM QUALIFICATION, 3 YEARS' TRAINING AND PRACTICAL EXPERIENCE IN RADIO ENGINEERING.<br>STARTING PAY ACCORDING TO AGE. UP TO $£ 1,130$ p.a. (AT AGE 25) RISING TO £1,304 p.a. WITH PROSPECTS OF PROMOTION.<br>5-DAY WEEK-GOOD HOLIDAYS—HELP WITH FURTHER STUDIES—OPPORTUNITIES FOR PENSIONABLE EMPLOYMENT.<br>WRITE FOR FURTHER DETAILS TO:<br>MINISTRY OF DEFENCE CE3h(AIR),<br>SENTINEL HOUSE, SOUTHAMPTON ROW, LONDON W.C. 1 APPLICANTS MUST BE UK RESIDENTS 2208

## REDIFFUSION

## COLOUR TELEVISION FAULTFINDERS \& TESTERS

We have a number of vacancies in our Production Test Departments for experienced faultfinders and testers.
Knowledge of transistor circuitry and experience with Colour Receivers together with R.T.E.B. Final Certificate or equivalent qualifications required.
These will be staff appointments with all the expected benefits.
Applications to:

Works Manager,<br>Rediffusion Vision Service Ltd., Fullers Way South,<br>Chessington, Surrey (near Ace of Spades).<br>Phone: 0l-397 54II

A FULL-TIME technical experienced salesman re A quired for retall sales: write giving detalls of age, Henry's Radio, Ltd., 303 Edgware Rd., London, W.2

FLECTRICAL \& GENERAL DEVELOPMENT LIMITED, of Wimbledon, S.W.19, require engineers for testing Public Address Equipment. Phone
(01) 9470222 .

EXPERIENCED ENGINEER required for repair and E caibration of electronlc test equipment.-Apply A. J. Whittemore (Aeradio) Lid... Blestin Hill Aero-
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UNIVERSITY OF SHEFFIELD. CHIEF ELEC TRONICS TECHNICIAN required in Departmen of Chemlstry to take charge of electronics workshop concerned with development and construction of new electronic equipment for use in research and teachin range of elect:onic instruments and equipment. Considerabie experience necessary. Paper qualfications in appropriate fleld desirable. Salary £ 1,294-£ 1,475 per annin. Suparanniation. Write to the Bursar (Ref
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Finding and Testing of Moblle VHF and UHF Mobll Equipment. Exce:lent Opportunities for promotion du to Expansion Programme. Please apply to Personne Manager, Pye Telecommunications Ltd., Cambridge Works. Hai3 Road, Cambridge. Tel. Cambridge 51351 Extn. 327

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BUILD IT in a DEWBOX quallty plastics cabinet. $\mathrm{Bing}^{2}$ In. $x{ }^{2 \frac{1}{2}} \ln$. $x$ any length. D.E.W. Ltd. (W), Write now-Right now.

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THE IDEAL PANEL Mounting Meter Mowement for S.D Sensitive Test Meter, etc. 200 Micro Amp only 39/6. P. $\& 2$ P. Free. Limited number only. Walton's Wireless Stores. 55A Worcester Street. Wolverhampton,
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## STAVELEY-SMITH CONTROLS LIMITED SERVICE ENGINEERS

Vacancies exist for both Marine and Industrial Electronic Service Engineers in the London area.

The Marine Engineer will be required to service Radio, Radar, and Navigational Aids on shipping in the docks and other locations in the South East.

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Applicants must be either ex-seagoing personnel and/or experienced Industrial Service Engineers, resident near London preferably Essex for the the Marine Engineer and West or North for the Industrial.

All applicants must hold clean driving licence and be willing to travel.

All positions are Staff, with contributory Superannuation.

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Excellent working conditions in modern factory and laboratory.

APPLY: J. H. R. Manners, Chief Engineer, H.C.D. Research Limited,



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This private College provides efficient theoretical and practical training in the above subiects. One-year day courses are available for beginners and shortened
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Write for details to: The Secretary, London Electronics College, 20 Penywern Road, Earls Court, London, S.W.5. Tel.: 01-373 8721 .

## BOURNEMOUTH COLLEGE OF TECHNOLOGY FULL-TIME COURSE

university of London external honours degree in electrical engineering
G.C.E. 'A' level entry or O.N.C.(Eng.) or O.N.D.(Eng.) entry

Next session's course commences September, 1969. Details from The Principal, Room E7, College of Technology, Lansdowne, Bournemouth BH1 3JJ. Tel: 20844 APPROVED LODGINGS ARRANGED early application is desirable

## NEWCASTLE UPON TMNE POLYTECHNIC (Designate)

## RUTHERFORD COLLEGE OF TECHNOLOGY

B.Sc. ELECTRICAL AND ELECTRONIC ENGINEERING (Honours and Ordinary)
B.Sc. PHYSICAL ELECTRONICS (Honours and Ordinary) M.Sc. ADVANCED EXPERIMENTAL PHYSICS

Further details of these and other courses and of residential accommodation available, may be obtained from Administrative Officer, Rutherford College of Technology, Ellison Place, Newcastle upon Tyne, NEI 8ST quoting WW 693

## TRANSISTOR ELECTRONIC ENGINEERS

NEWMARKET are expanding their applications laboratory which deals with device evaluation, customer circuit problems, micro circuit design, etc.

There are now, interesting openings for qualified and unqualified engineers who have some experience in transistors.

WRITE or TELEPHONE, in confidence, and give Mr. Towers, Marketing Manager, details of your age, qualifications and experience.

## AT NEWMARKET TRANSISTORS LTD. EXNING ROAD, NEWMARKET, SUFFOLK. TEL. NEWMARKET 3381 or

On Stand E201 at the R.E.C.M.F. Exhibition, Olympia.

CLOSED CIRCUIT TELEVISION EQUIPMENT, We Chave a quantity of industrial and broadcast television equipment for dlsposal at reduced price. Write tor list.-J. D. Jackson Electronics, Eggleston Works,
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TNTEGRATED CIRCUITS at lowest rate GT Type ach including data. P. \& P. C.W.O. JEF ELEC. TRONICS, 12 York Drive, Grappenhall, Warrington Lancs. Mall Order only.
L ARGE SCREEN colour T.V. projectors, Cintel Model condition but require assembly Spare CRT inputs. Good condition but reauire assembly, Spare CRT's. Offers as

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Quarter of
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UFO DETECTOR CIRCUITS, data, 10s. (refundable) Paraphysical Laboratory (UFO Observatory),
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[^1]:    The hp 8005 produces wave forms single-handedly. It is both function generator and pulse generator. And, with appropriate gating signals, a word generator as well. We call it a multi-function pulse generator, the idea being that a single, sensibly priced instrument should be able to do the job of a whole battery of specialized pulse generators
    Hence the wide ranges of repetition ranges, pulse widths and pulse delays-all combined with DC offset for both positive and negative output channels (they are available simultaneous(y). In the double pulse mode. you can even simulate a 20 MHz repetition rate. Variable rise and fall times extend from 10 ns to 2 s . Add the passibility of combining both output channels in the output terminal while DC offset remains available. Add simultaneous and seperate gating, asynchronous as well as synchronous.
    And the result? Three generators-pulse.
    function and ward-in one
    hp 8005A: f 417 excluding duty WW--064 FOR FURTHER DETAIL.S

[^2]:    Mullard Limited
    Consumer Electronics Division
    Mullard House Torrington Place London WC1

[^3]:    *W'est Ham College of Technology, London, E. 15.

[^4]:    A Member Company of the Rediffusion Organisation

[^5]:    TECHNIOAL TRAINING
    B guaranteed diploma and exam. home-study courses in radio. TV. servicing and maintenance. R.T.E.B., City \& Guilids, etc., highly informative 120 -page Gulde-iree,-Chambers College (Dept. 837 K ), $\quad 148$
    Holborn, London, E.C.1.

